

FIG. 1

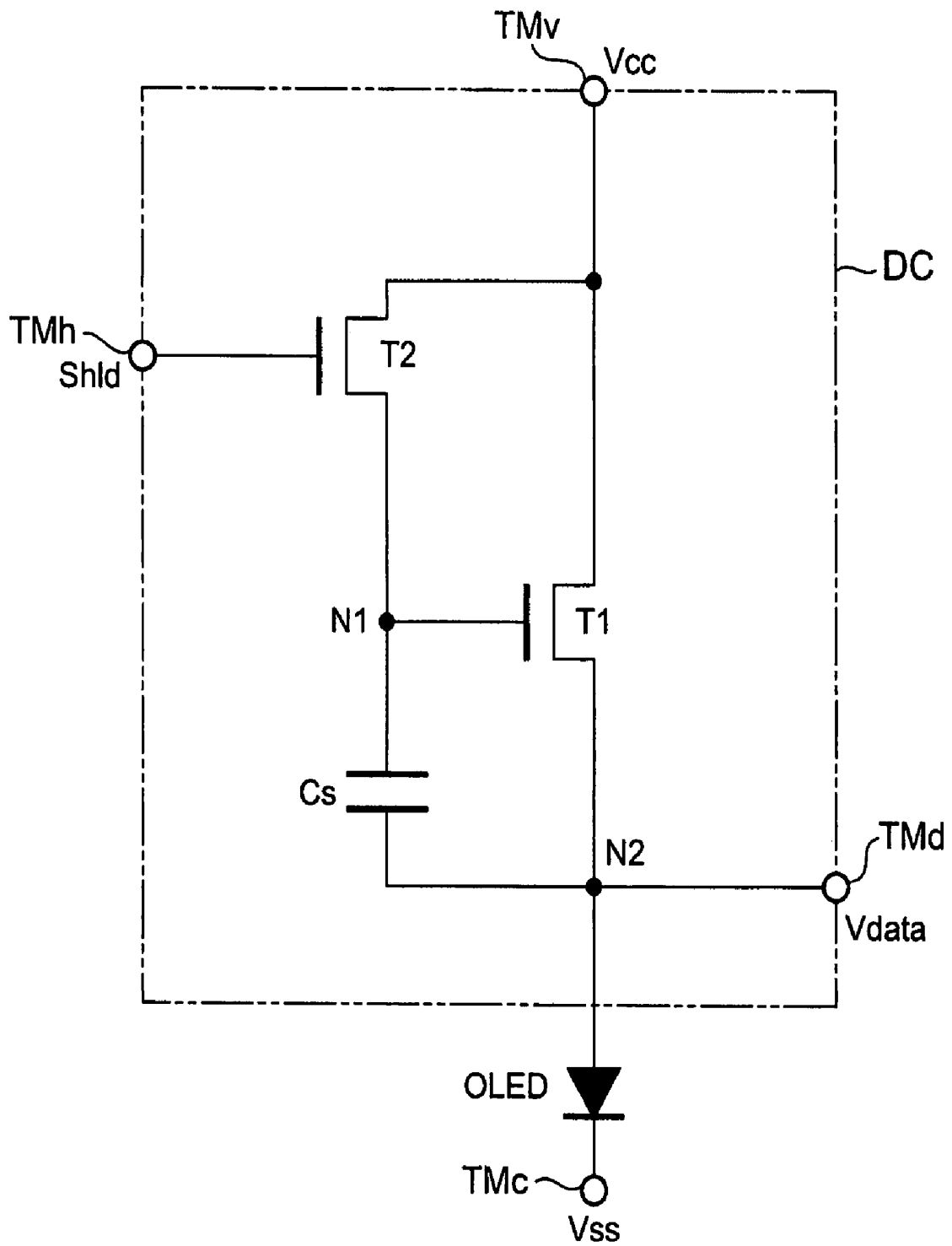


FIG. 2

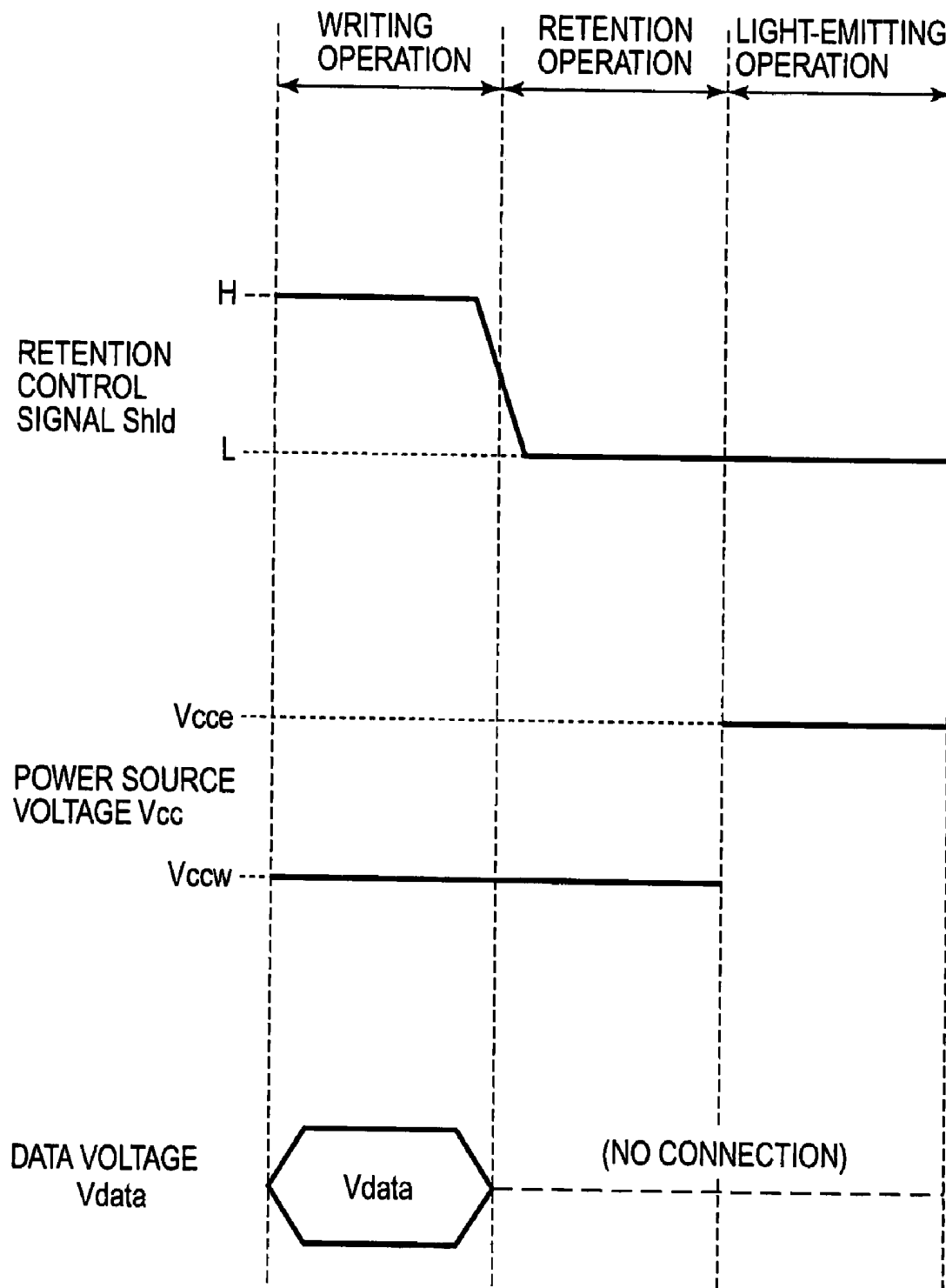


FIG. 3A

DURING WRITING OPERATION

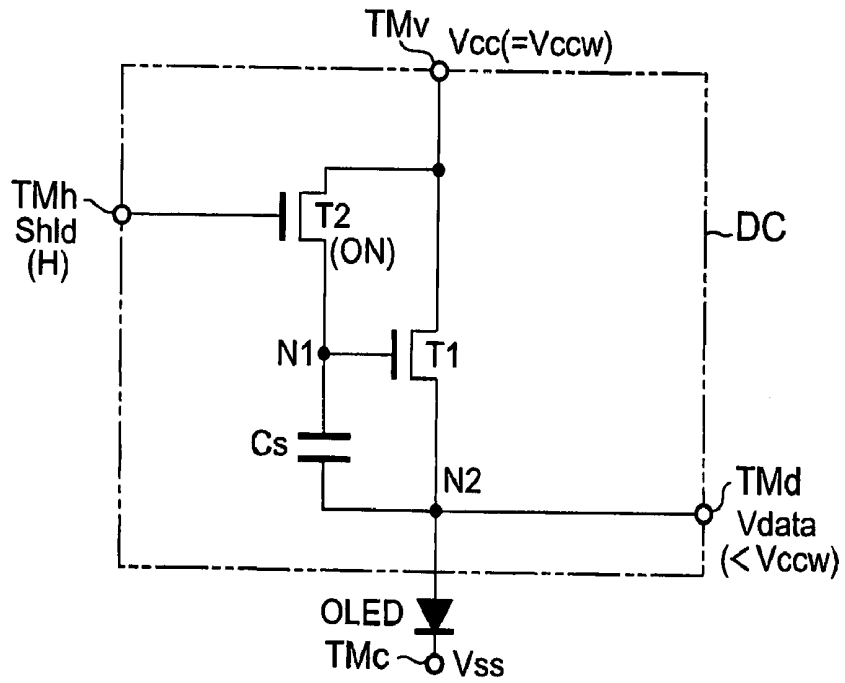


FIG. 3B

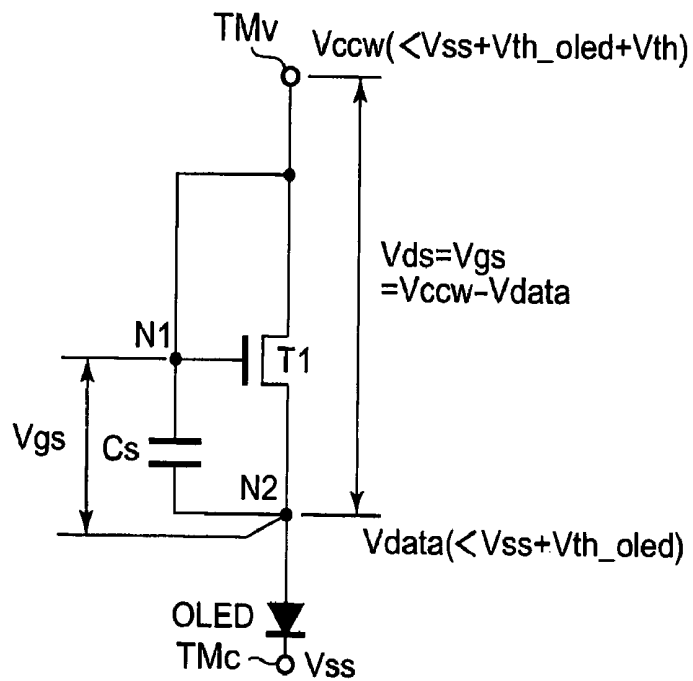


FIG. 4A

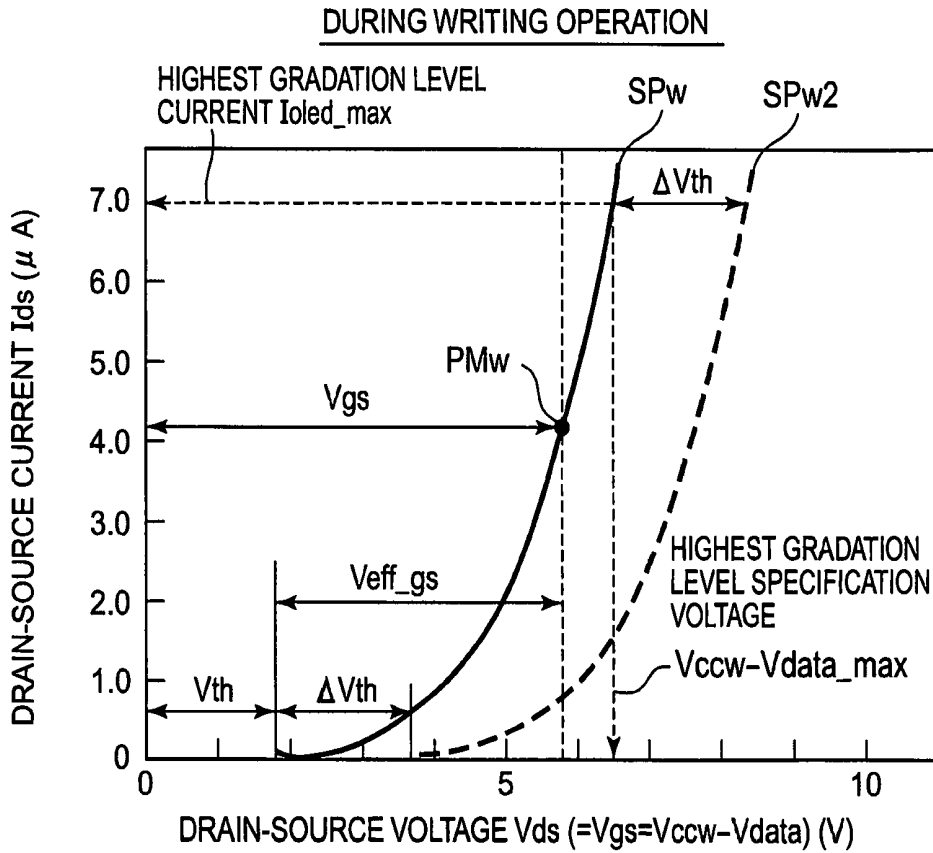


FIG. 4B

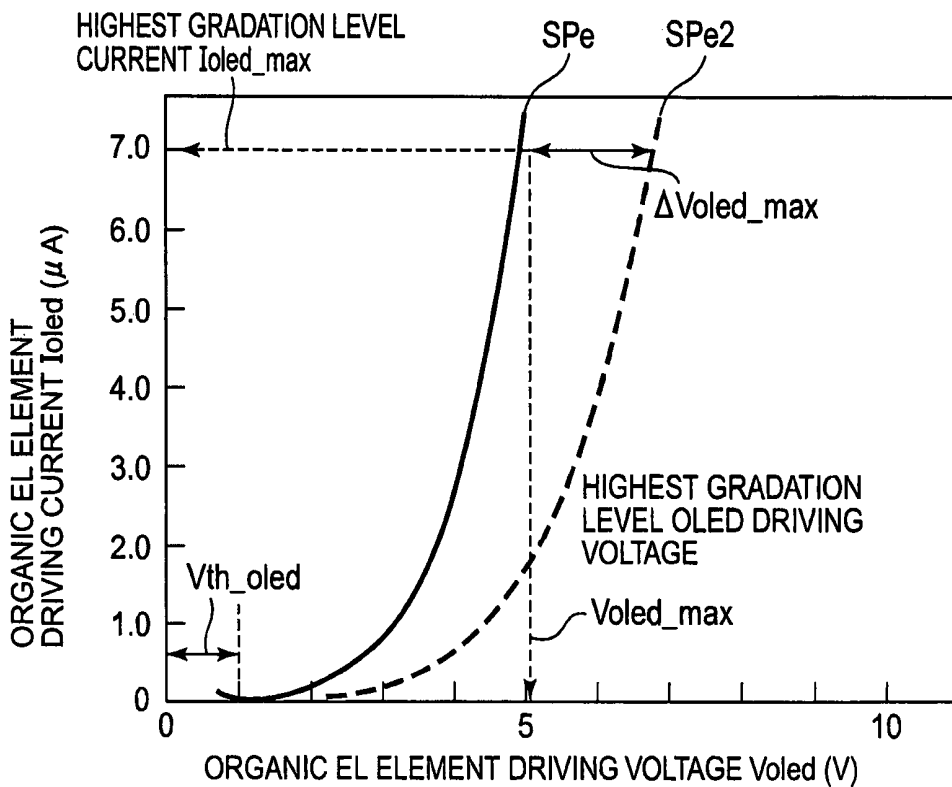


FIG. 5A

DURING RETENTION OPERATION

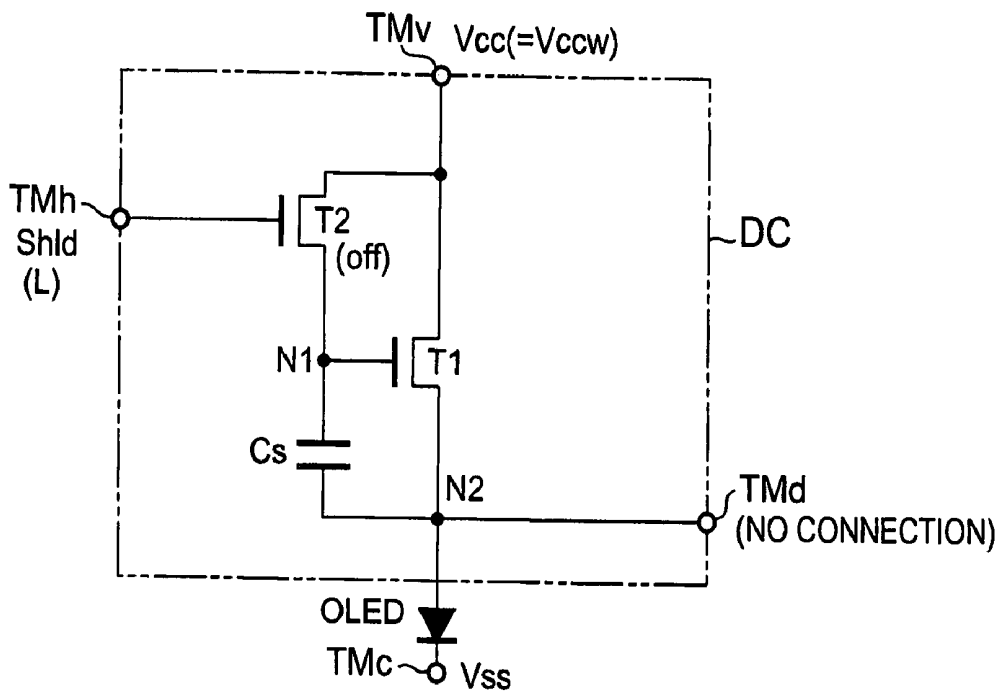


FIG. 5B

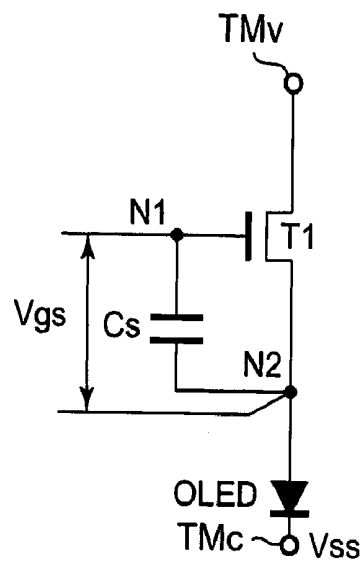


FIG. 6

DURING RETENTION OPERATION

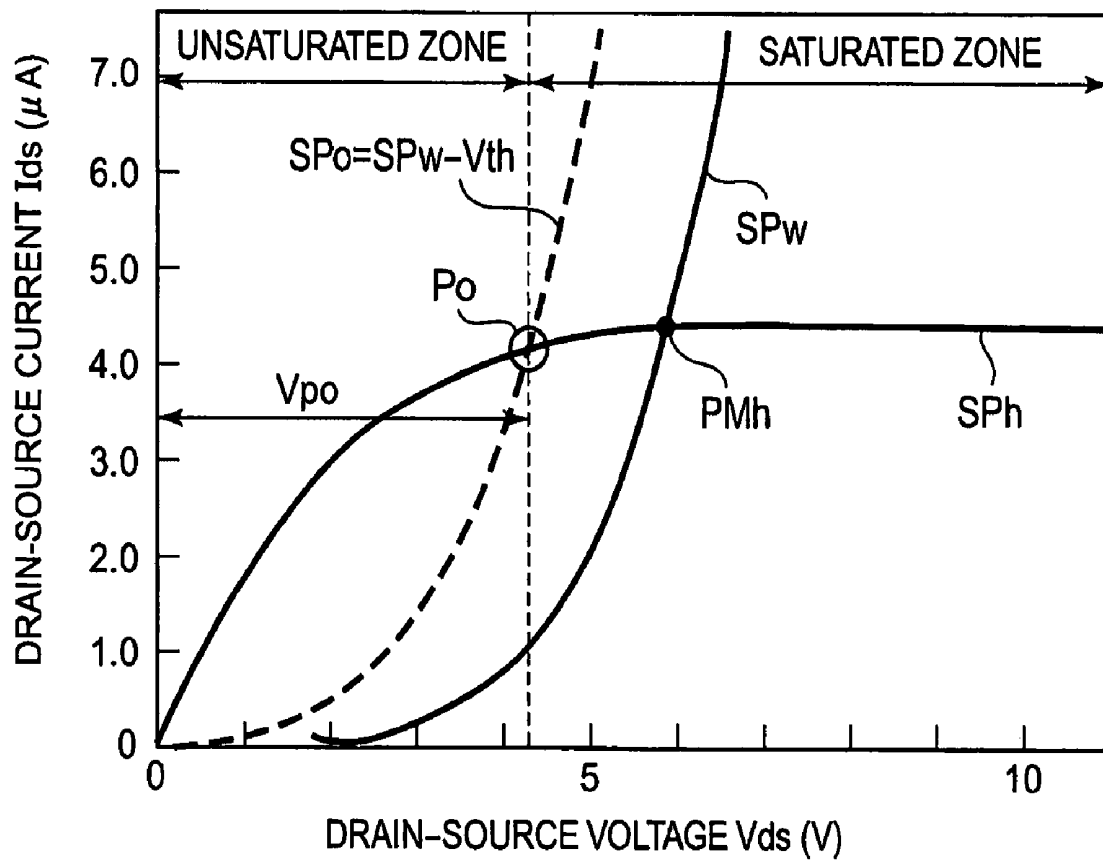


FIG. 7A

DURING LIGHT-EMITTING OPERATION

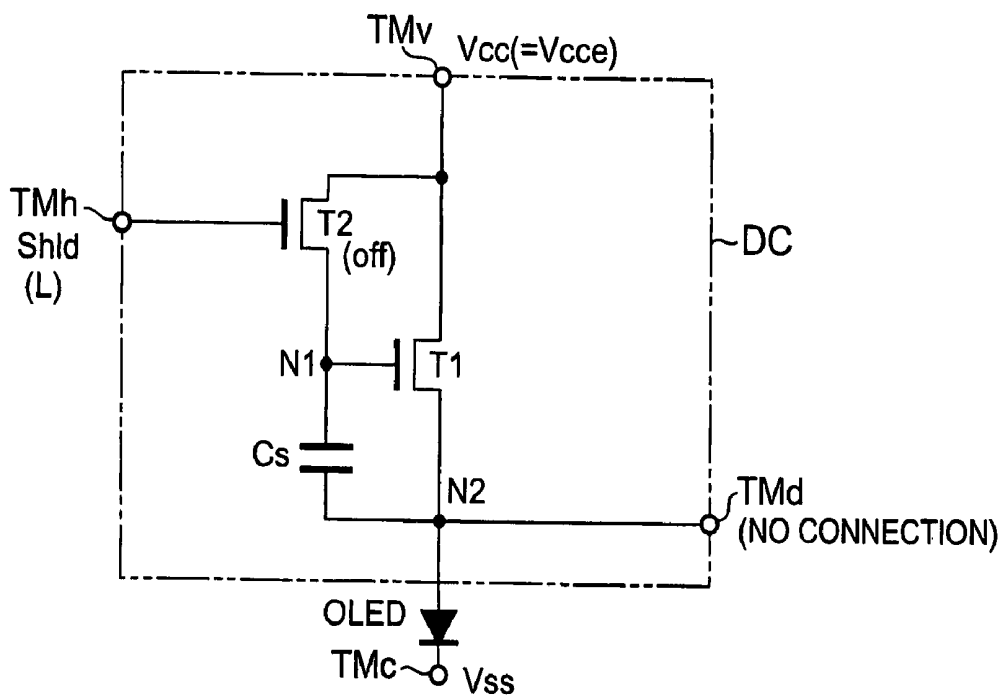


FIG. 7B

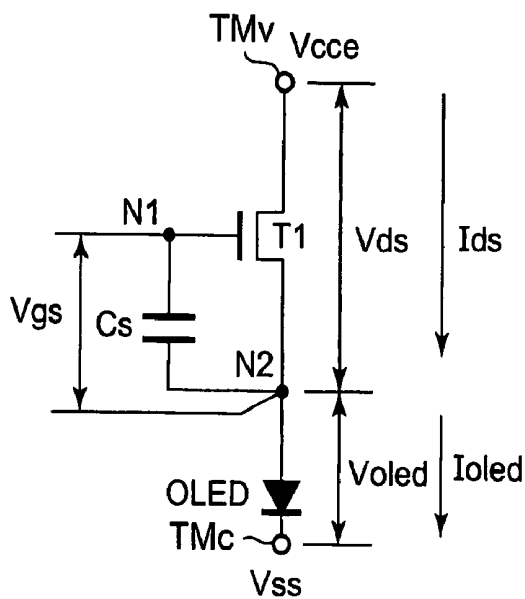


FIG. 8A

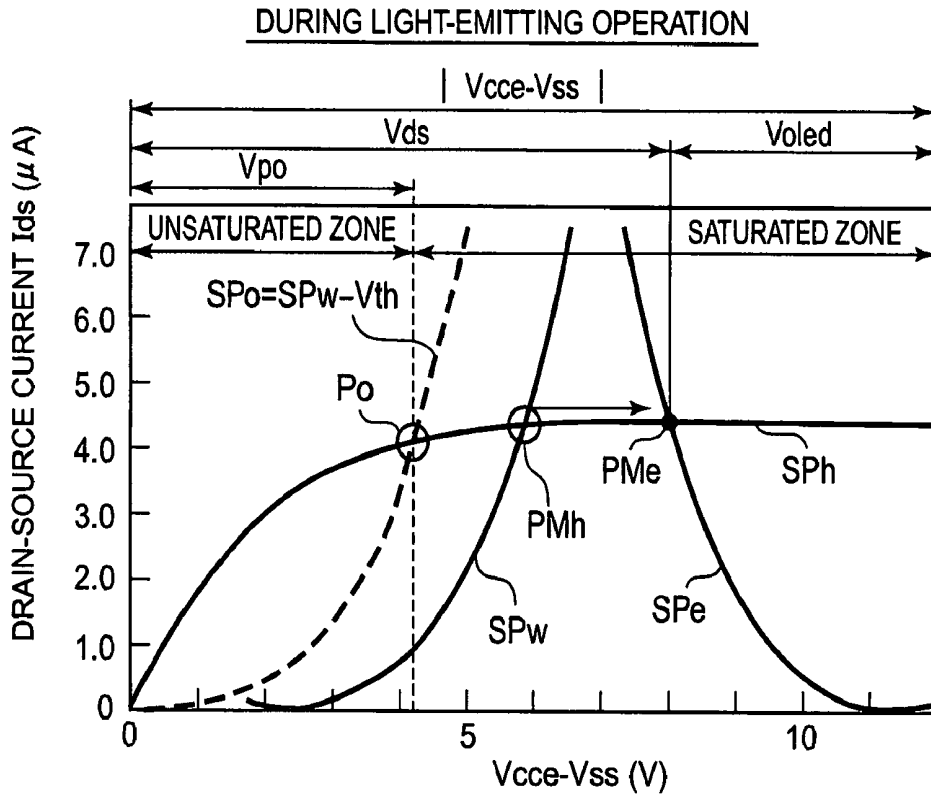


FIG. 8B

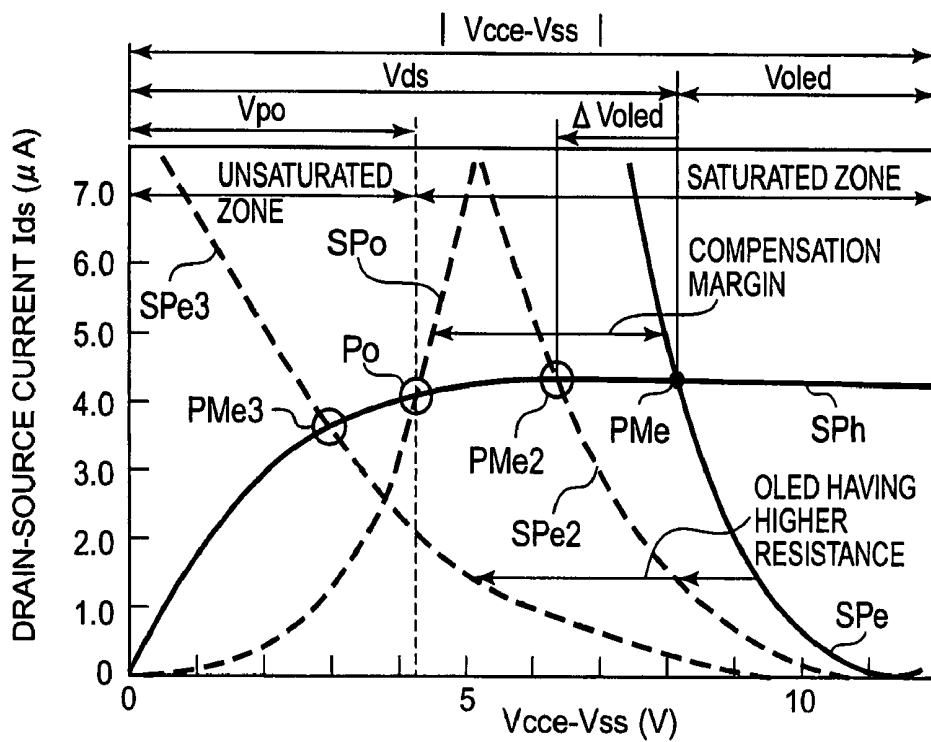


FIG. 9

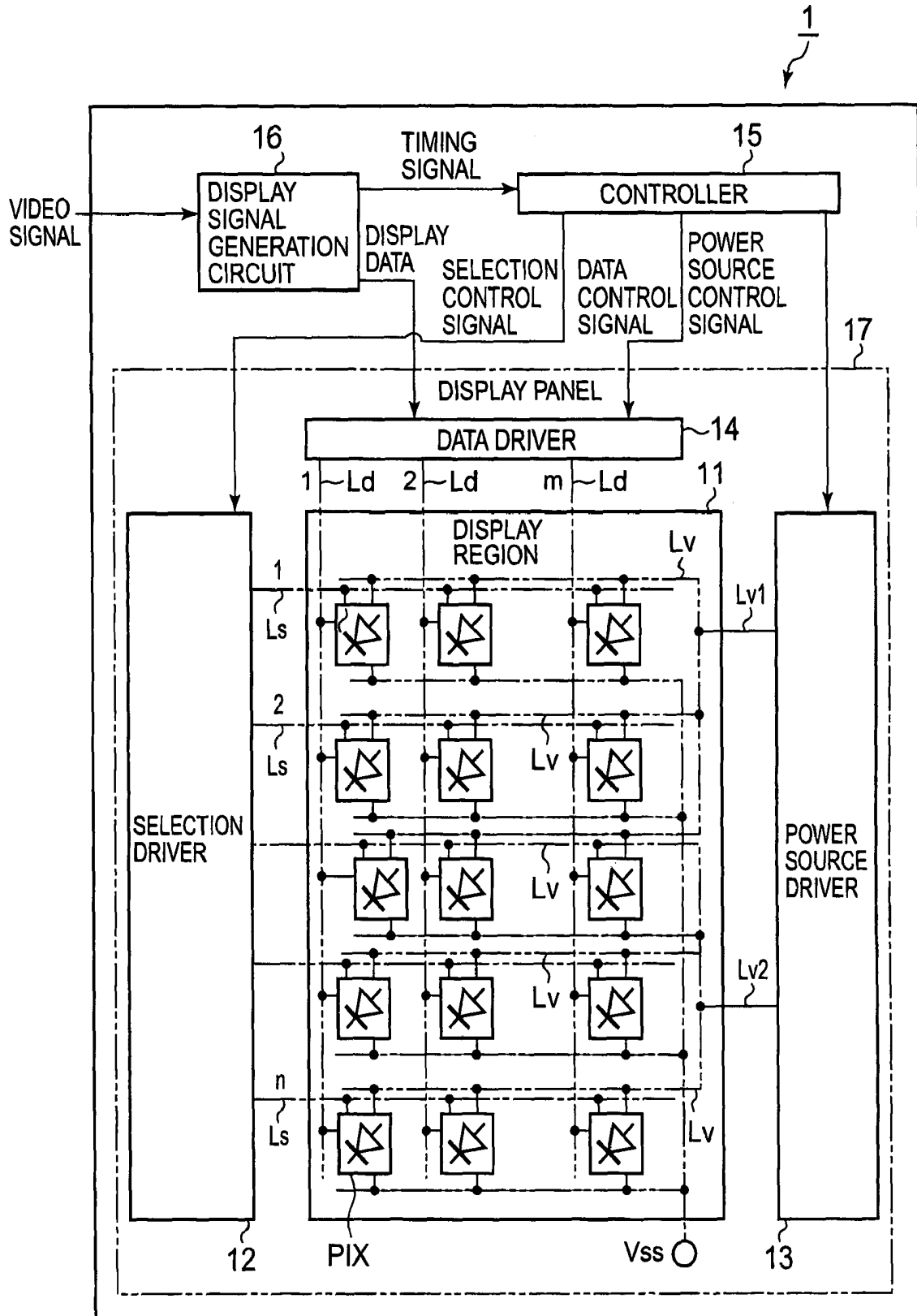


FIG. 10

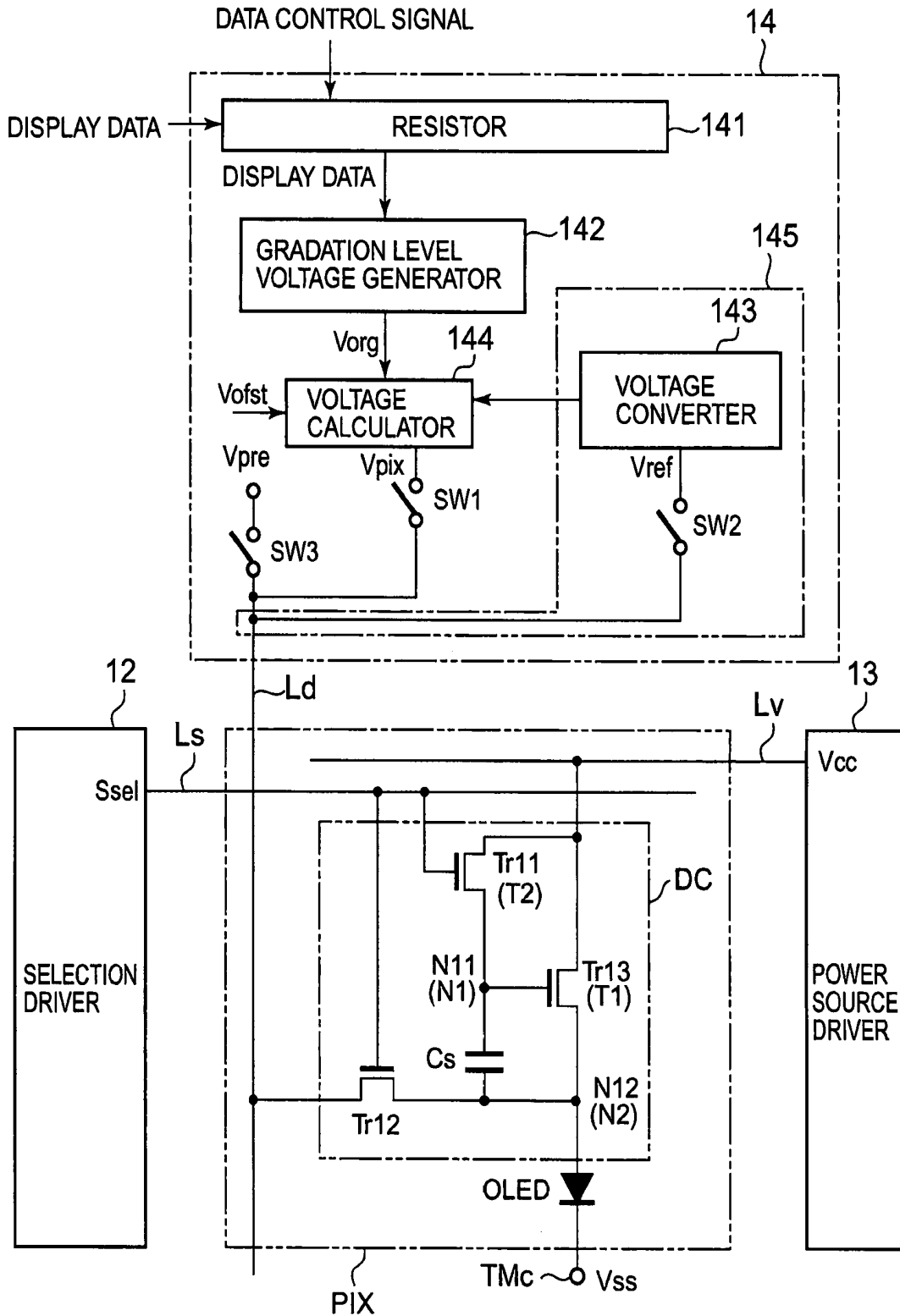


FIG. 11

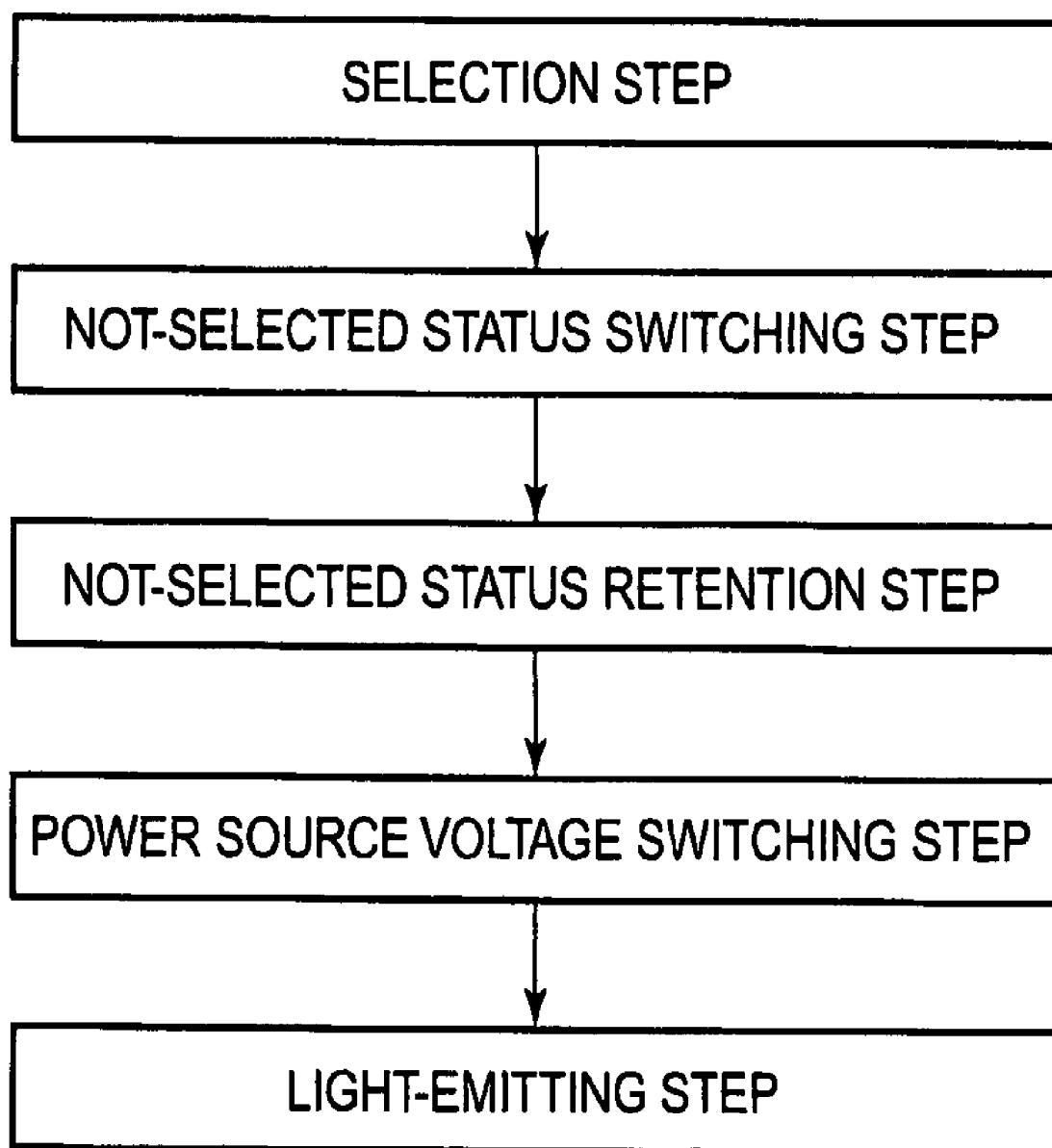


FIG. 12

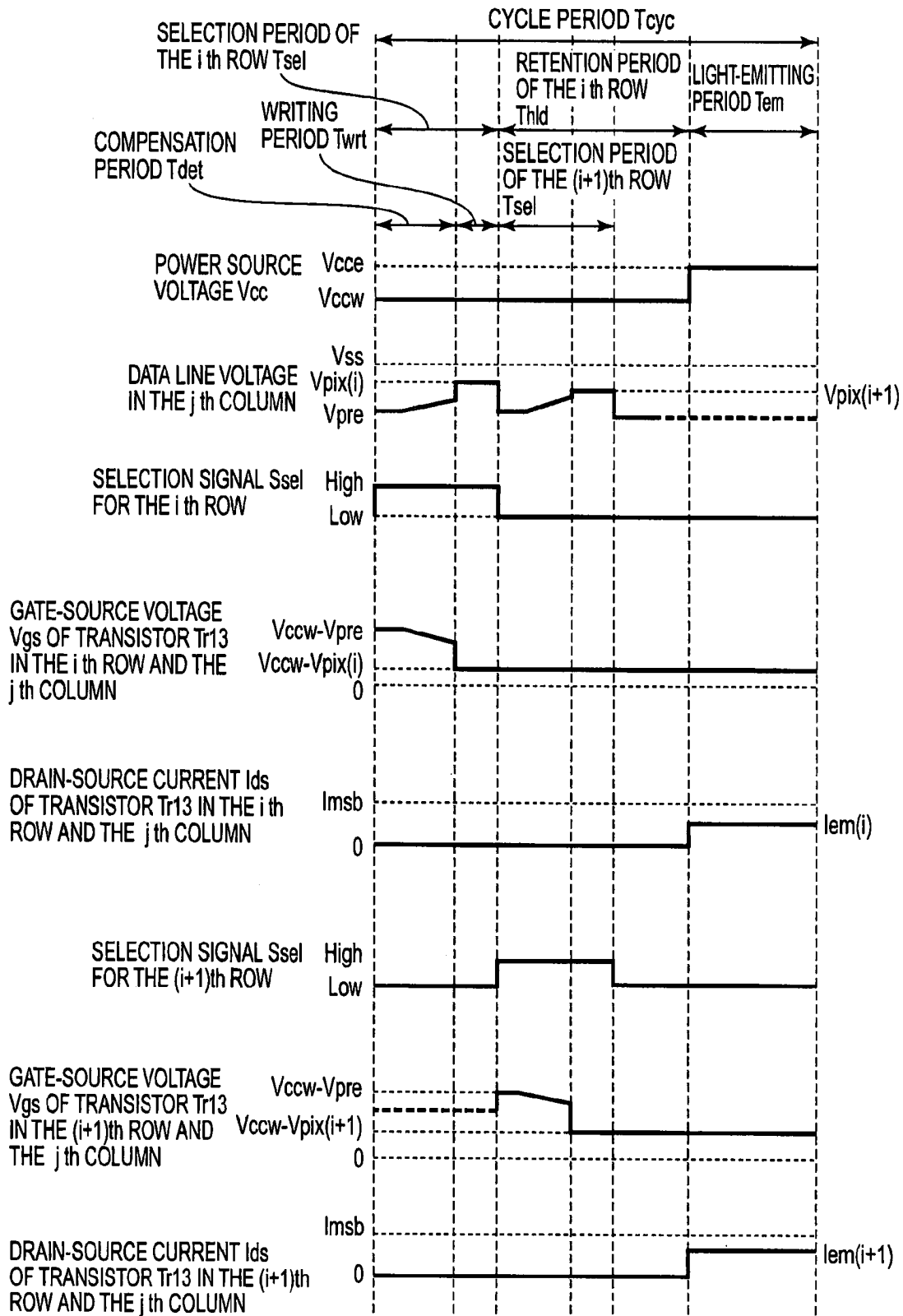


FIG. 13

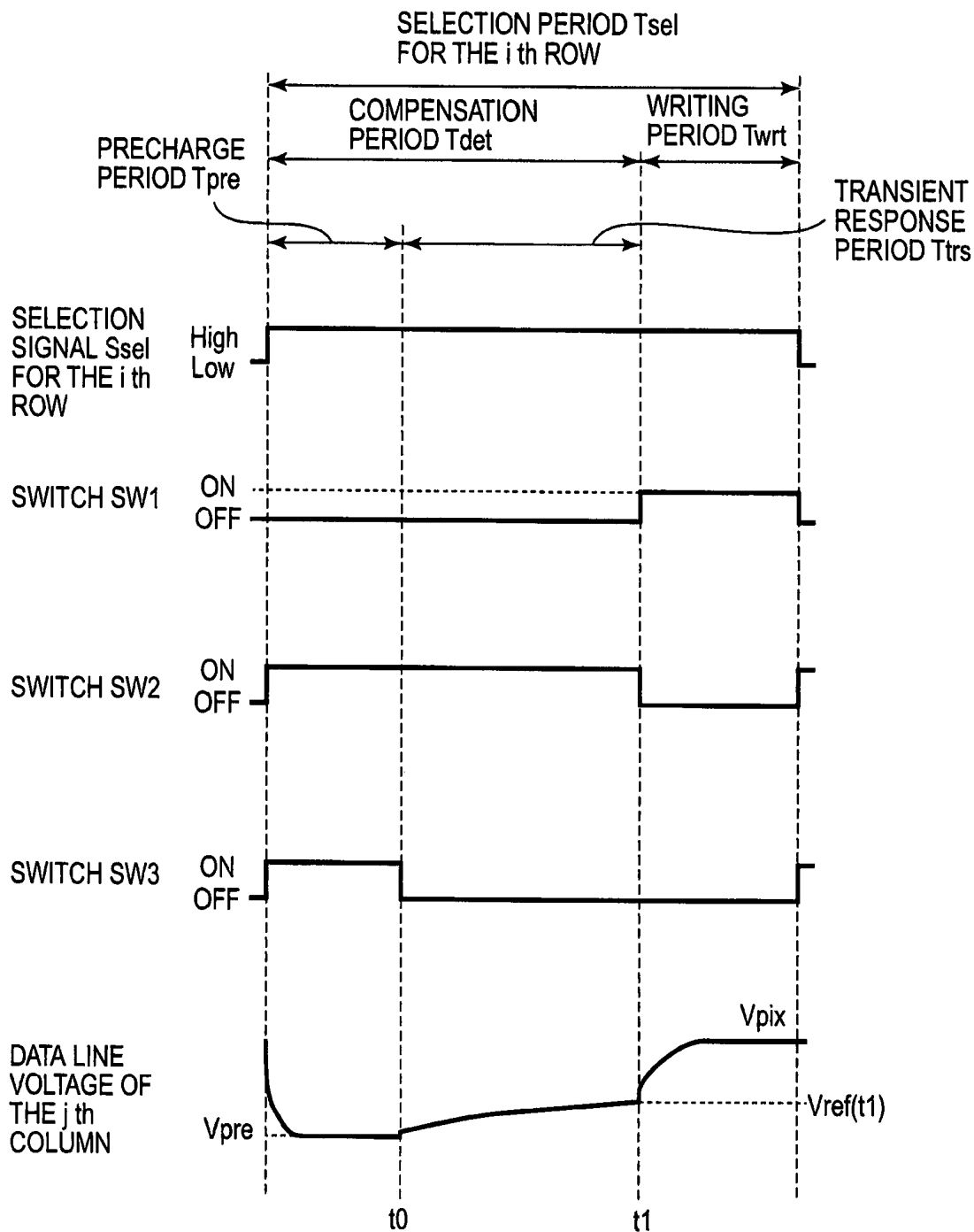


FIG. 14

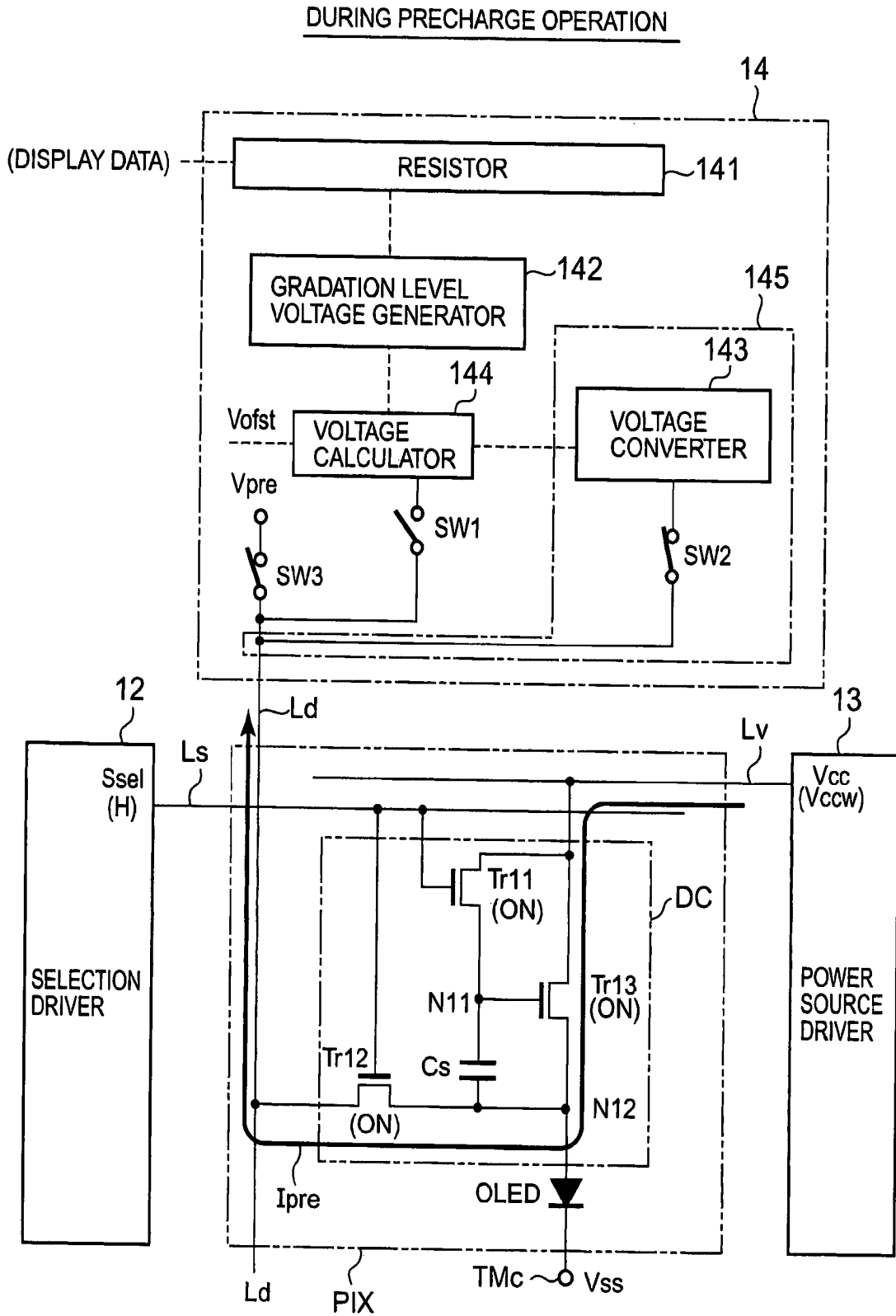


FIG. 15

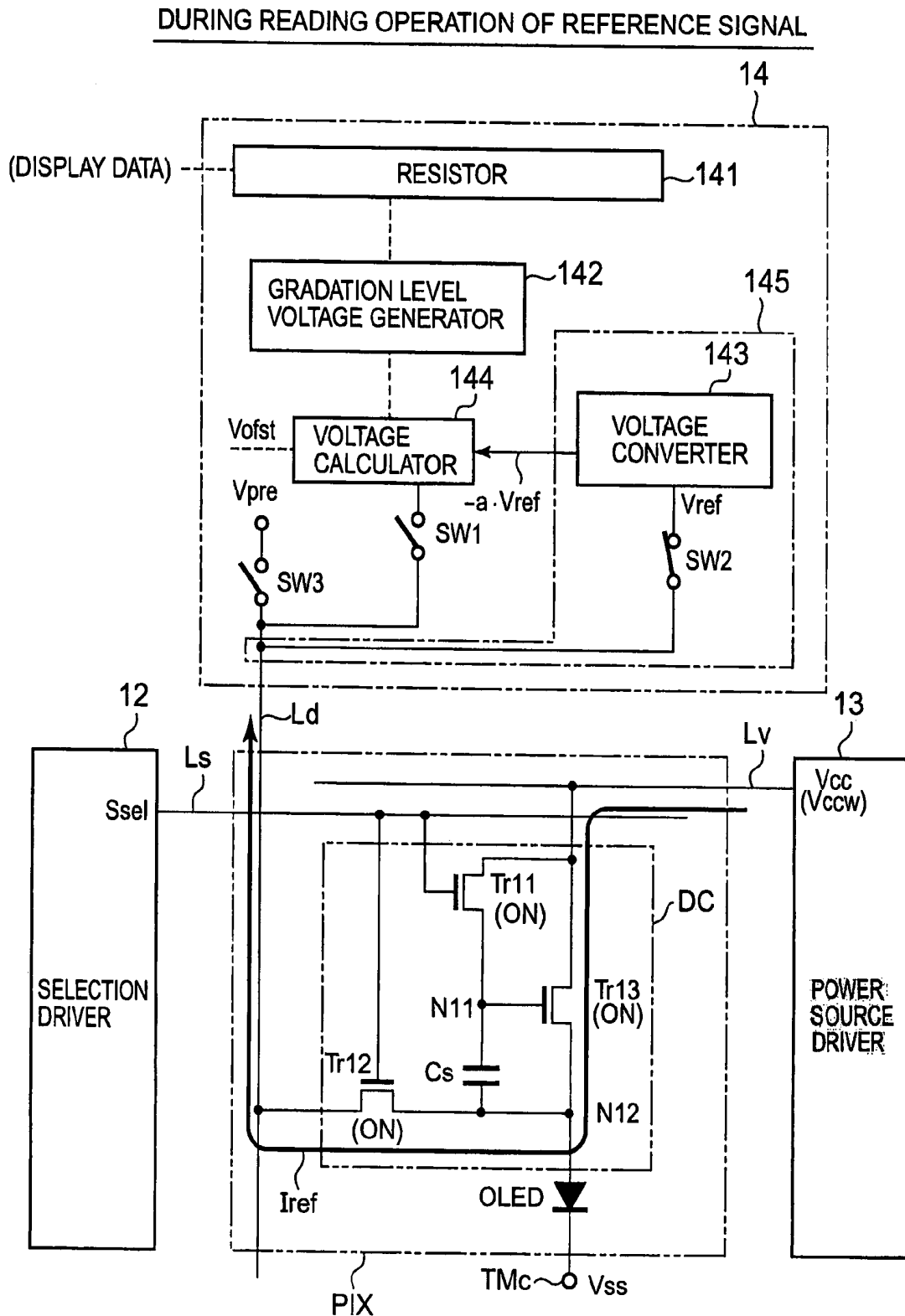


FIG. 16

DURING WRITING OPERATION

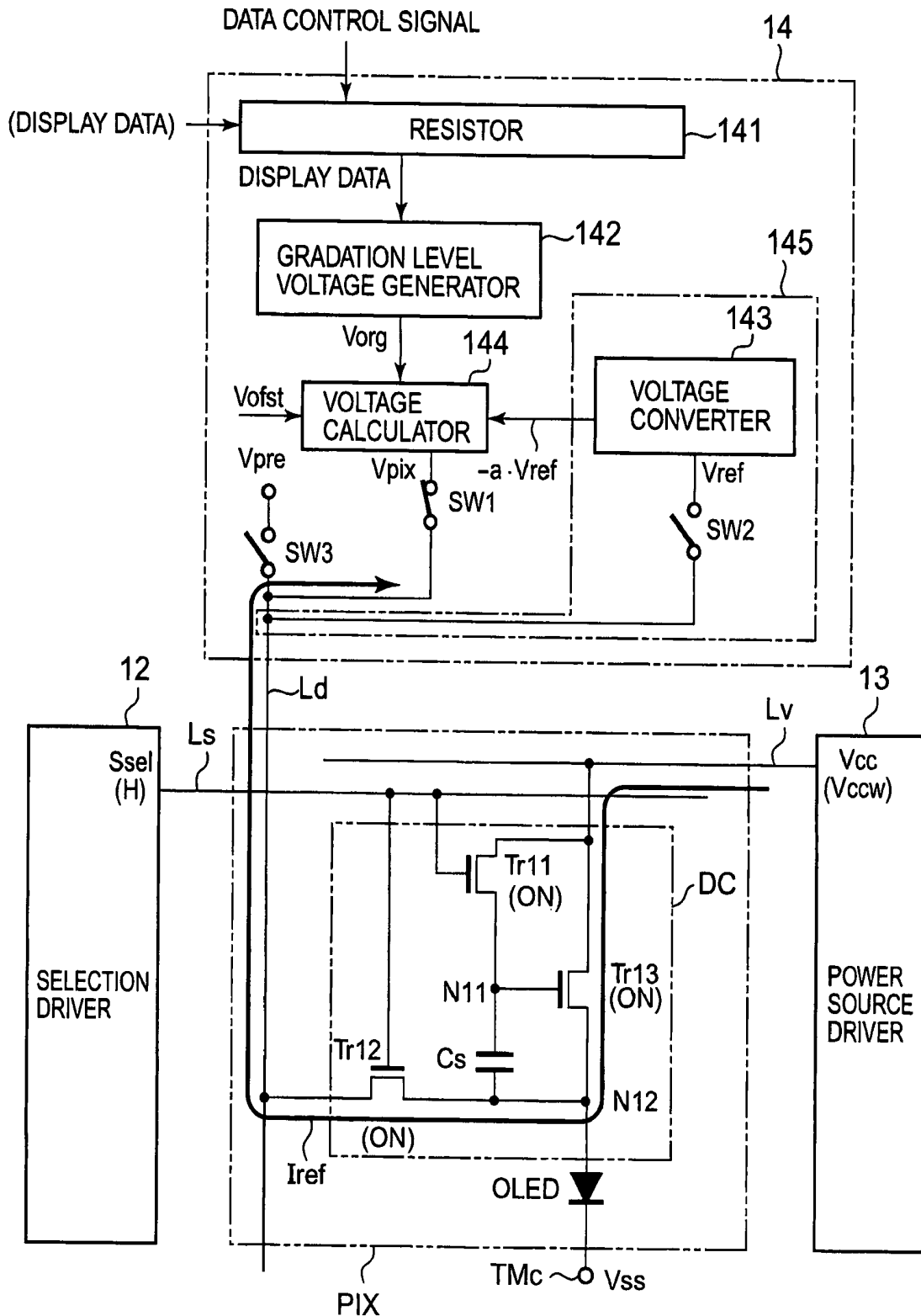


FIG. 17

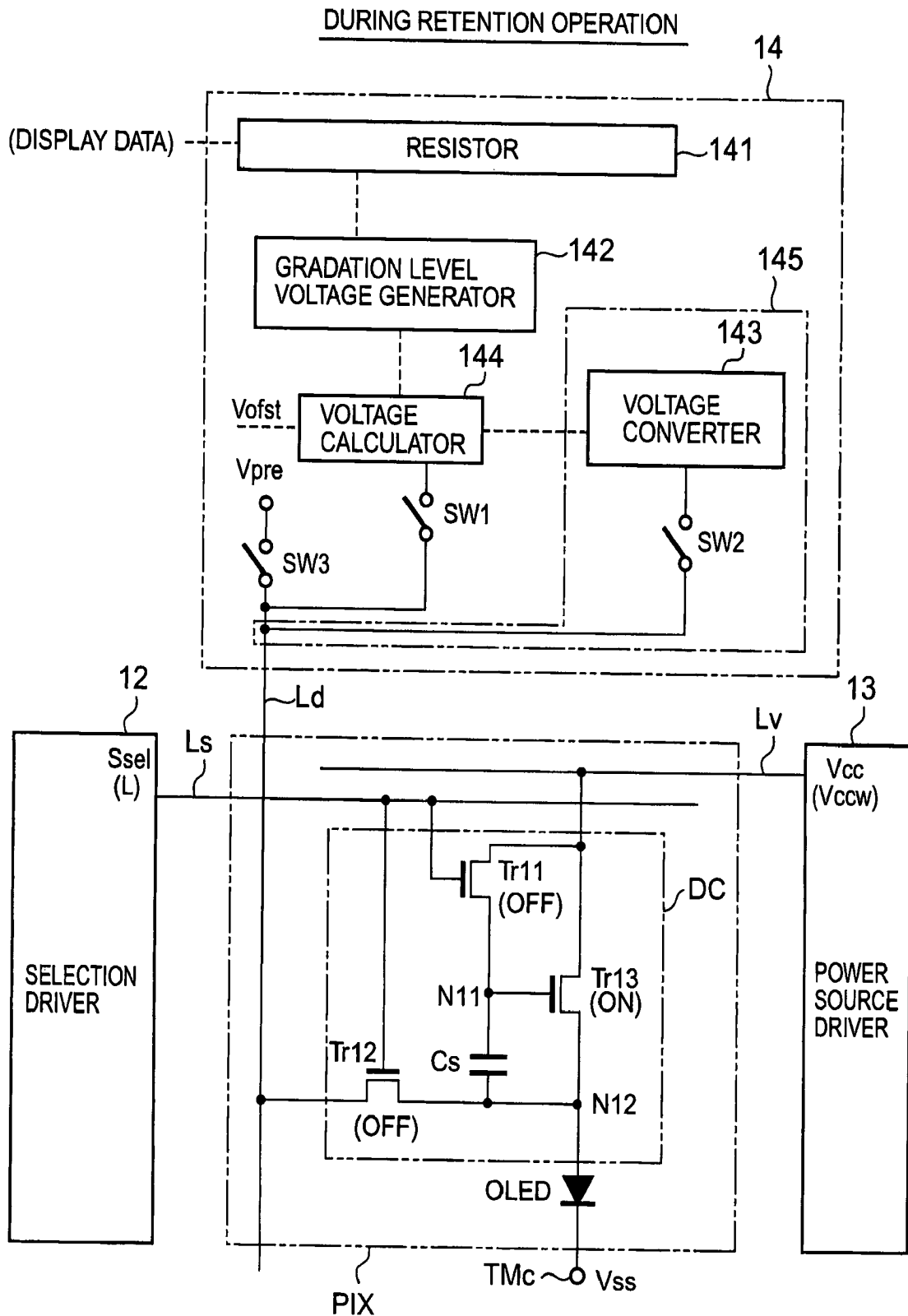


FIG. 18

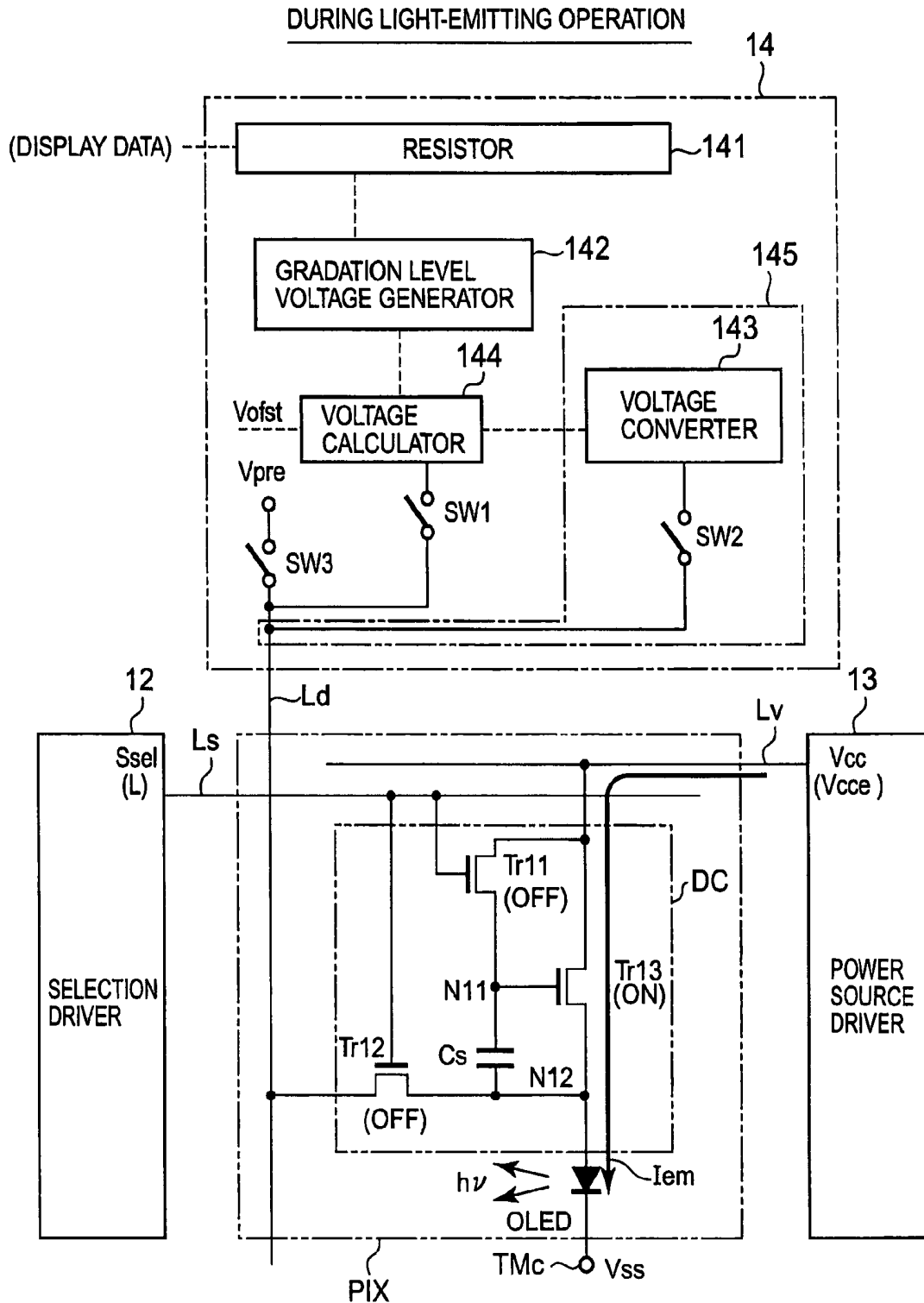


FIG. 19

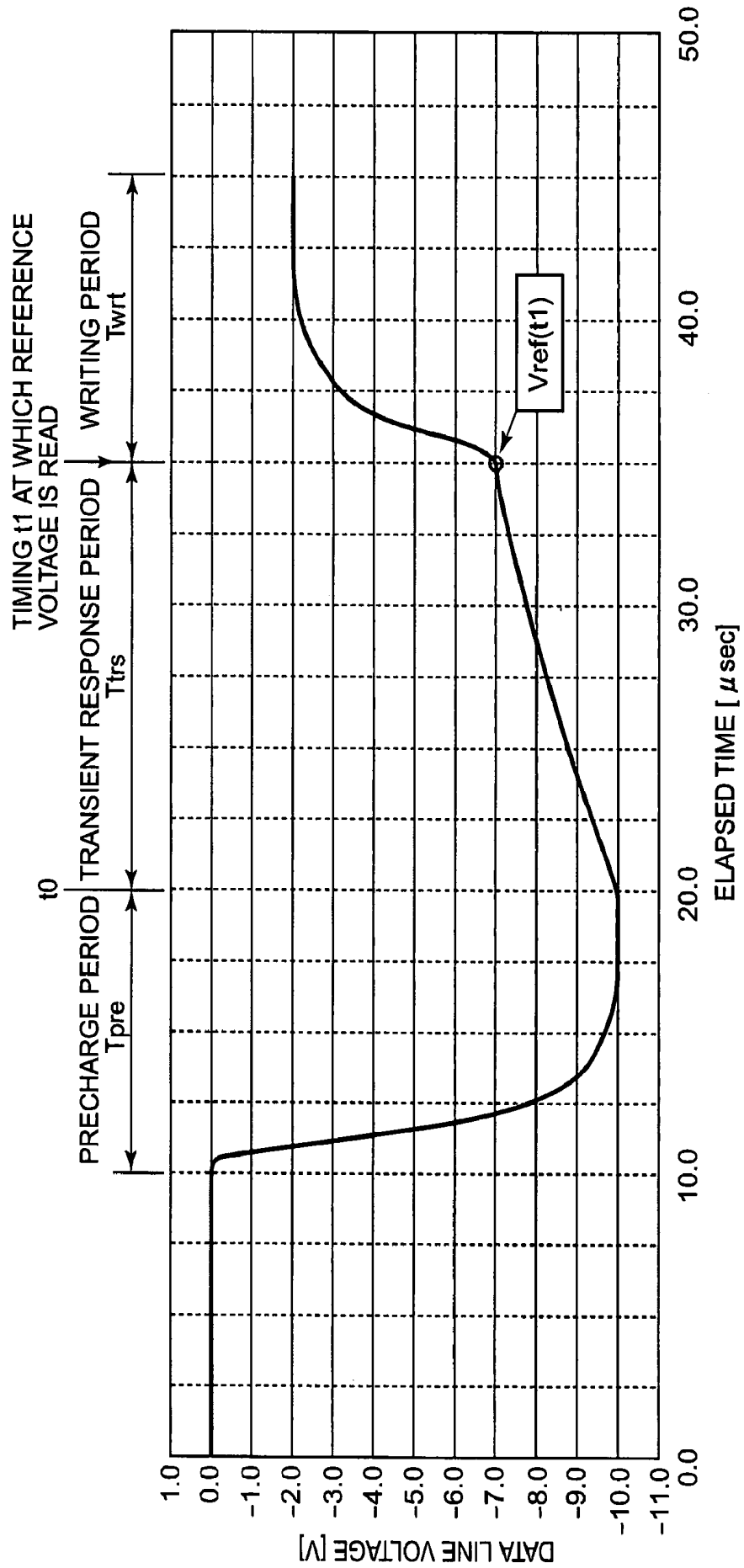


FIG. 20

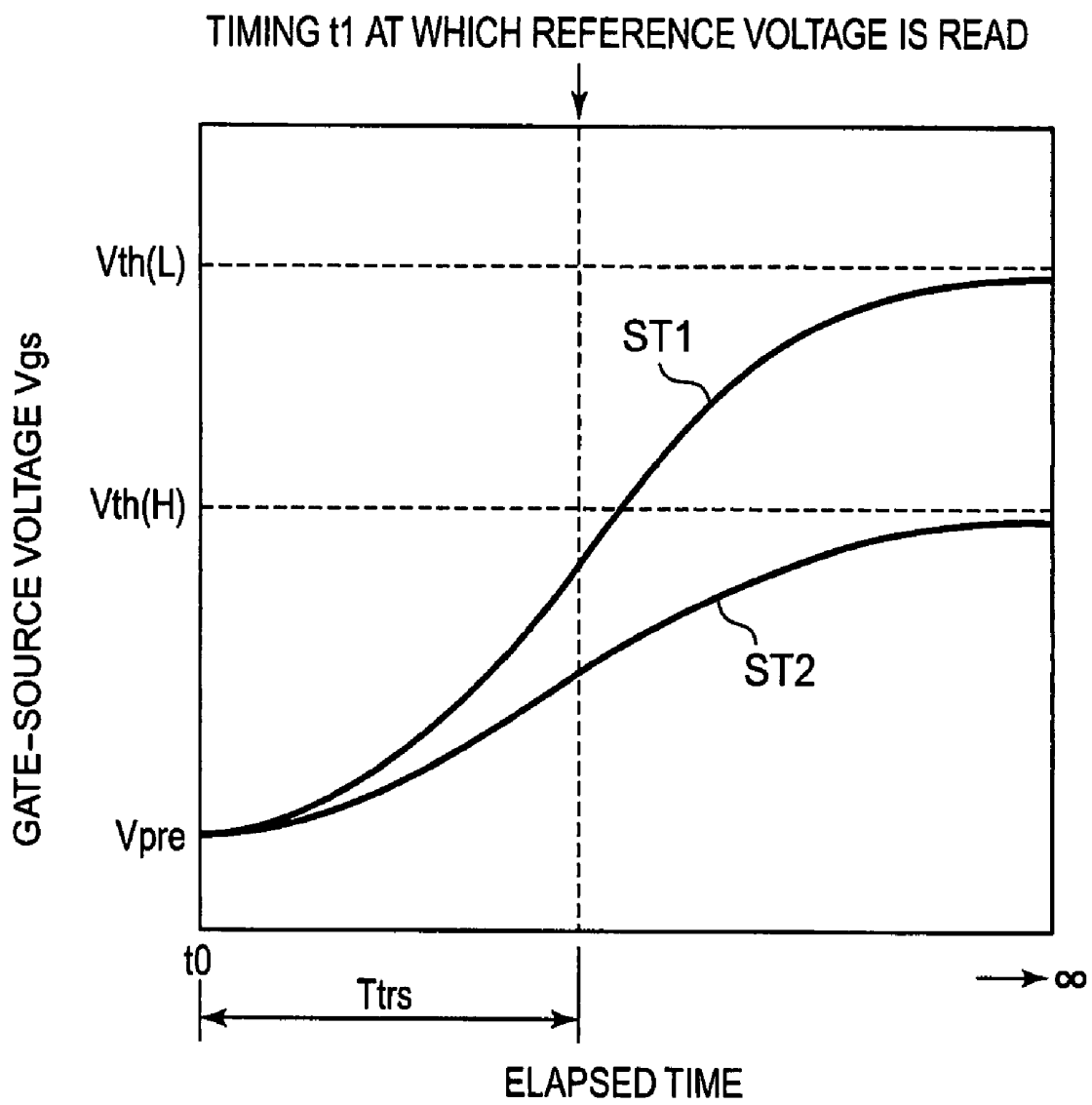


FIG. 21

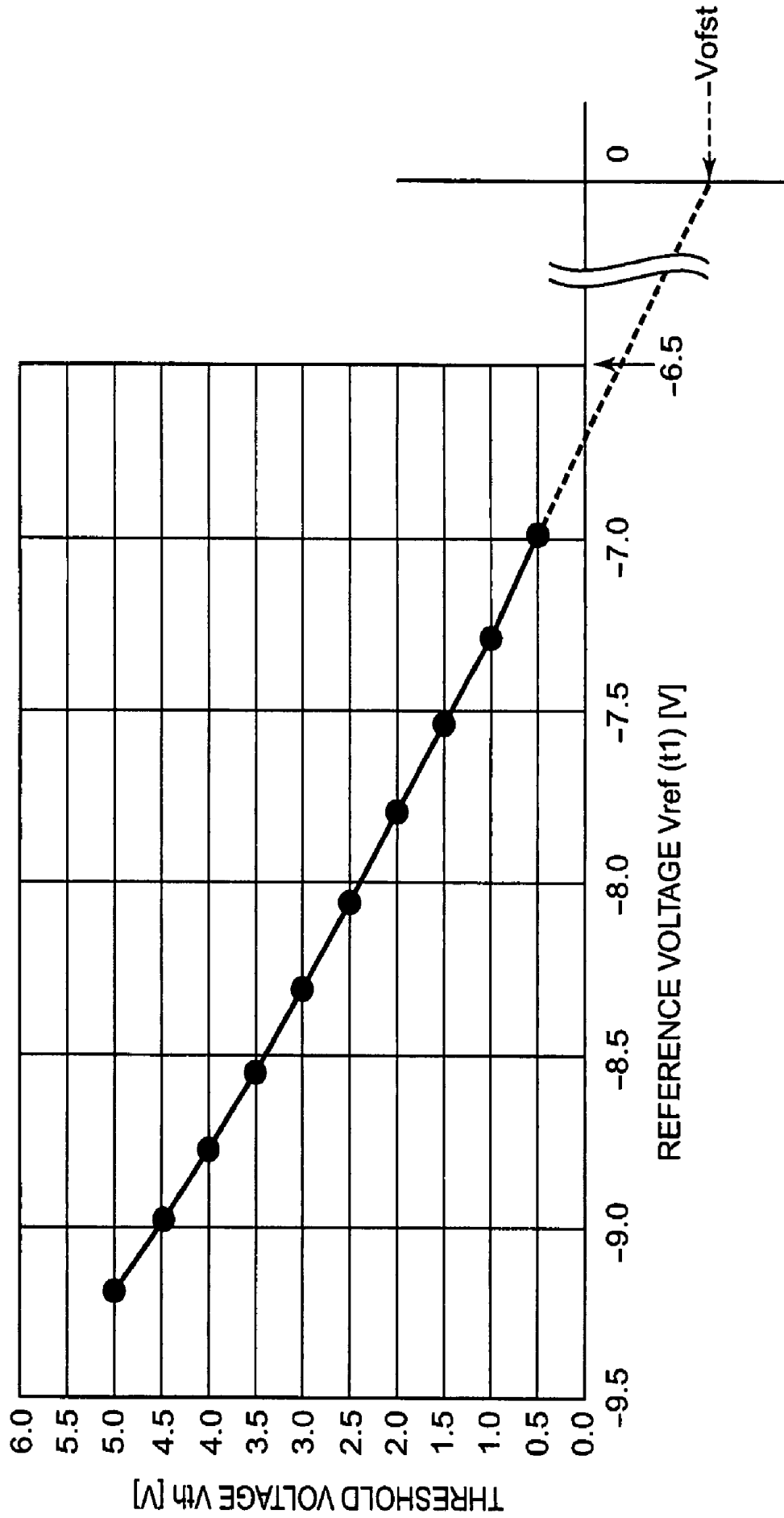
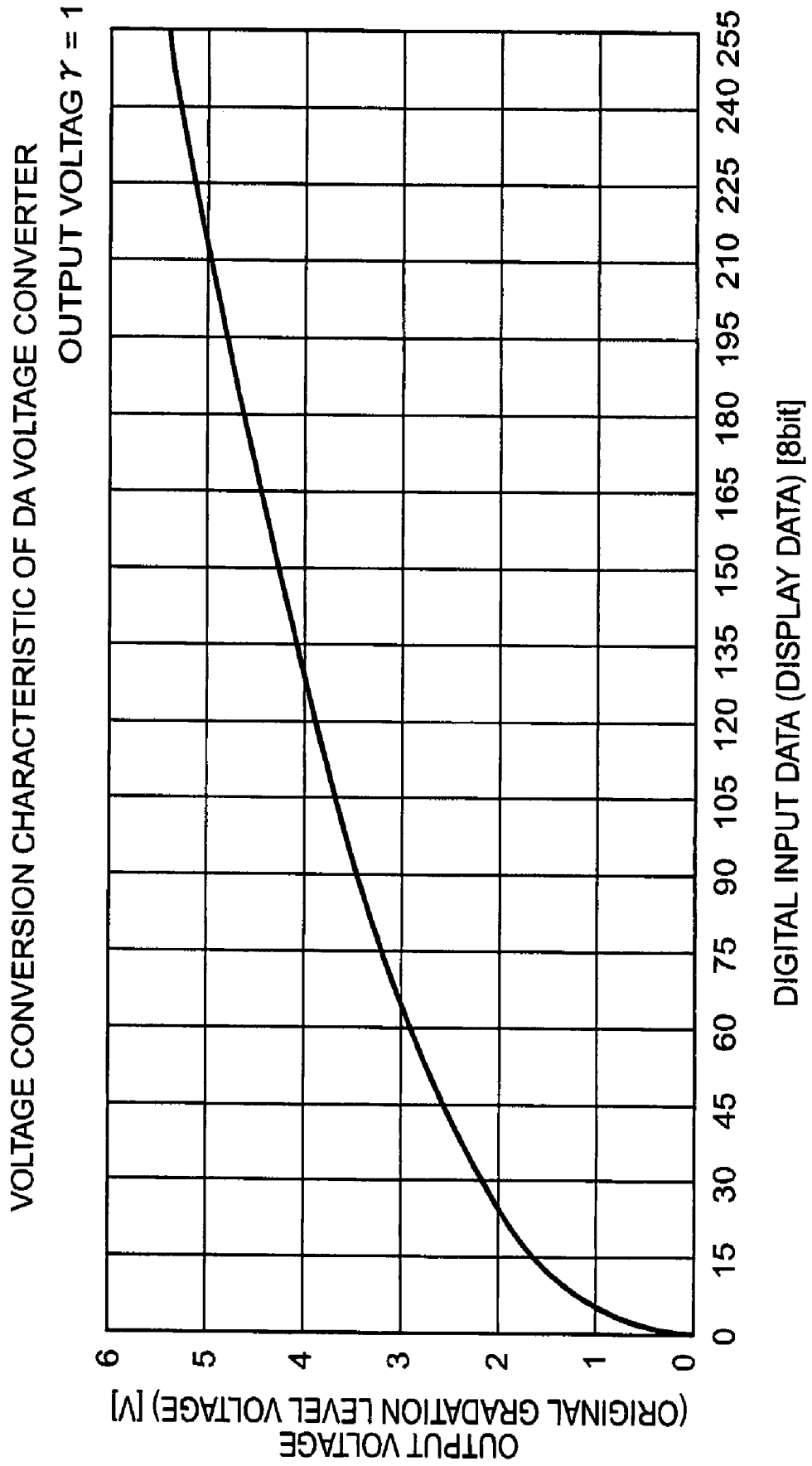
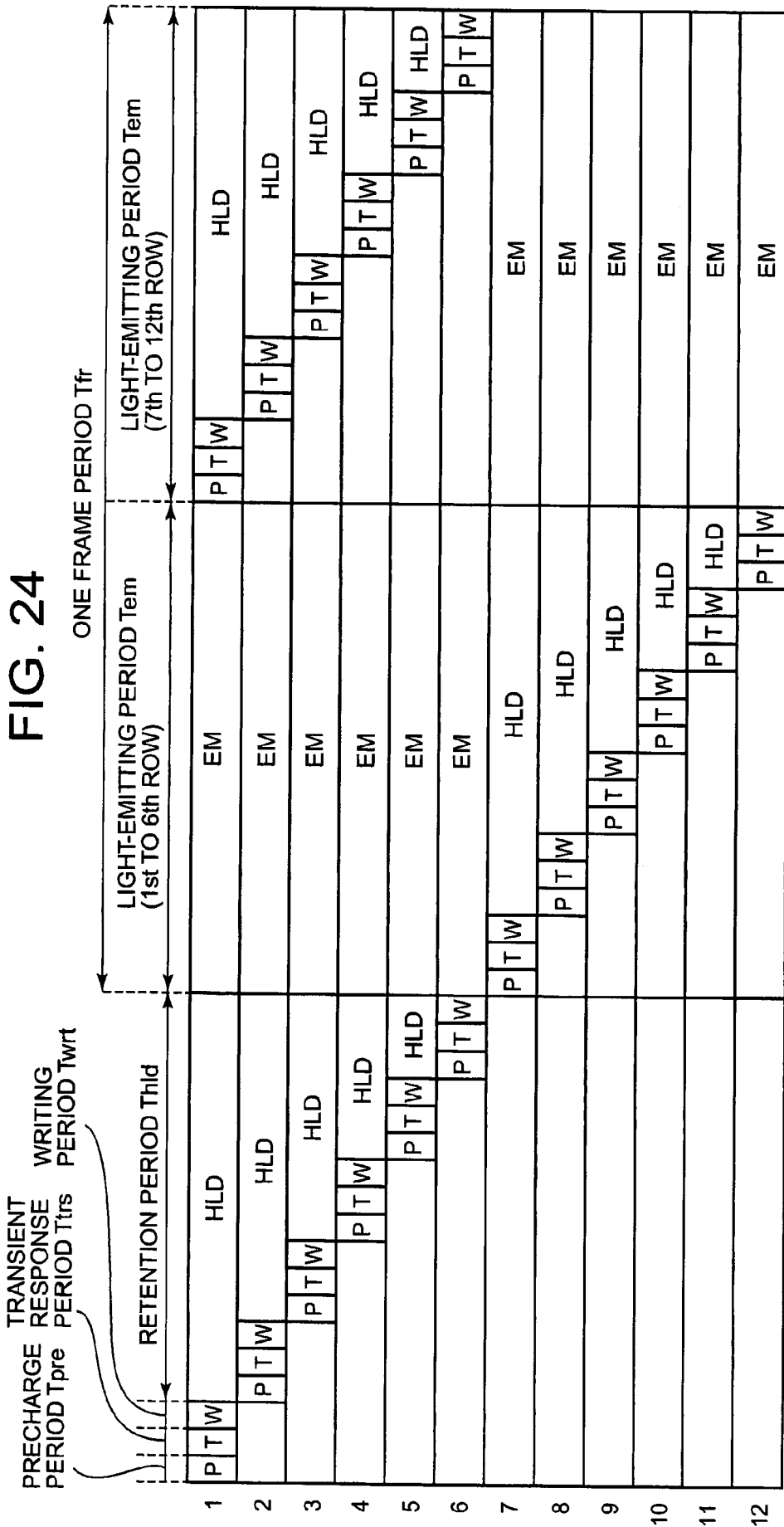


FIG. 23





P PRECHARGE OPERATION, T TRANSIENT RESPONSE, W WRITING OPERATION,
 HLD RETENTION OPERATION, EM LIGHT-EMITTING OPERATION

FIG. 25

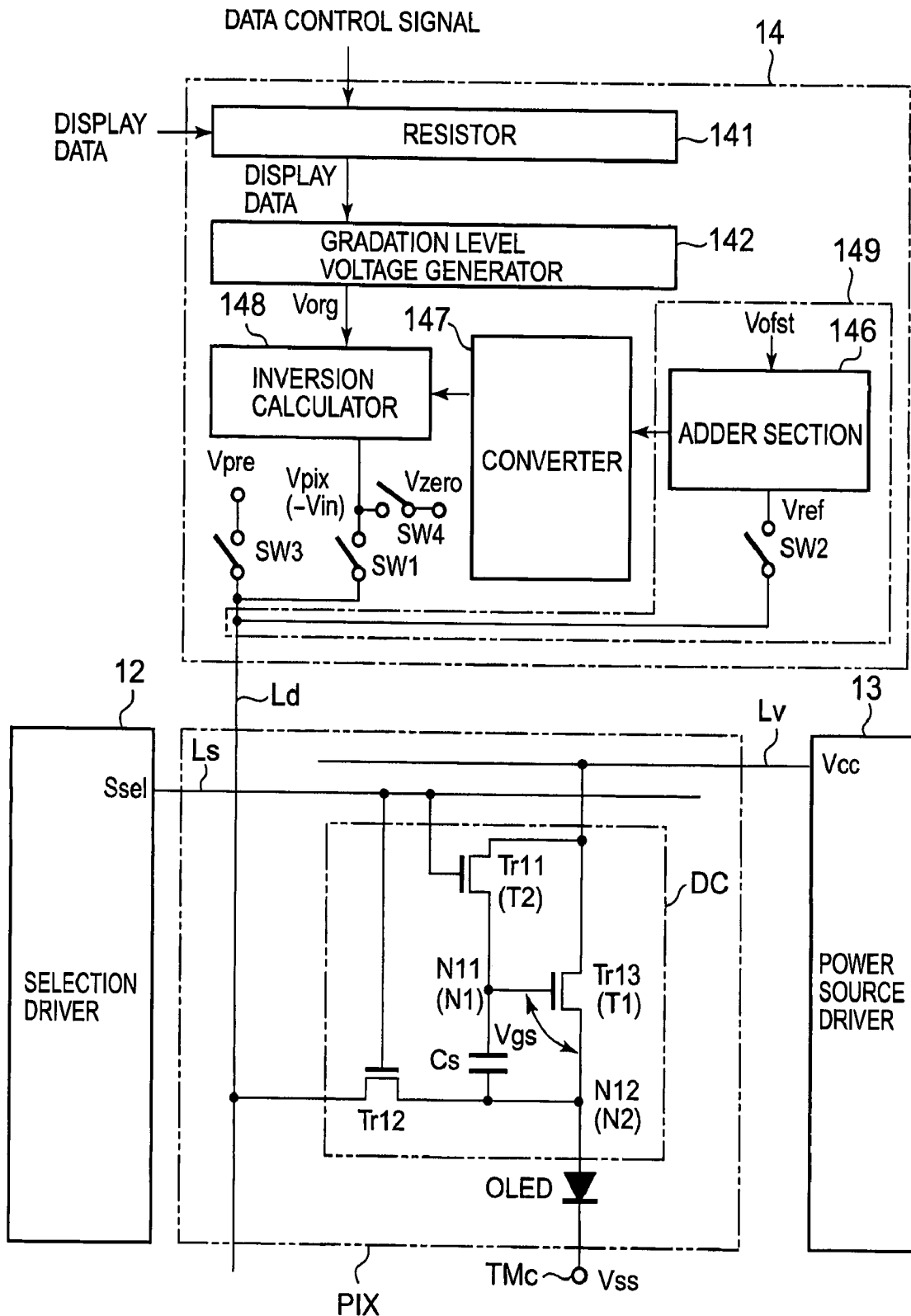


FIG. 26A

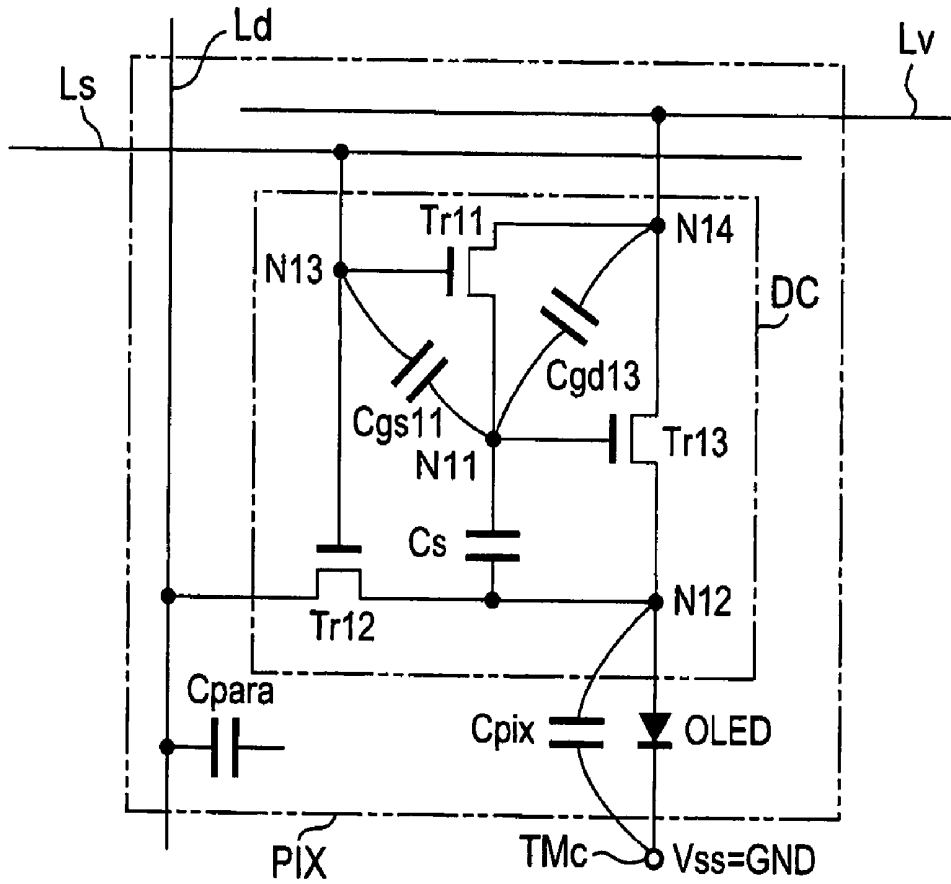


FIG. 26B

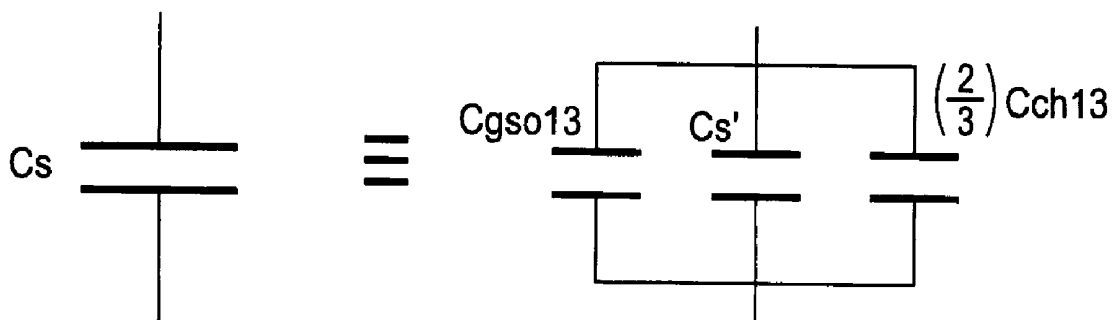


FIG. 27C

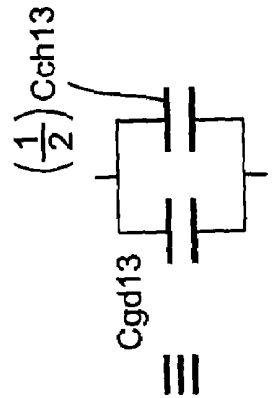


FIG. 27B

EQUIVALENT CIRCUIT DURING LIGHT-EMITTING OPERATION

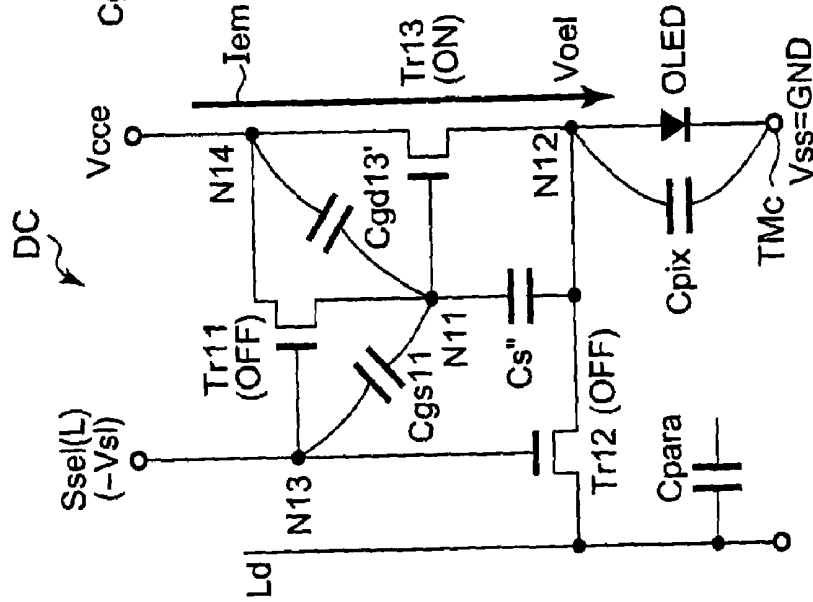


FIG. 27A

EQUIVALENT CIRCUIT DURING WRITING OPERATION

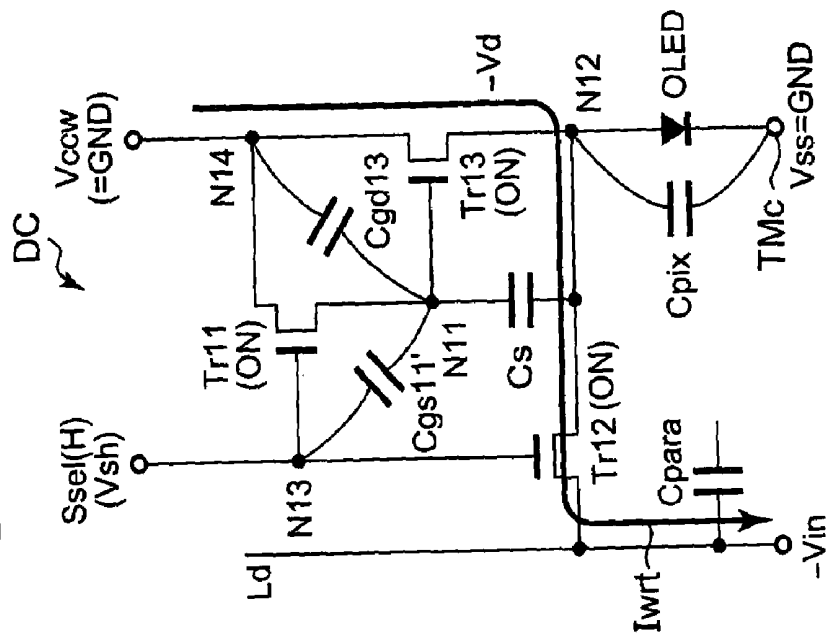


FIG. 27D

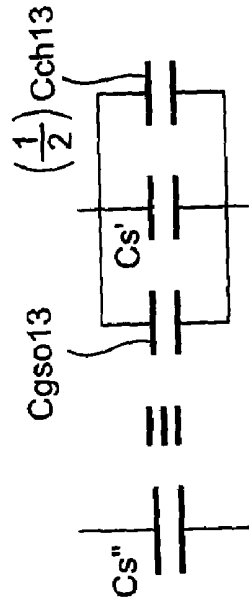


FIG. 28A

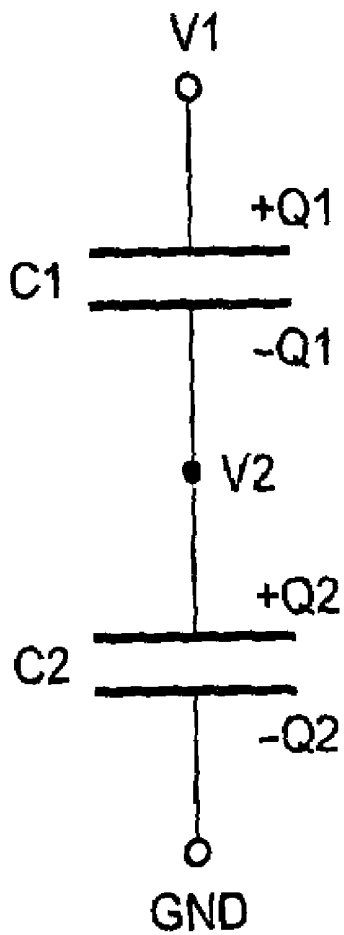


FIG. 28B

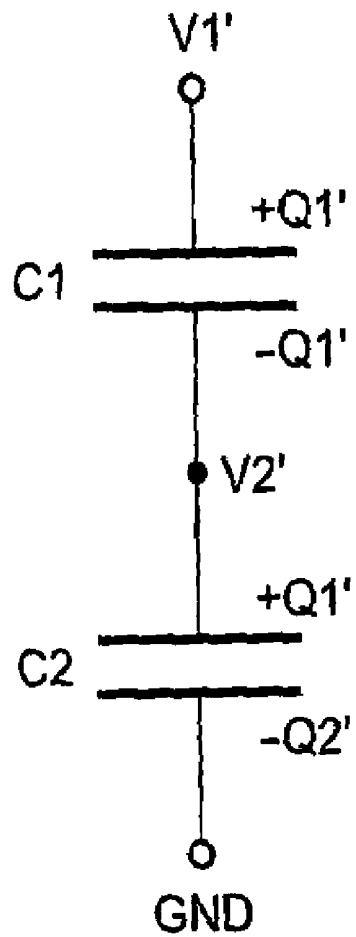


FIG. 29A

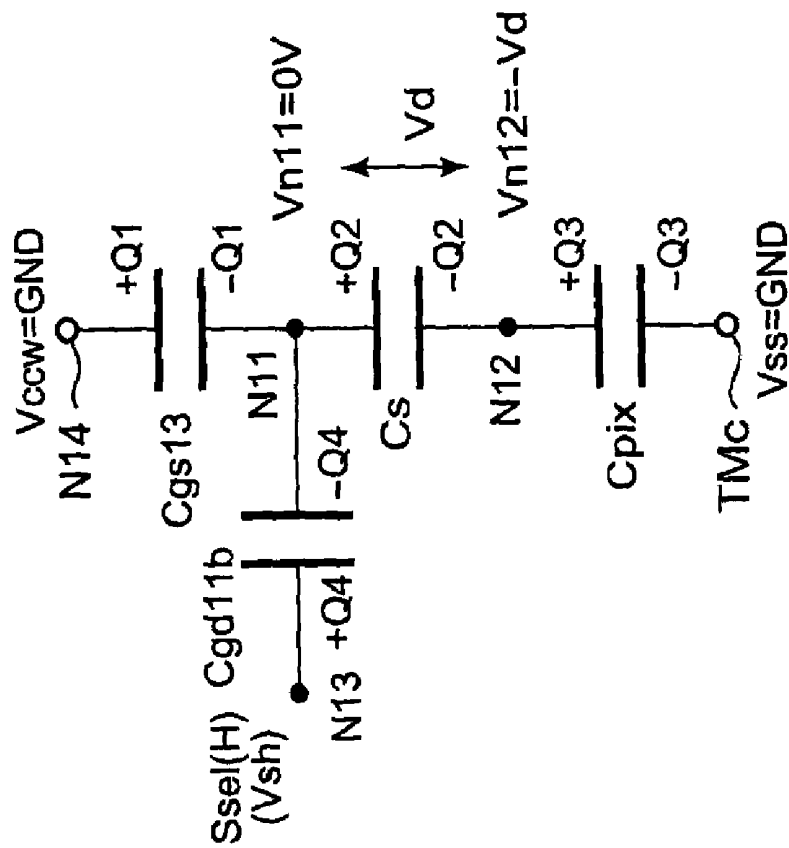


FIG. 29B

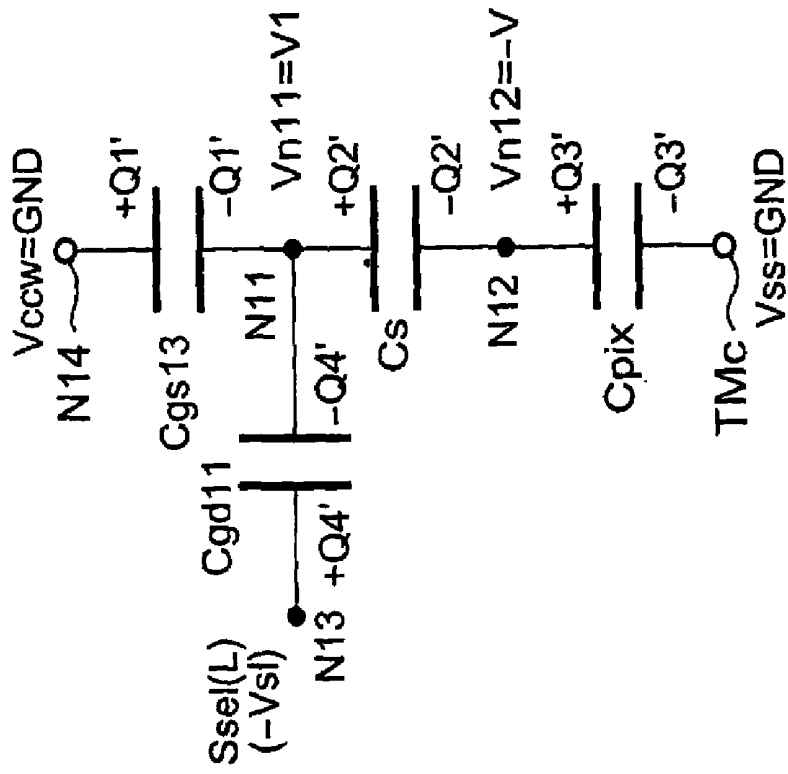


FIG. 31A

SHIFT FROM SELECTION STEP
TO NOT-SELECTED STATUS

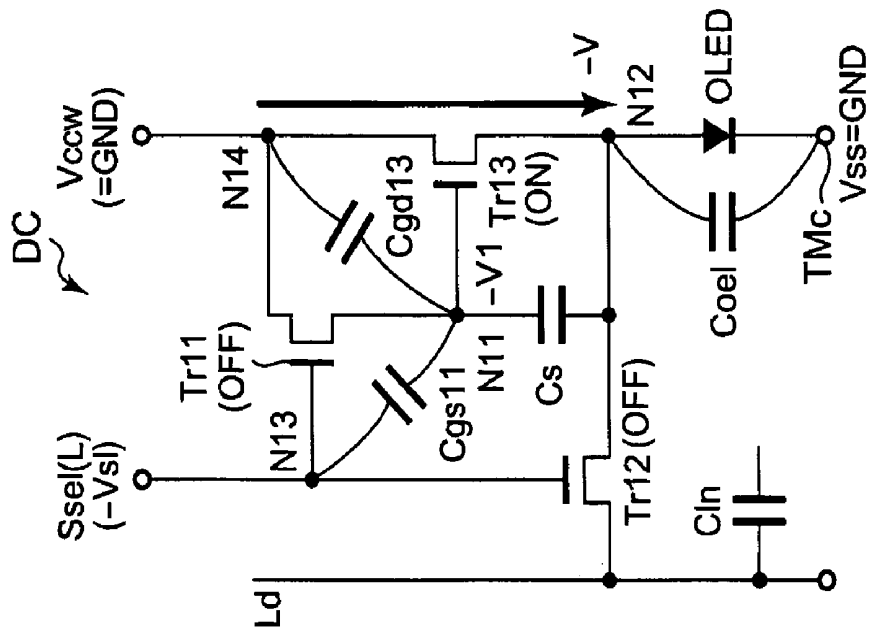


FIG. 31B

VOLTAGE CHANGE IN NOT-SELECTED
STATUS RETENTION STEP

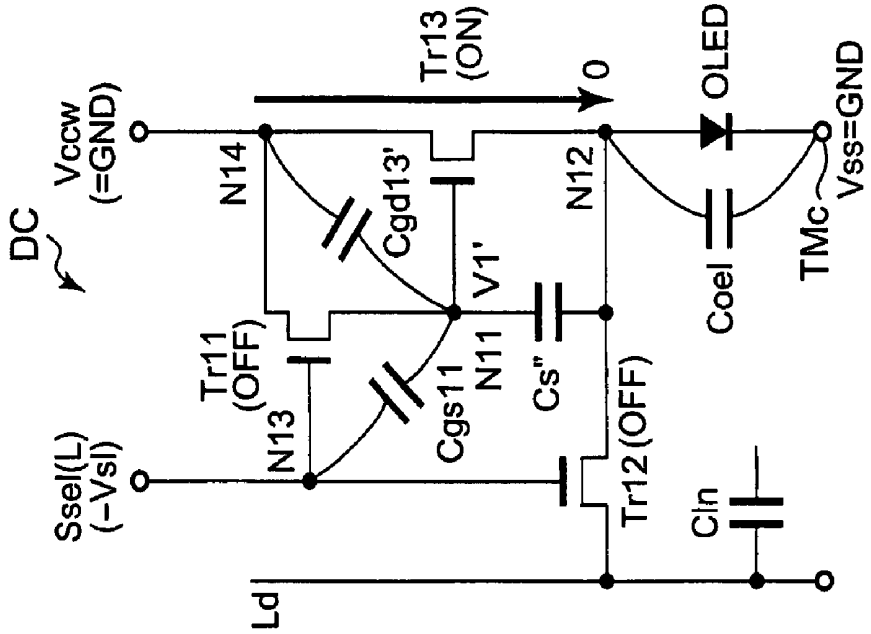


FIG. 34

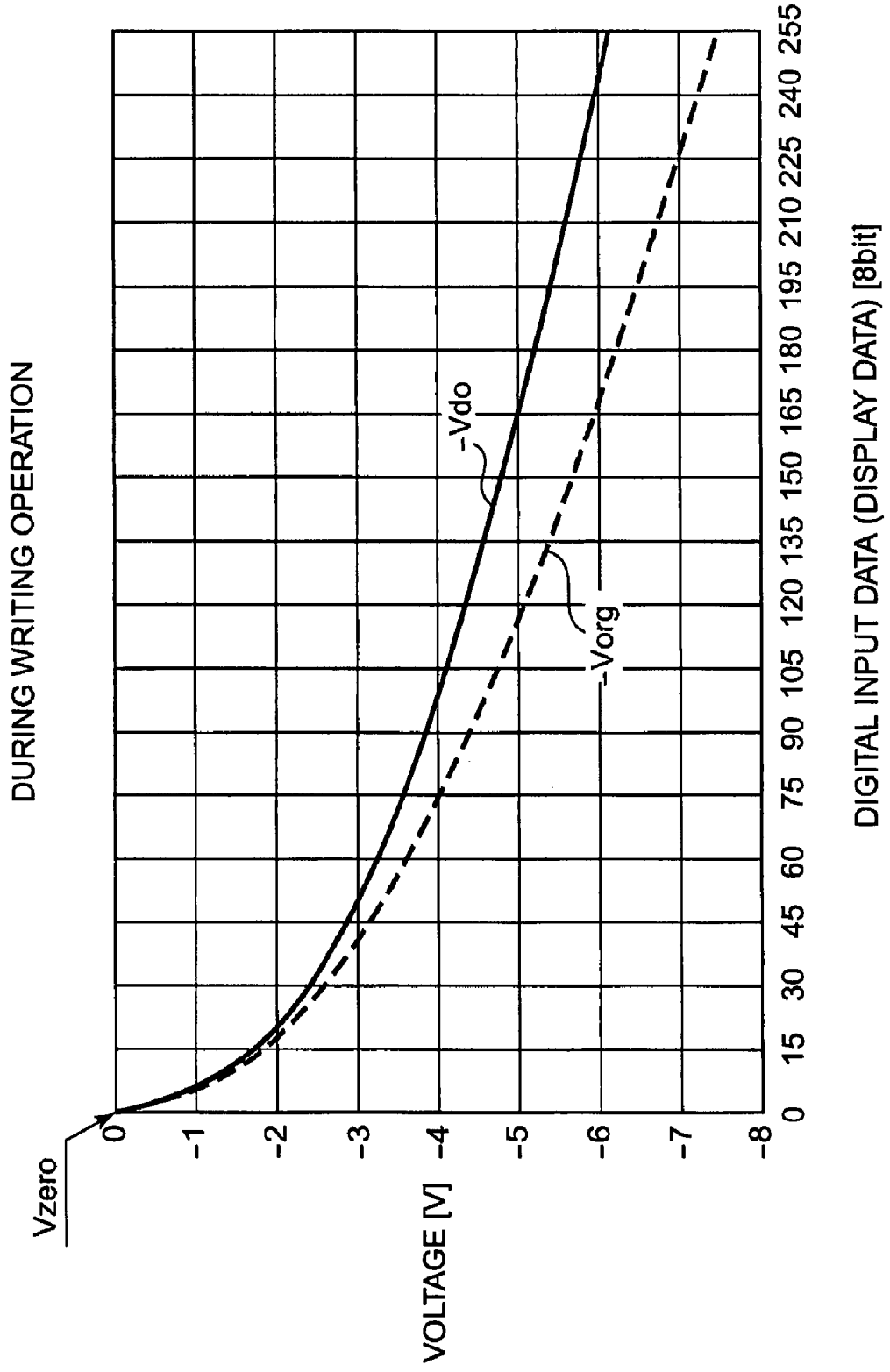


FIG. 35

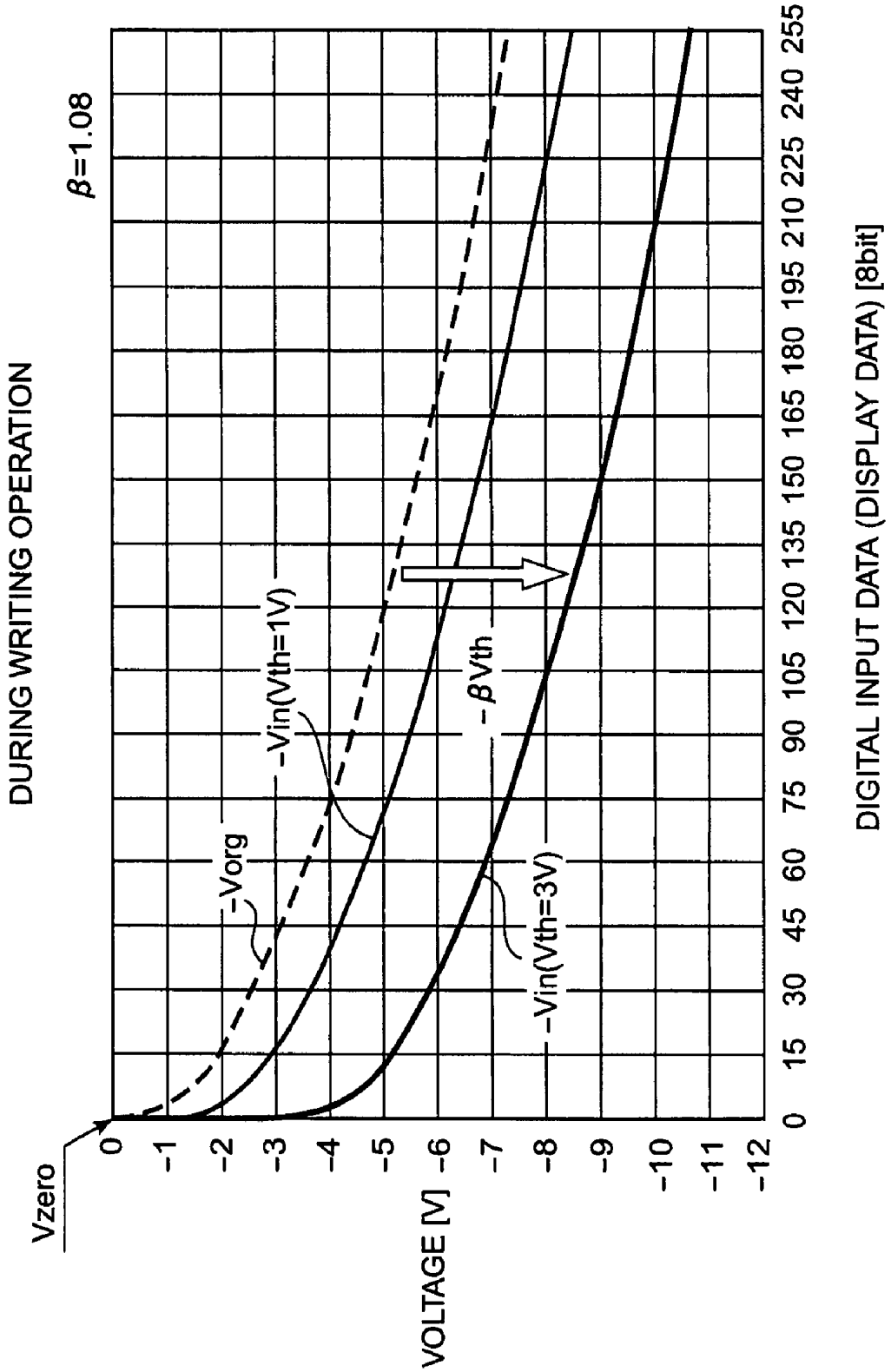


FIG. 36A

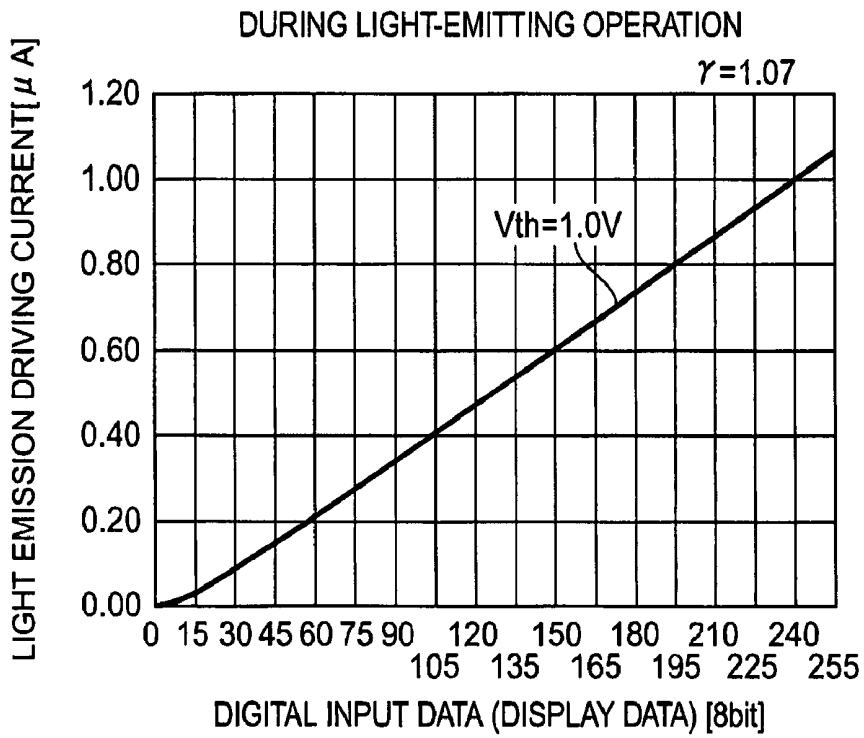


FIG. 36B

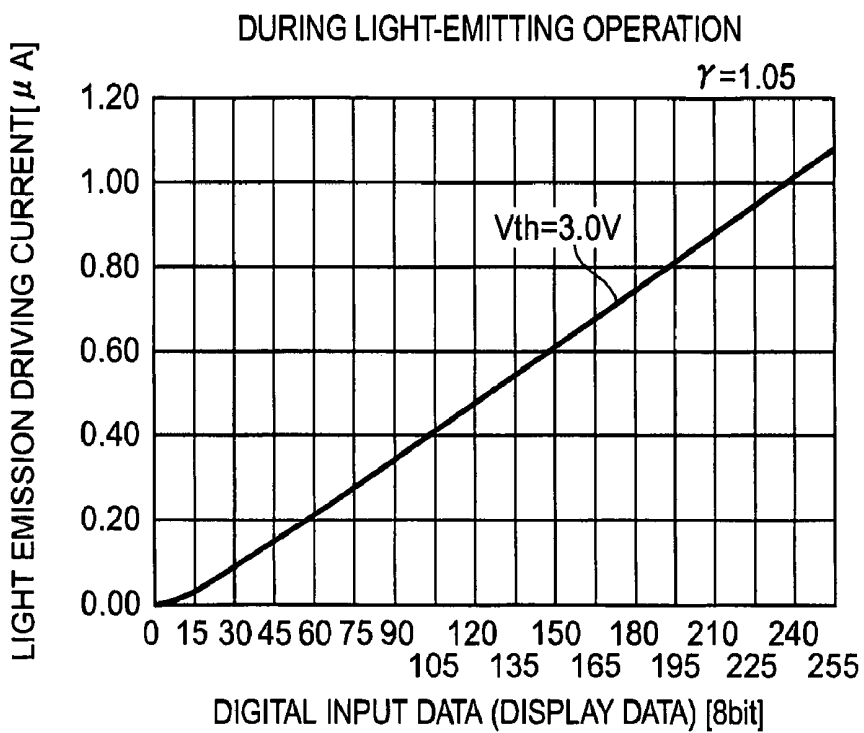


FIG. 37A

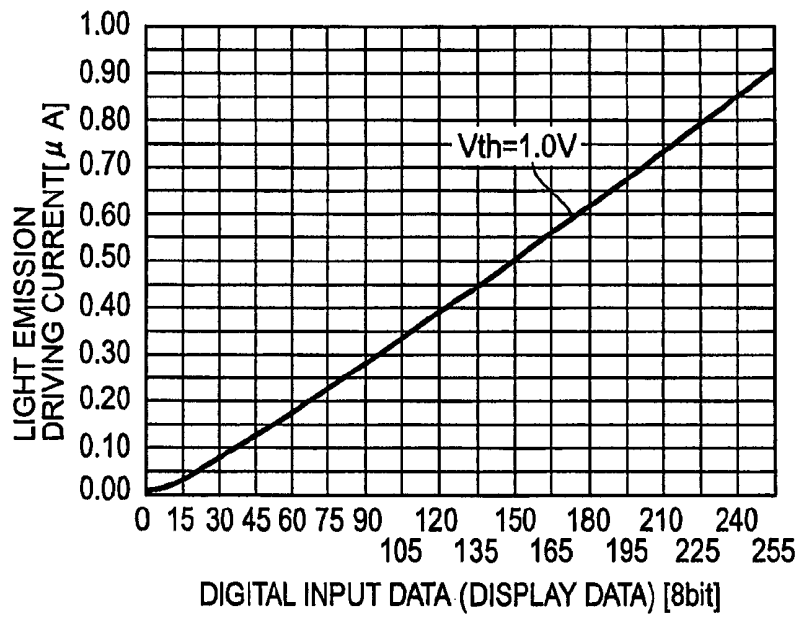


FIG. 37B

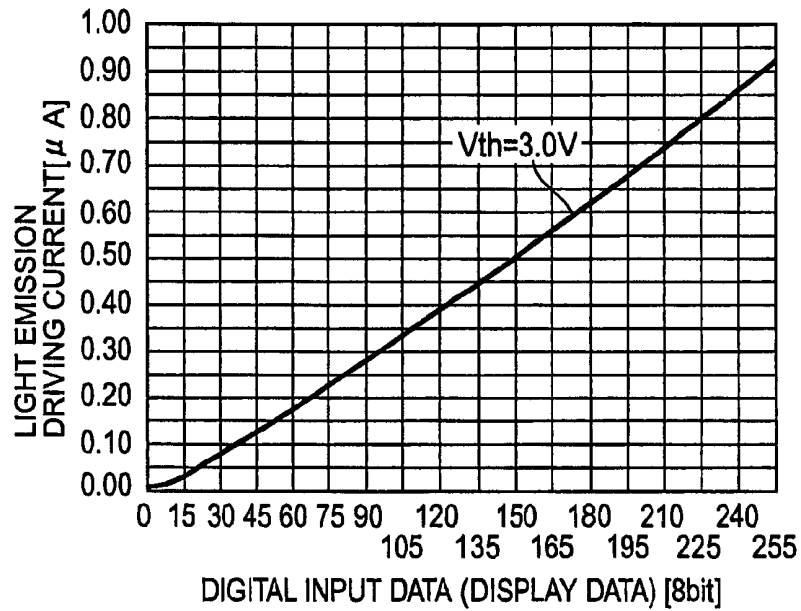


FIG. 37C

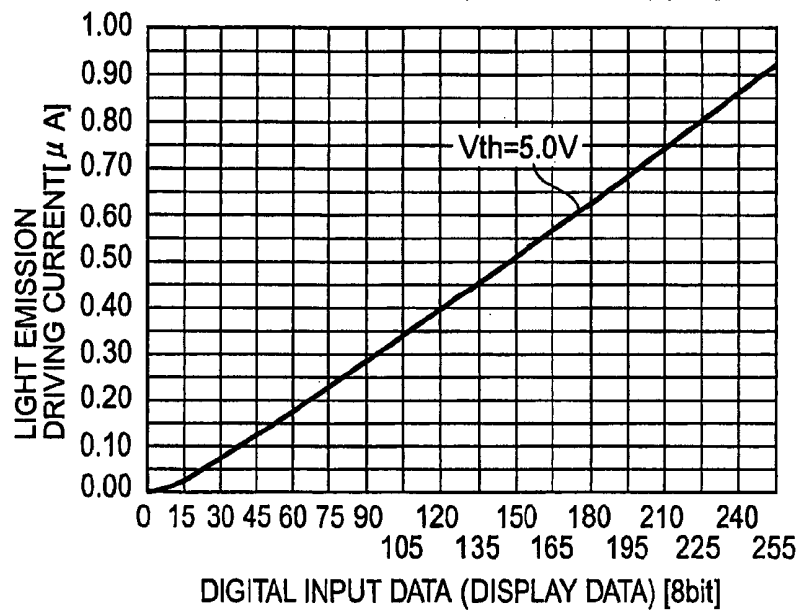


FIG. 38A

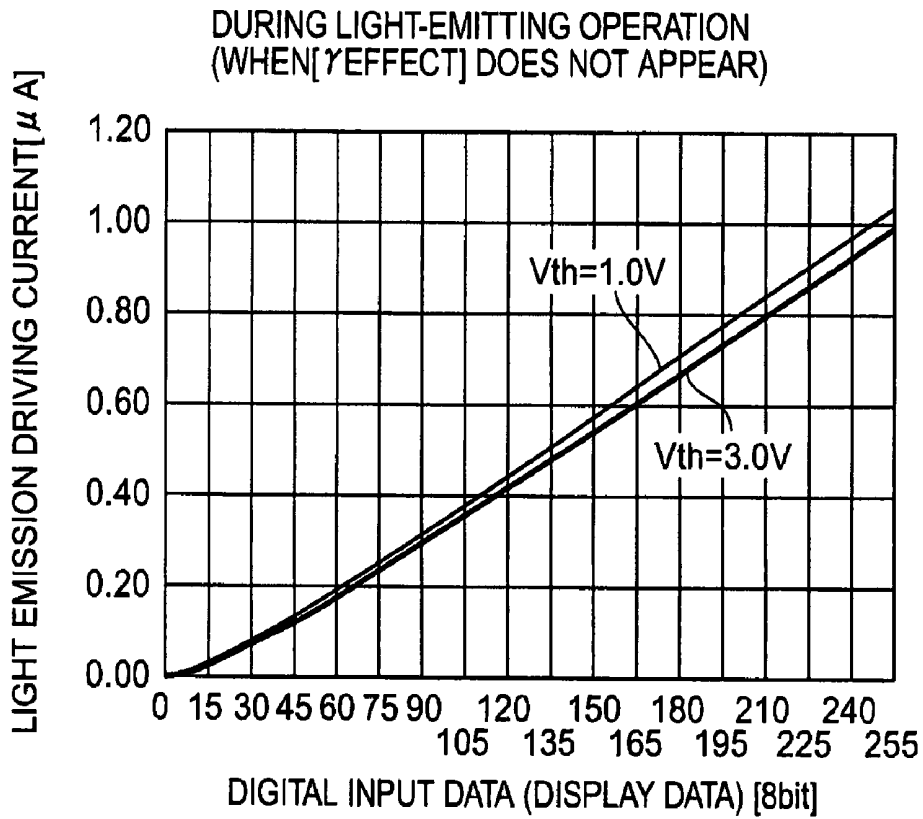


FIG. 38B

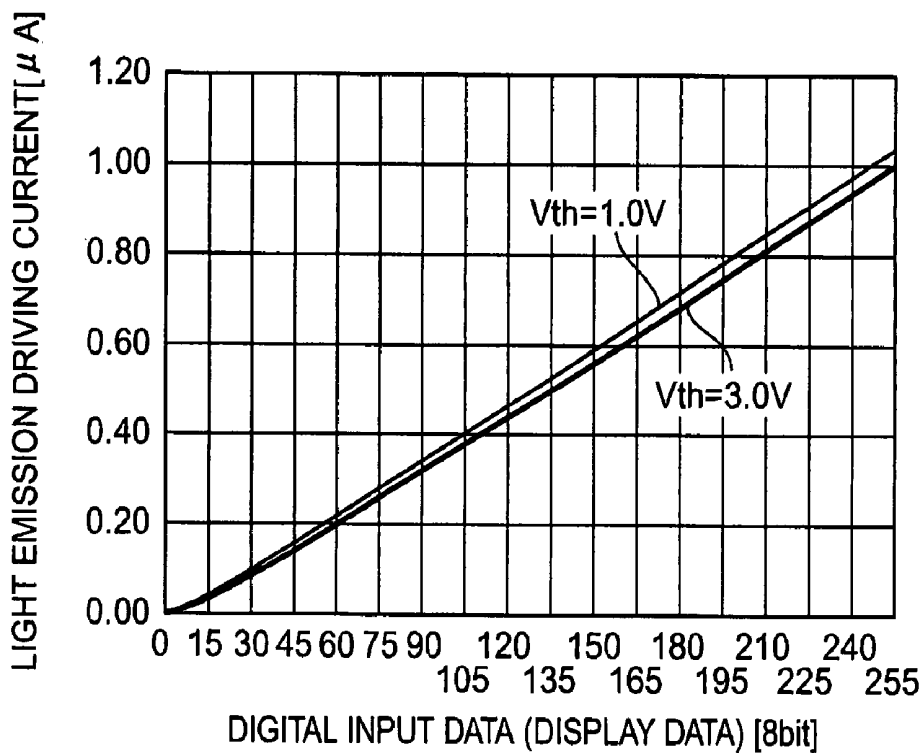


FIG. 39

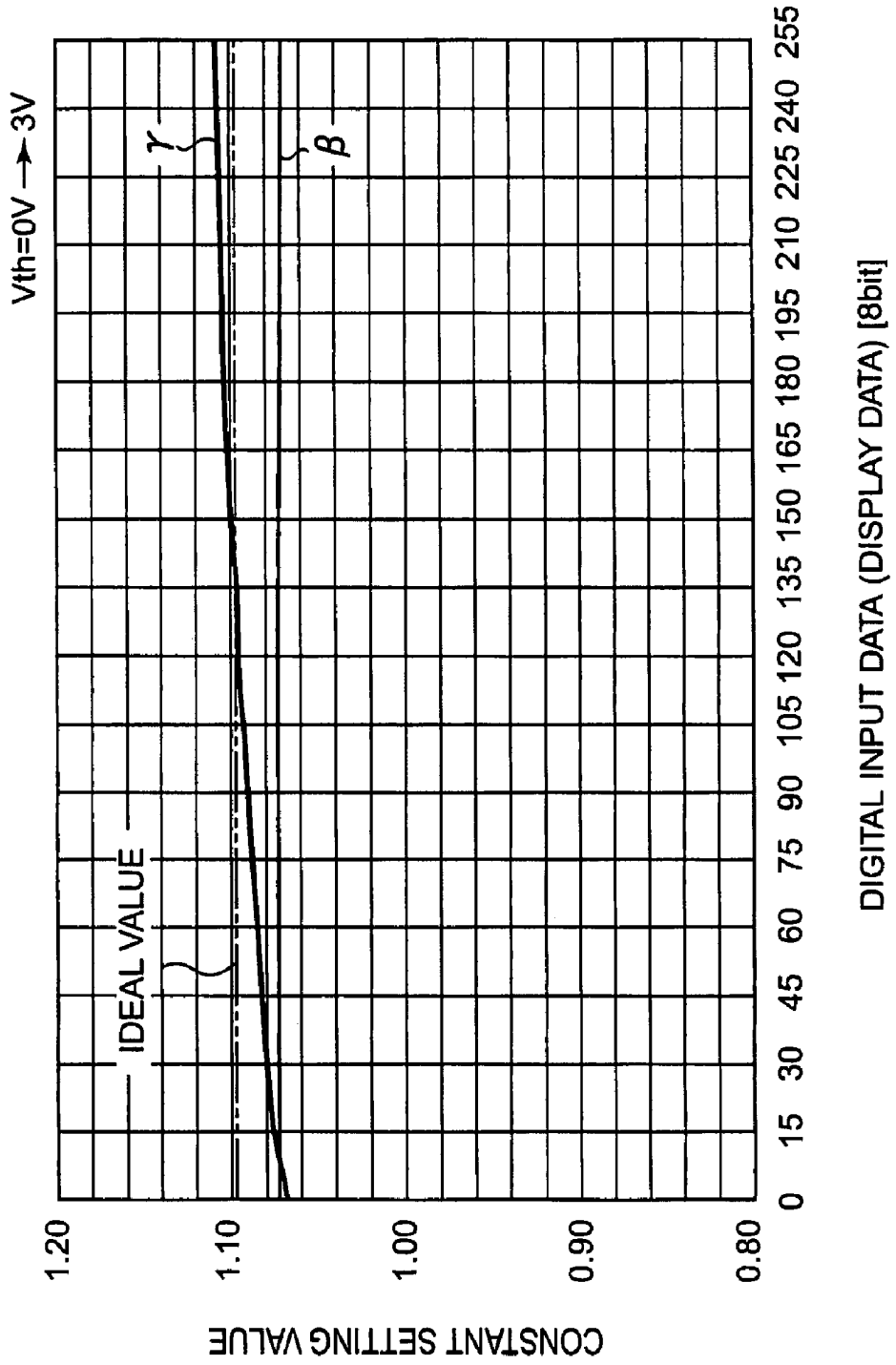


FIG. 40

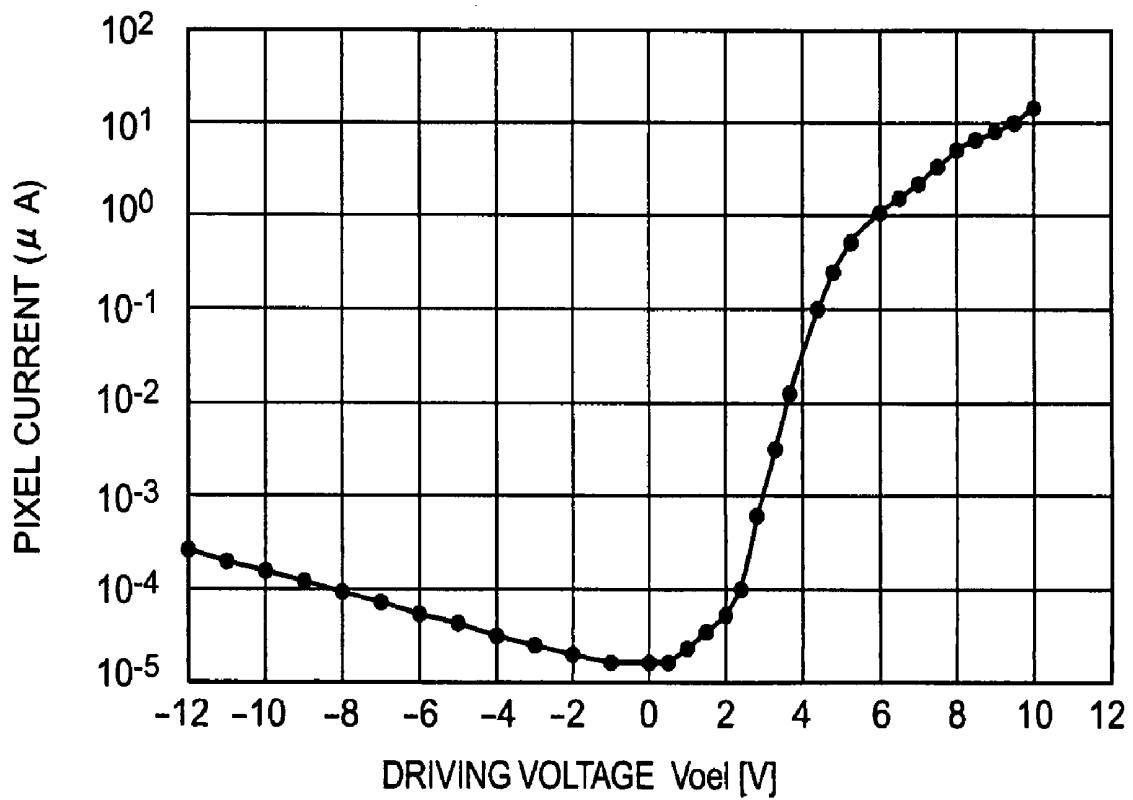
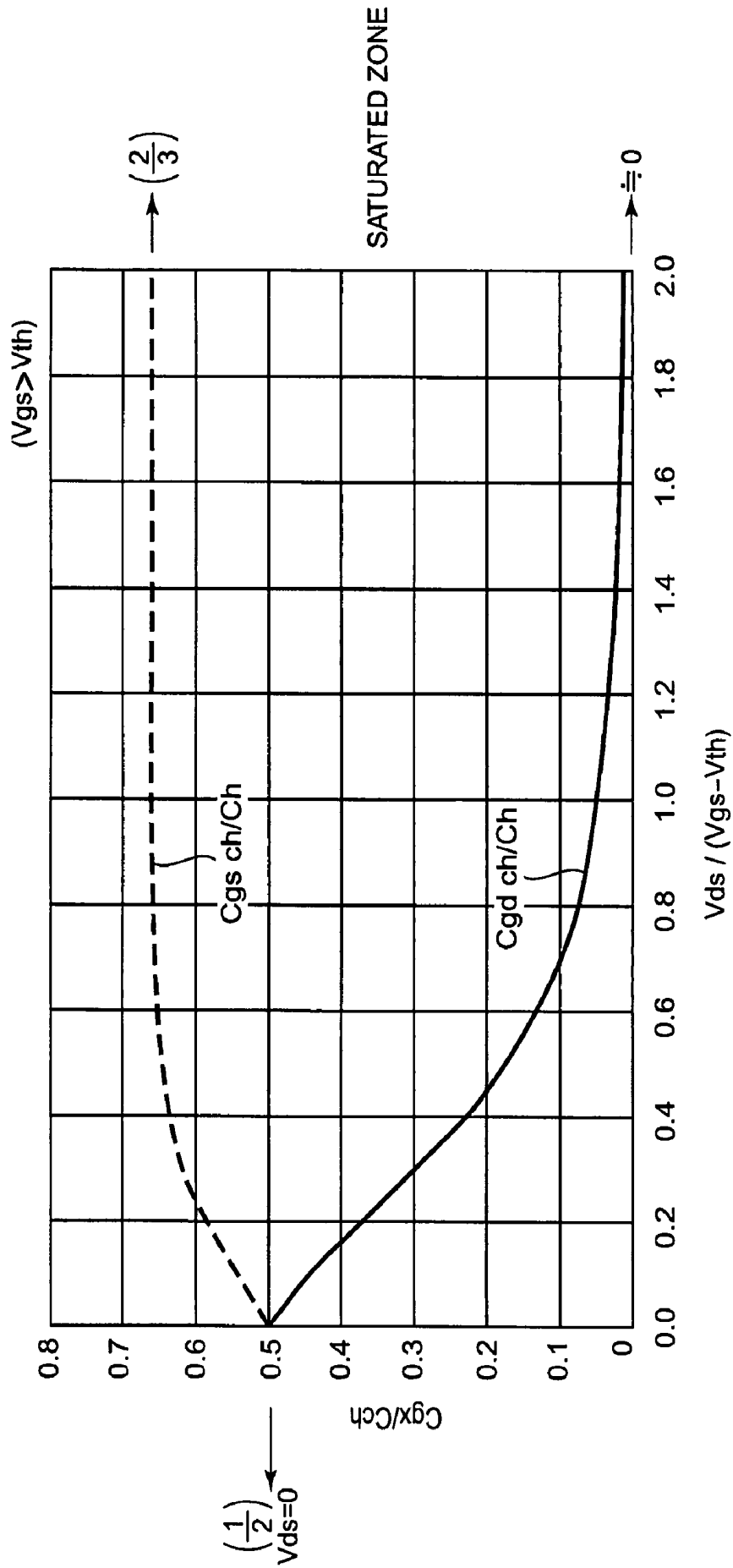


FIG. 41



**DISPLAY DRIVING APPARATUS AND
METHOD FOR DRIVING DISPLAY DRIVING
APPARATUS, AND DISPLAY APPARATUS
AND MTEHOD FOR DRIVING DISPLAY
APPARATUS**

CROSS REFERENCE TO RELATED
APPLICATIONS

This application is based on and claims the benefit of priority of Japanese Patent Application No. 2006-258717 filed on Sep. 25, 2006, and Japanese Patent Application No. 2007-078963 filed on Mar. 26, 2007, the entire contents of both of which are incorporated herein by reference.

BACKGROUND OF THE INVENTION

1. Field of the Invention

The present invention relates to a display driving apparatus and a method for driving a display driving apparatus as well as a display apparatus and a method for driving a display apparatus.

2. Description of the Related Art

There exists a display apparatus that includes a display panel in which current driving-type light-emitting elements (e.g., organic electroluminescence (EL) elements, inorganic EL elements, light-emitting diodes (LED)) are arranged in a matrix manner.

For example, Unexamined Japanese Patent Application KOKAI Publication No. H8-330600 discloses an active matrix-type driving display apparatus that is current-controlled by a voltage signal. This driving display apparatus is structured so that a current control thin film transistor and a switching thin film transistor are provided for each pixel. The current control thin film transistor flows current in an organic EL element when a voltage signal corresponding to image data is applied to a gate, and the switching thin film transistor turns ON or OFF the supply of the voltage signal to the gate of the current control thin film transistor. The driving display apparatus disclosed by Unexamined Japanese Patent Application KOKAI Publication No. H 8-330600 controls the brightness when an organic EL element emits light by controlling a voltage value of the voltage signal applied to the gate of the current control thin film transistor.

However, a threshold voltage of a transistor generally varies as time passes. Thus, in the case of the driving display apparatus of Unexamined Japanese Patent Application KOKAI Publication No. H 8-330600, a threshold voltage of a current control thin film transistor for supplying current to an organic EL element varies as time passes, which causes a variation in a value of current flowing in the organic EL element. As a result, there is a risk that brightness during the light emission by the organic EL element may vary.

SUMMARY OF THE INVENTION

The present invention has been made in view of the above disadvantage. It is an objective of the invention to provide a display apparatus in which a light-emitting element displays an image with an appropriate gradation level even when variation is caused in a threshold voltage of a transistor for supplying light-emitting current to the light-emitting element.

In order to solve the above problems, a display apparatus according to the present invention includes:

a light-emitting element for emitting light with a gradation level depending on supplied current;

a pixel driving circuit for supplying, to the light-emitting element, current depending on a voltage applied via a data line;

a precharge voltage source for applying a predetermined precharge voltage to the pixel driving circuit via the data line;

a voltage reader for reading, after the application of the precharge voltage by the precharge voltage source, the voltage of the data line after a predetermined transient response period; and

a compensated gradation data signal generator for generating, based on the read voltage of the data line, a compensated gradation data signal having a voltage value corresponding to an element characteristic unique to the pixel driving circuit to apply the compensated gradation data signal to the pixel driving circuit.

In order to solve the above problems, a driving method is provided to cause the display apparatus of the present invention to perform the characteristic operation thereof.

In order to solve the above problems, a display driving apparatus according to the present invention includes:

a precharge voltage source for applying a predetermined precharge voltage to a pixel driving circuit connected to a light-emitting element via a data line;

a voltage reader for reading, after the application of the precharge voltage by the precharge voltage source, the voltage of the data line after a predetermined transient response period; and

a compensated gradation data signal generator for applying, based on the read voltage of the data line, a compensated gradation data signal having a voltage value corresponding to an element characteristic unique to the pixel driving circuit to apply the compensated gradation data signal to the pixel driving circuit.

In order to solve the above problems, a driving method is provided to cause the display apparatus of the present invention to perform the characteristic operation thereof.

According to the present invention, even when variation is caused in a threshold voltage of a transistor for supplying a light-emitting current to an organic EL element, the light-emitting element can emit light with desired brightness of gradation level.

BRIEF DESCRIPTION OF THE DRAWINGS

These objects and other objects and advantages of the present invention will become more apparent upon reading of the following detailed description and the accompanying drawings in which:

FIG. 1 illustrates the main structure of a display pixel used in a display apparatus according an embodiment of the present invention;

FIG. 2 illustrates a signal waveform in the respective operations of a display pixel;

FIG. 3A illustrates an operation status in a writing operation of a display pixel;

FIG. 3B illustrates an equivalent circuit in a writing operation of a display pixel;

FIG. 4A shows an example of an operating characteristic of a driving transistor in a writing operation of a display pixel;

FIG. 4B shows an example of a relation between the driving current of an organic EL element and a driving voltage in a writing operation;

FIG. 5A illustrates an operation status in a retention operation of a display pixel;

FIG. 5B illustrates an equivalent circuit in a retention operation of a display pixel;

FIG. 6 illustrates an operating characteristic of a driving transistor in a retention operation of a display pixel;

FIG. 7A illustrates an operation status in a light-emitting operation of a display pixel;

FIG. 7B illustrates an equivalent circuit in a light-emitting operation of a display pixel;

FIG. 8A shows an example of an operating characteristic of a driving transistor in a light-emitting operation of a display pixel;

FIG. 8B shows an example of a load characteristic of the organic EL element in a light-emitting operation;

FIG. 9 is a block diagram showing the structure of the display apparatus in Embodiment 1;

FIG. 10 shows the structure of the main part of the data driver and the display pixel (pixel driving circuit, light-emitting element) in Embodiment 1;

FIG. 11 shows the respective steps from a selection operation to a light-emitting operation;

FIG. 12 illustrates a timing chart in a driving control of the display apparatus;

FIG. 13 illustrates a timing diagram in the selection operation of the display apparatus;

FIG. 14 illustrates operation statuses of the data driver and the display pixel in the precharge operation;

FIG. 15 illustrates the operation statuses of the data driver and the display pixel in the reading operation of a reference voltage;

FIG. 16 illustrates the operation statuses of the data driver and the display pixel in the writing operation of the display apparatus;

FIG. 17 illustrates the operation statuses of the data driver and the display pixel in the retention operation of the display apparatus;

FIG. 18 illustrates the operation statuses of the data driver and the display pixel in the light-emitting operation of the display apparatus;

FIG. 19 shows an example of a voltage applied to the data line in the selection period;

FIG. 20 illustrates a relation between an elapsed time and a potential change of a source terminal of a driving transistor during a transient response period;

FIG. 21 illustrates a relation between a threshold voltage of a driving transistor and a difference to a reference voltage;

FIG. 22 shows an example of a circuit structure of a data driver;

FIG. 23 shows a characteristic when a digital voltage of a digital-analog converter used as a data driver is converted to an analog voltage;

FIG. 24 illustrates an operation timing in a method for driving a display apparatus including a display zone of this embodiment;

FIG. 25 illustrates the structure of the main part of a data driver and a display pixel of Embodiment 2 (pixel driving apparatus, light-emitting element);

FIG. 26A illustrates an equivalent circuit including a capacity component parasitic on the pixel driving circuit;

FIG. 26B illustrates an equivalent circuit corresponding to the capacity component Cs shown in FIG. 27A;

FIG. 27A illustrates an equivalent circuit in a writing operation of a display pixel in Embodiment 2;

FIG. 27B illustrates an equivalent circuit in a light-emitting operation of a display pixel in Embodiment 2;

FIG. 27C illustrates an equivalent circuit corresponding to the capacity component Cgd13' shown in FIG. 27B;

FIG. 27D illustrates an equivalent circuit corresponding to the capacity component Cs" shown in FIG. 27B;

FIG. 28A illustrates the first model for describing law of conservation of charge amount;

FIG. 28B illustrates the second model for describing law of conservation of charge amount;

FIG. 29A illustrates a model for describing a status in which charge is retained in a display pixel when a high level selection signal is applied thereto;

FIG. 29B illustrates a model for describing a status in which charge is retained in a display pixel when a low level selection signal is applied thereto;

FIG. 30A illustrates a voltage in the equivalent circuit in a selection step;

FIG. 30B illustrates a voltage in the equivalent circuit in a not-selected status switching step;

FIG. 31A illustrates a voltage change when the selection step (writing operation) shifts to the not-selected status;

FIG. 31B illustrates a voltage change in the not-selected status retention step;

FIG. 32A illustrates a voltage in the equivalent circuit of the not-selected status retention step;

FIG. 32B illustrates a voltage in the equivalent circuit of the power source voltage switching step;

FIG. 32C illustrates a voltage in the equivalent circuit of the light-emitting step;

FIG. 33 illustrates a voltage in the equivalent circuit during a writing operation;

FIG. 34 illustrates a relation between input data and a data voltage and an original gradation level voltage in a writing operation;

FIG. 35 illustrates a relation between input data and a compensated gradation level voltage and a threshold voltage in a writing operation;

FIG. 36A illustrates the first example of a relation between input data and a light emission driving current and a threshold voltage in a light-emitting operation;

FIG. 36B illustrates the second example of a relation between input data and a light emission driving current and a threshold voltage in a light-emitting operation;

FIG. 37A illustrates the first example of a relation between the input data and the light emission driving current and variation in the threshold voltage in a light-emitting operation;

FIG. 37B illustrates the second example of a relation between the input data and the light emission driving current and variation in the threshold voltage in a light-emitting operation;

FIG. 37C illustrates the third example of a relation between the input data and the light emission driving current and variation in the threshold voltage in a light-emitting operation;

FIG. 38A illustrates the first example of the relation between the input data and the light emission driving current and the threshold voltage when a "γ effect" is not provided;

FIG. 38B illustrates the second example of the relation between the input data and the light emission driving current and the threshold voltage when a "γ effect" is not provided;

FIG. 39 illustrates a relation between a constant and input data set to cause the effect of the present invention;

FIG. 40 illustrates a relation between a voltage and a current of the organic EL element used for a test for checking the effect of the present invention; and

FIG. 41 illustrates a relation between an in-channel parasitic capacitance and a voltage of a transistor used for a display pixel (pixel driving circuit).

DETAILED DESCRIPTION OF THE PREFERRED EMBODIMENTS

Hereinafter, a display apparatus and a display driving apparatus according to an embodiment of the present invention will be described. This embodiment is an example in which the display apparatus of the present invention is a display apparatus **1** using a current driving-type light-emitting element to display an image. This light-emitting element may be an arbitrary light-emitting element. However, the following will describe a case where the light-emitting element is an organic EL element.

First, a display pixel PIX of the display apparatus **1** of this embodiment will be described. As shown in FIG. 1, the display pixel PIX includes a pixel driving circuit DC and an organic EL element OLED. The pixel driving circuit DC has a transistor T1, a transistor T2, and a capacitor Cs. The transistor T1 and the transistor T2 may have arbitrary element structures and characteristics. However, the following will describe a case where the transistor T1 and the transistor T2 are n channel-type thin film transistors.

The transistor T1 is an n channel-type thin film transistor (hereinafter referred to as “driving transistor”) for driving the organic EL element OLED to emit light. The driving transistor T1 is structured so that a drain terminal is connected to a power source terminal TMv, a source terminal is connected to a contact point N2, and a gate terminal is connected to a contact point N1. This power source terminal TMv is applied with a power source voltage Vcc having different voltage values depending on an operation status of the pixel driving circuit DC.

The transistor T2 is an n channel-type thin film transistor that is hereinafter referred to as a “retention transistor”. The retention transistor T2 is structured so that a drain terminal is connected to the power source terminal TMv (a drain terminal of the driving transistor T1), a source terminal is connected to the contact point N1, and a gate terminal is connected to the control terminal TMh. The control terminal TMh is applied with a retention control signal Shld.

The capacitor Cs is connected between the gate terminal and the source terminal of the driving transistor T1 (between the contact point N1 and the contact point N2). The capacitor Cs may be parasitic capacitance formed between the gate and source terminals of the driving transistor T1 or also may be the parasitic capacitance connected with a capacitive element in parallel thereto.

The organic EL element OLED is an organic EL element that emits light with a gradation level depending on supplied current. The organic EL element OLED is structured so that an anode terminal is connected to the contact point N2 and a cathode terminal Tmc is applied with a reference voltage Vss. This reference voltage Vss has a fixed value. A data terminal Tmd is connected to the contact point N2 is applied with a data voltage Vdata corresponding to the gradation level value of display data.

Next, a method for controlling the display pixel PIX having the above structure will be described.

The pixel driving circuit DC applies a voltage corresponding to the gradation level value of display data to the capacitor Cs to charge the capacitor Cs (hereinafter referred to as a “writing operation”). After the writing operation, the capacitor Cs retains the written voltage (hereinafter referred to as a “retention operation”). Based on the charging voltage retained by the capacitor Cs, gradation level current corresponding to the gradation level of the display data flows in the organic EL element OLED and the organic EL element OLED emits light (hereinafter referred to as a “light-emitting

operation”). The brightness of the light emitted by the organic EL element OLED corresponds to the gradation level of the display data.

As shown in FIG. 2, the pixel driving circuit DC sequentially performs the above-described writing operation, retention operation, and light-emitting operation. The following will describe conditions required for the display pixel PIX to perform the respective operations.

(Writing Operation)

In the writing operation, the capacitor Cs is written with a voltage corresponding to the gradation level value of the display data. During the writing operation, the organic EL element OLED is in a light-off status in which the organic EL element OLED does not emit light. During the writing operation by the pixel driving circuit DC, the driving transistor T1 shows an operating characteristic illustrated in FIG. 4A,

In FIG. 4A, a characteristic line SPw, shown by a solid line, shows a relation between the drain-source voltage Vds and a drain-source current Ids in an initial state in which the n channel-type thin film transistor used as the driving transistor T1 is diode-connected. A point PMw on the characteristic line SPw is an operation point of the driving transistor T1. A characteristic line SPw2, shown by a broken line in FIG. 4A, shows a relation between the drain-source voltage Vds and the drain-source current Ids when the driving transistor T1 has a characteristic change due to its driving history. As shown in FIG. 4A, the drain-source voltage Vds is a sum of a threshold voltage Vth and a voltage Veff_gs, as shown in the following formula (1).

$$V_{ds} = V_{th} + V_{eff_gs} \quad (1)$$

When the drain-source voltage Vds exceeds the threshold voltage Vth (a threshold voltage between a gate and a source—a threshold voltage between a drain and a source), the drain-source current Ids nonlinearly increases with an increase of the drain-source voltage Vds as shown by the characteristic line SP2. Thus, Veff_gs in FIG. 4A represents a voltage effectively forming the drain-source current Ids.

During the writing operation shown in FIG. 2, the driving current and the driving voltage of the organic EL element OLED show the characteristic shown in FIG. 4B. In FIG. 4B, the characteristic line SPE shown by the solid line shows a relation, in an initial state, between a driving voltage Voled applied between an anode and a cathode of the organic EL element OLED and a driving current Ioled flowing between the anode and the cathode. When the driving voltage Voled exceeds the threshold voltage Vth_oled, the driving current Ioled nonlinearly increases with an increase of the driving voltage Voled as shown by the characteristic line SPE. In FIG. 4B, a characteristic line SPE2 represents an example of a relation between the driving voltage Voled and the driving current Ioled when the characteristic changes in accordance with the driving history of the organic EL element OLED.

As shown in FIG. 3A, during the writing operation, the control terminal TMh of the retention transistor T2 is applied with a retention control signal Shld of an ON-level (high level H) to turn ON the retention transistor T2. As a result, the connection (short-circuiting) between the gate and the drain of the driving transistor T1 is established to cause the driving transistor T1 to be in a diode-connected state. The power source terminal TMv is applied with the first power source voltage Vccw for a writing operation and the data terminal Tmd is applied with a data voltage Vdata corresponding to the gradation level value of the display data.

Then, the drain and source of the driving transistor T1 have therebetween current Ids corresponding to the potential dif-

ference between the drain and the source ($V_{ccw}-V_{data}$) (hereinafter referred to as “expected value current”). The data voltage V_{data} is set to include this expected value current I_{ds} as a voltage value required for obtaining a current value that is required for the organic EL element OLED to emit light with an appropriate brightness depending on the gradation level value of the display data. At this timing, as mentioned above short-circuiting is caused between the gate and the drain of the driving transistor T1 and the drain of the driving transistor T1 is in a diode-connected status. Thus, as shown in FIG. 3B, the drain-source voltage V_{ds} of the driving transistor T1 equals the gate-source voltage V_{gs} and is represented by the following formula (2). It is noted that the capacitor C_s is written (or charged) with this gate-source voltage V_{gs} .

$$V_{ds}=V_{gs}=V_{ccw}-V_{data} \quad (2)$$

Next, the first power source voltage V_{ccw} will be described. The driving transistor T1 is an n channel-type transistor. Thus, in order to flow the drain-source current I_{ds} of the driving transistor T1, the gate potential must be higher than the source potential (positive potential). As shown in FIG. 3B, the gate potential equals the drain potential (the first power source voltage V_{ccw}) and the source potential equals the data voltage V_{data} . Thus, to flow the drain-source current I_{ds} , the following formula (3) must be established.

$$V_{data}<V_{ccw} \quad (3)$$

In order for the organic EL element OLED to be in a light-off state, a difference between a voltage of the anode terminal of the organic EL element OLED and a voltage of the cathode terminal TMc must be equal to or less than the light-emitting threshold voltage V_{th_oled} of the organic EL element OLED. As shown in FIG. 3B, the contact point N2 is connected to the anode terminal of the organic EL element OLED. The contact point N2 is connected to the data terminal TMD and is applied with the data voltage V_{data} . On the other hand, the cathode terminal TMc is applied with the reference voltage V_{ss} having a fixed value.

Therefore, in order to cause the organic EL element OLED to be in a light-off state in the writing operation, a difference between the data voltage V_{data} and the reference voltage V_{ss} must be equal to or less than the light-emitting threshold voltage V_{th_oled} of the organic EL element OLED. In this case, the contact point N2 has the potential V_{data} ; therefore the following formula (4) must be satisfied in order for the organic EL element OLED to be in a light-off state during the writing operation. It is noted that, when the reference voltage V_{ss} is set to a ground potential of 0V, the formula (4) can be represented by the following formula (5).

$$V_{data}-V_{ss}\leq V_{th_oled} \quad (4)$$

$$V_{data}\leq V_{th_oled} \quad (5)$$

Thus, in order to cause the capacitor C_s to be written with the gate-source voltage V_{gs} of the driving transistor T1 and to cause the organic EL element OLED not to emit light during a writing operation, a relation shown in the following formula (6) based on the above-described formula (2) and formula (5) must be established.

$$V_{ccw}-V_{gs}\leq V_{th_oled} \quad (6)$$

Then, the relation of the formula (1) established for the gate-source voltage V_{gs} when the driving transistor Tr1 is diode-connected ($V_{gs}=V_{ds}=V_{th}+V_{eff_gs}$) is substituted into the formula (6) to provide the following formula (7).

$$V_{ccw}\leq V_{th_oled}+V_{th}+V_{eff_gs} \quad (7)$$

When voltage $V_{eff_gs}=0$ is established at which the drain-source current I_{ds} is formed, the formula (7) is represented by the following formula (8). As shown by this formula (8), during a writing operation, the first power source voltage V_{ccw} at a writing level must have a value that is equal to or lower than the sum of the light-emitting threshold voltage V_{th_oled} and the threshold voltage V_{th} of the driving transistor T1 (a gate-source threshold voltage=a drain-source threshold voltage).

$$V_{ccw}\leq V_{th_oled}+V_{th} \quad (8)$$

Generally, the characteristic of the driving transistor T1 of FIG. 4A and the characteristic of the organic EL element shown in FIG. 4B change in accordance with the driving history. The following will describe an influence of the change in the characteristic of the driving transistor T1 and the organic EL element OLED in accordance with the driving history in a writing operation.

First, the characteristic of the driving transistor T1 will be described. As shown in FIG. 4A, the threshold voltage V_{th} of the driving transistor T1 in the initial state increases in accordance with the driving history by a threshold voltage change amount ΔV_{th} . When the threshold voltage varies in accordance with the driving history, the characteristic line becomes a characteristic line SPw2 obtained by substantially translating the initial characteristic line SPw to a higher voltage side. In this case, in order to obtain gradation level current (drain-source current I_{ds}) in accordance with the gradation level value of the display data, the data voltage V_{data} must be increased by the threshold voltage change amount ΔV_{th} .

Next, the following will describe an influence of the change in the characteristic of the organic EL element OLED during a writing operation. Generally, the organic EL element has resistance that increases in accordance with the driving history. As shown in FIG. 4B, in the characteristic line SPe2 after a change in the resistance of the organic EL element OLED, a rate at which the driving current I_{oled} increases with regards to an increase in the driving voltage V_{oled} (increase rate) decreases when compared with the initial characteristic line SPe before the resistance change.

In order to allow the organic EL element OLED to emit light with an appropriate brightness depending on the gradation level value of the display data even when the resistance is high, the driving current I_{oled} in accordance with the gradation level value must be supplied to the organic EL element OLED. In order to supply such a driving current I_{oled} , the driving voltage V_{oled} must be increased by a difference between the voltage corresponding to the necessary driving current I_{oled} for the gradation level in the characteristic line SPe2 and the voltage corresponding to the necessary driving current I_{oled} for the gradation level in the characteristic line SPe. It is noted that this difference voltage reaches the maximum value ΔV_{oled_max} when the driving current I_{oled} is the maximum value I_{oled_max} . When the writing operation is completed to satisfy the above-described conditions, the display pixel PIX carries out a retention operation.

(Retention Operation)

During the retention operation, as shown in FIG. 5A, the control terminal TMh is applied with the retention control signal Shld of an OFF level (low level L). As a result, the retention transistor T2 is turned OFF to block electric connection between the gate and the drain of the driving transistor T1. Thus, the diode connection of the driving transistor T1 is cancelled to stop the charging of the capacitor C_s . As shown in FIG. 5B, the capacitor C_s retains the drain-source voltage V_{ds} of the driving transistor T1 (=gate-source voltage V_{gs}) charged during the writing operation.

The relation between the drain-source voltage V_{ds} and the drain-source current I_{ds} when the diode connection of the driving transistor T1 is cancelled follows the characteristic line S_{Ph} shown by the solid line in FIG. 6. The gate-source voltage V_{gs} in this case is maintained to have a fixed value (e.g., a value of a voltage retained by the capacitor C_s during the retention operation).

The characteristic line S_{Pw} in FIG. 6 is substantially the same as the characteristic line S_{Pw} during the writing operation shown in FIG. 4A and shows the characteristic when the driving transistor T1 is diode-connected. An intersecting point of the characteristic line S_{Ph} and the characteristic line S_{Pw} is at the operation point PM_h during the retention. The characteristic line S_{Po} in FIG. 6 is obtained by deducting the threshold voltage V_{th} from the voltages V_{gs} of the characteristic line S_{Pw} . At the intersecting point Po of the characteristic line S_{Po} and the characteristic line S_{Ph} , the drain-source voltage V_{ds} has a pinch-off voltage V_{po} .

When the driving transistor T1 operates in accordance with the characteristic line S_{Ph} , a zone within which the drain-source voltage V_{ds} changes from 0V to a pinch-off voltage V_{po} is an unsaturated zone. In the unsaturated zone, the drain-source current I_{ds} increases with an increase of the drain-source voltage V_{ds} . A zone within which the voltage V_{ds} is equal to or higher than the pinch-off voltage V_{po} is a saturated zone. In the saturated zone, there is substantially no change in the drain-source current I_{ds} even when the drain-source voltage V_{ds} increases.

It is noted that the retention control signal Sh_{ld} may be switched from an ON-level to an OFF level when the power source voltage V_{cc} is switched from the first power source voltage V_{ccw} for a writing operation to the second power source voltage V_{cce} for a light-emitting operation (when the retention operation is switched to the light-emitting operation). When the retention operation is completed in the manner described above, the display pixel PIX carries out a light-emitting operation.

(Light-Emitting Operation)

As shown in FIG. 7A, during a light-emitting operation, after the above-described retention operation, the diode connection of the driving transistor T1 remains cancelled. The power source terminal TM_v is applied with the second power source voltage V_{cce} for a light-emitting operation as the terminal voltage V_{cc} instead of the first power source voltage V_{ccw} for a writing operation. This second power source voltage V_{cce} has a higher potential than that of the first power source voltage V_{ccw} .

As a result, as shown in FIG. 7B, the current I_{ds} in accordance with the value of the gate-source voltage V_{gs} flows between the drain and source of the driving transistor T1. This current I_{ds} is supplied to the organic EL element OLED to allow the organic EL element OLED to emit light with a brightness in accordance with the value of the current I_{ds} . During the light-emitting operation, the current I_{ds} can be maintained at a fixed level by maintaining the gate-source voltage V_{gs} at a fixed level. Thus, a voltage retained by the capacitor C_s (a voltage applied to the capacitor C_s from a retention operation period to a light-emitting operation period) may be applied between the gate and the source for example.

During the light-emitting operation, when the gate-source voltage V_{gs} is fixed, the organic EL element OLED operates based on a load line S_{Pe} shown by the solid line in FIG. 8A. The load line S_{Pe} represents an inverted relation between the driving voltage V_{oled} and the driving current I_{oled} of the organic EL element OLED with regards to a value of a poten-

tial difference ($V_{cce}-V_{ss}$) between the power source terminal TM_v and the cathode terminal TM_c of the organic EL element OLED as reference. In FIG. 8A, the characteristic line S_{Ph} is substantially the same as the characteristic line S_{Ph} shown in FIG. 6 during the retention operation.

As shown in FIG. 8A, when processing proceeds from the retention operation to the light-emitting operation, the operation point of the driving transistor T1 moves from the operation point PM_h during the retention operation to an operation point PM_e during the light-emitting operation (an intersecting point during the retention operation of the characteristic line S_{Ph} and the load line S_{Pe} of the organic EL element OLED). As shown in FIG. 8A, this operation point PM_e is a point at which a potential difference ($V_{cce}-V_{ss}$) between the power source terminal TM_v and the cathode terminal TM_c of the organic EL element is distributed between the drain and the source of the driving transistor T1 and between the anode and the cathode of the organic EL element OLED. Specifically, at the operation point PM_e during the light-emitting operation, the voltage v_{ds} is applied between the drain and the source of the driving transistor T1 and the driving voltage V_{oled} is applied between the anode and the cathode of the organic EL element OLED as shown in FIG. 7B.

When the expected value current I_{ds} flowing between the drain and the source of the driving transistor T1 during the writing operation is equal to the driving current I_{oled} supplied to the organic EL element OLED during the light-emitting operation, the organic EL element OLED emits light having a brightness depending on the gradation level value of the display data. To realize this, the operation point PM_e of the driving transistor T1 during the light-emitting operation must be maintained within the saturated zone shown in FIG. 8A.

On the other hand, the driving voltage V_{oled} of the organic EL element OLED has the maximum value V_{oled_max} when the highest display gradation level is reached. Specifically, in order to allow the organic EL element OLED to emit light with brightness depending on the gradation level value of the display data, the second power source voltage V_{cce} for a light-emitting operation may be set to satisfy a relation shown in the following formula (9). It is noted that the left-hand side of the formula (9) represents a voltage applied between the above-described power source terminal TM_v and the cathode terminal TM_c of the organic EL element OLED. When the reference voltage V_{ss} applied to the cathode terminal of the organic EL element OLED is set to have the ground potential of 0V, the formula (9) can be represented by the following formula (10).

$$V_{cce}-V_{ss}\leq V_{po}+V_{oled_max} \quad (9)$$

$$V_{cce}\geq V_{po}+V_{oled_max} \quad (10)$$

Next, the following will describe an influence of a change in the characteristic of the organic EL element OLED during the light-emitting operation.

As shown in FIG. 4B, the organic EL element OLED has higher resistance in accordance with the driving history and as a result the increase rate of the driving current I_{oled} with respect to the driving voltage V_{oled} decreases. Then, the load line S_{Pe} of the organic EL element OLED more gently inclines as shown by S_{Pe2} and S_{Pe3} in FIG. 8B. Specifically, the load line of the organic EL element OLED changes in accordance with the driving history to cause a change in the load line from S_{Pe} through S_{Pe2} to S_{Pe3} . As a result, the operation point of the driving transistor T1 changes on the characteristic line S_{Ph} from PM_e through PM_e2 to PM_e3 .

When the operation point of the driving transistor T1 exists in the saturated zone (PM_e to PM_e2), the driving current I_{oled}

maintains a value of the expected value current I_{ds} during the writing operation. When the operation point exists in the unsaturated zone (when the operating point moves from P_{Me2} to P_{Me3} , for example) however, the driving current I_{oled} decreases and is lower than the expected value current I_{ds} during the writing operation. The decrease in the driving current I_{oled} causes the light-emitting element to emit light with a gradation level lower than the brightness corresponding to the gradation level value of the display data.

In the example of FIG. 8B, the pinch-off point P_o exists at a boundary between the unsaturated zone and the saturated zone. Thus, a potential difference between the operation point P_{Me} and the pinch-off point P_o during the light-emitting operation functions, when the organic EL element has higher resistance, as a compensation margin for maintaining a driving current I_{oled} during the light-emitting operation. In other words, a compensation margin corresponding to the current value of the driving current I_{oled} functions as a potential difference on the characteristic line SP_h between a pinch-off point trajectory SP_o and the load line SP_e of the organic EL element. It is noted that the compensation margin decreases with an increase of the driving current I_{oled} . The compensation margin increases when a voltage that is applied between the power source terminal TM_v and the cathode terminal TM_c of the organic EL element OLED ($V_{ce}-V_{ss}$) increases.

In the above-described illustrative embodiment, a transistor voltage is used to control brightness of the respective light-emitting elements (hereinafter referred to as “voltage gradation level control”). Then, the data voltage V_{data} is set based on initial characteristics of the previously determined transistor drain-source voltage V_{ds} and the drain-source current I_{ds} . However, the data voltage V_{data} set based on the method as described above causes an increase in the threshold voltage V_{th} in accordance with the driving history. Thus, the driving current supplied to the light-emitting element fails to correspond to the display data (data voltage) and thus the light-emitting element does not emit light with preferred brightness. When the transistor is an amorphous transistor in particular, the element characteristic remarkably varies.

In an n-channel-type amorphous silicon transistor, a driving history or temporal change causes carrier trap to a gate insulating film. This carrier trap offsets a gate field and the characteristic between the drain-source voltage V_{ds} and the drain-source current I_{ds} have an increased threshold voltage V_{th} . In the example of FIG. 4A, during the writing operation, the threshold voltage V_{th} shifts from the characteristic SP_w in an initial status to the characteristic SP_w2 at a higher voltage. When the drain-source voltage V_{ds} is fixed in this case, the drain-source current I_{ds} decreases and the light-emitting element has reduced brightness. It is noted that the amorphous transistor in the example shown in FIG. 4A is designed to have a gate insulating film thickness of 300 nm (3000 Å), a channel width of 500 μm , a channel length of 6.28 μm , and a threshold voltage of 2.4V.

When the element characteristic of the transistor varies, the threshold voltage V_{th} mainly increases. After the variation in the element characteristic, the characteristic line SP_w2 showing the relation between the drain-source voltage V_{ds} and the drain-source current I_{ds} is a substantial translation of the characteristic line SP_w in the initial state. Thus, a characteristic substantially corresponding to the varied characteristic line SP_w2 can be obtained by adding a fixed voltage (hereinafter referred to as “OFFSET voltage V_{ofst} ”) corresponding to the change amount ΔV_{th} of the initial threshold voltage V_{th} to the drain-source voltage V_{ds} of the initial characteristic line SP_w . Specifically, during an operation for writing the display data to the pixel driving circuit DC, the source termi-

nal of the driving transistor T1 (contact point N2) is applied with a voltage obtained by the drain-source voltage V_{ds} on the characteristic line SP_w with and an OFFSET voltage V_{ofst} (hereinafter referred to as “compensated gradation level voltage V_{pix} ”).

By doing this, a change in the element characteristic due to the variation in the threshold voltage V_{th} can be compensated. Specifically, the light emission driving current I_{em} having a value depending on display data can be supplied to the organic EL element OLED. The organic EL element OLED having received the light emission driving current I_{em} emits light with brightness in accordance with the display data.

Embodiment 1

The following section will describe the display apparatus 1 of Embodiment 1 for displaying an image by the above-described display pixel PIX. First, the structure of the display apparatus 1 will be described. As shown in FIG. 9, the display apparatus 1 includes: a display zone 11; a selection driver 12; a power source driver 13; a data driver (display driving apparatus) 14; a controller 15; a display signal generation circuit 16; and a display panel 17.

The display zone 11 includes: a plurality of selection lines L_s ; a plurality of data lines L_d ; and a plurality of display pixels PIX. The respective selection lines L_s are arranged in the row direction of the display zone 11 (left-and-right direction in FIG. 9). The respective selection lines L_s are parallel to one another. The respective data lines L_d are arranged in the column direction of the display zone 11 (up-and-down direction in FIG. 9). The respective data lines L_d are parallel to one another. The respective display pixels PIX are arranged in the vicinity of the respective intersecting points of the respective selection lines L_s and the respective data lines L_d and in a lattice-like manner in “n” rows \times “m” columns (n and m are a positive integer).

The selection driver 12 supplies a selection signal S_{sel} to the respective selection lines L_s with a predetermined timing. This selection signal S_{sel} is a signal for instructing the capacitor C_s with regards to the display pixel PIX to which a voltage corresponding to the gradation level value of the display data should be written. The selection driver 12 may be structured by any of an Integrated Circuit (IC) chip or a transistor.

The power source driver 13 supplies, with a predetermined timing, the power source voltage V_{cc} of the predetermined voltage level to a plurality of power source voltage lines L_v arranged in the selection line L_s in parallel with the selection line L_s .

The data driver (display driving apparatus) 14 applies, with a predetermined timing, the compensated gradation level voltage V_{pix} (e.g., $V_{pix}(i)$, $V_{pix}(i+1)$) to the respective data lines L_d .

The controller 15 generates, based on a timing signal supplied from the display signal generation circuit 16, a signal for controlling the operations of the respective members to supply the signal to the respective members. For example, the controller 15 supplies a selection control signal for controlling the operation of the selection driver 12, a power source control signal for controlling the operation of the power source driver 13, and a data control signal for controlling the operation of the data driver 14.

The display signal generation circuit 16 generates display data (data for brightness) based on a video signal inputted from the exterior of the display apparatus 1 to supply the display data to the data driver 14. The display signal generation circuit 16 also extracts, based on the generated display data, a timing signal (e.g., system clock) for displaying an

image in the display zone 11 to supply the timing signal to the controller 15. This timing signal also may be generated by the display signal generation circuit 16.

The display panel 17 is a board having thereon the display zone 11, the selection driver 12, and the data driver 14. This board also may have thereon the power source driver 13. The display panel 17 also may have thereon a part of the data driver 14 and the remaining part of the data driver may be provided at the exterior of the display panel 17. In this case, a part of the data driver 14 in the display panel 17 may include an IC chip or a transistor.

The display panel 17 has, at the center thereof, the display panel 17 in which the respective display pixels PIX are arranged in a lattice-like manner. The respective display pixels PIX are divided into a group positioned at an upper zone of the display zone 11 and a group positioned at a lower zone. The display pixels PIX included in each group are connected to branched power source voltage lines Lv, respectively. It is noted that the group at the upper zone in Embodiment 1 includes the first to (n/2)th display pixels PIX ("n" is an even number). The group at the lower zone includes the (n/2+1) to "n"th display pixels PIX.

The respective power source voltage lines Lv in the group at the upper zone are connected to the first power source voltage line Lv1. The respective power source voltage lines Lv in the group at the lower zone are connected to the second power source voltage line Lv2. The first power source voltage line Lv1 and the second power source voltage line Lv2 are connected to the power source driver 13 in an independent manner. Thus, the power source voltage Vcc is commonly applied to the first to (n/2)th display pixels PIX via the first power source voltage line Lv1. The (n/2+1) to "n"th display pixels PIX are commonly applied with the power source voltage Vcc via the second power source voltage line Lv2. The power source driver 13 applies the power source voltage Vcc via the first power source voltage line Lv1 at a timing different from a timing at which the power source driver 13 applies the power source voltage Vcc via the second power source voltage line Lv2.

The display pixel PIX shown in FIG. 9 includes, as shown in FIG. 10, the pixel driving circuit DC and the organic EL element OLED. The pixel driving circuit DC has a transistor Tr11, a selection transistor Tr12, a driving transistor Tr13, and a capacitor Cs. This transistor Tr11 corresponds to the retention transistor T2 shown in FIG. 1 and the driving transistor Tr13 corresponds to the driving transistor T1 shown in FIG. 1. It is noted that the respective transistors Tr11 to Tr13 may be an arbitrary type of transistor but the respective transistors Tr11 to Tr13 in the following description are all an n channel-type field effect-type transistor.

The retention transistor Tr11 is a transistor for diode connection of the driving transistor Tr13. The retention transistor Tr11 is structured so that a gate terminal is connected to the selection line Ls, a drain terminal is connected to the power source voltage line Lv, and a source terminal is connected to the contact point N11. The selection line Ls is applied with the selection signal Ssel. This selection signal Ssel is identical with the retention control signal Shld shown in FIG. 2.

The selection transistor Tr12 shown in FIG. 10 is structured so that a gate terminal is connected to the selection line Ls, a source terminal is connected to the data line Ld, and a drain terminal is connected to the contact point N12. This contact point N12 corresponds to the contact point N2 shown in FIG. 1. The driving transistor Tr13 is structured so that a gate terminal is connected to the contact point N11, a drain terminal is connected to the power source voltage line Lv, and a

source terminal is connected to the contact point N12. The contact point N11 corresponds to the contact point N1 shown in FIG. 1.

The capacitor Cs is identical as that shown in FIG. 1. The capacitor Cs shown in FIG. 10 is connected between the contact point N11 and the contact point N12 (between the gate and the source of the driving transistor Tr13). The organic EL element OLED is structured so that an anode terminal is connected to the contact point N12 and the cathode terminal TMc is applied with a fixed reference voltage Vss.

During the writing operation, the compensated gradation level voltage Vpix corresponding to the gradation level value of the display data is applied to the capacitor Cs in the pixel driving circuit DC. Then, the compensated gradation level voltage Vpix, the reference voltage Vss, and the power source voltage Vcc (Vcce) having a high potential applied to the power source voltage line Lv for a light-emitting operation satisfy the relations of the above-described formulae (3) to (10). Thus, during the writing operation, the organic EL element OLED is in a light-off status. It is noted that pixel driving circuit DC is not limited to the structure shown in FIG. 10 and also may have any structure so long as that structure has elements corresponding to the respective elements shown in FIG. 1 and has a current path of the driving transistor T1 that has thereon current driving-type light-emitting elements OLED arranged in series. The light-emitting element is not limited to the organic EL element OLED and also may be other current driving-type light-emitting element such as a light-emitting diode.

The selection driver 12 includes, for example, a shift register and an output circuit section (output buffer). The shift register sequentially outputs, based on the selection control signal from the controller 15, shift signals corresponding to selection lines Ls of the respective rows. The output circuit section converts the level of this shift signal to a predetermined selected level (high level H or low level L). After the conversion, the output circuit section sequentially outputs the converted shift signals to the selection lines Ls of the respective rows as the selection signals Ssel.

For example, during a selection period Tsel shown in FIG. 13 (a period including a precharge period Tpre, a transient response period Ttrs, and a writing period Twrt), the selection driver 12 supplies the selection signal Ssel of a high level to the selection lines Ls of the respective rows connected with the display pixels PIX. The selection driver 12 supplies the selection signal Ssel to the selection line Ls in each row with a predetermined timing to sequentially set the display pixel PIX in each row to a selected status. The selection driver 12 may include a transistor that is the same as those of the respective transistors Tr11 to Tr13 in the pixel driving circuit DC.

During the selection period Tse, the power source driver 13 applies, based on the power source control signal from the controller 15, the power source voltage Vcc of a low potential (=Vccw) to the respective power source voltage lines Lv. During the light-emitting period, the power source driver 13 applies the power source voltage Vcc of a high potential (=Vcce) to the respective power source voltage lines Lv. In the example of FIG. 9, the power source driver 13 applies, during the operation of the display pixels PIX included in the group at the upper zone, the power source voltage Vcc to these display pixels PIX via the first power source voltage line Lv1. The power source driver 13 also applies, during the operation of the display pixels PIX included in the group at the upper zone, the power source voltage Vcc to these display pixels PIX via the second power source voltage line Lv2.

The lower source driver **13** may include a timing generator and an output circuit section. The timing generator generates, based on a power source control signal from the controller **15**, timing signals corresponding to the respective power source voltage lines L_v . The timing generator is a shift register that sequentially outputs a shift signal for example. The output circuit section converts a timing signal to a predetermined voltage level (voltage values V_{ccw} and V_{ccw}) to apply the power source voltage V_{cc} suitable for this voltage level to the respective power source voltage lines L_v . When the number of the power source voltage lines L_v is small, the power source driver **13** may be provided in the controller **15** instead of the display panel **17**.

The data driver (display driving apparatus) **14** generates a signal voltage (original gradation level voltage V_{org}) corresponding to the display data (brightness corresponding to an emitting color) for each display pixel PIX supplied from the display signal generation circuit **16** for compensation. By the compensation of the original gradation level voltage V_{org} , the data driver **14** generates a compensated gradation level voltage V_{pix} corresponding to the element characteristic (threshold voltage) of the driving transistor Tr_{13} provided in each display pixel PIX. After the generation, the data driver **14** applies the compensated gradation level voltage V_{pix} to the respective display pixels PIX via the data line L_d .

As shown in FIG. **10**, the data driver **14** includes: a resistor **141**, a gradation level voltage generator **142**, a voltage converter **143**, a voltage calculator **144**, and changing-over switches SW_1 to SW_3 . The gradation level voltage generator **142**, the voltage calculator **144**, and the changing-over switches SW_1 to SW_3 are provided in the data line L_d of each column and are provided in a quantity of "m" in the entire data driver **14**.

A voltage reader **145** includes the voltage converter **143** and the changing-over switch SW_2 . The voltage converter **143** and the changing-over switch SW_2 are connected to the data line L_d . It is noted that wiring resistances and capacities from the data line L_d to the respective changing-over switches SW_1 to SW_3 are structured so as to be equal to one another. Thus, a voltage drop due to the data line L_d is substantially equal to any of the respective changing-over switches SW_1 to SW_3 .

The resistor **141** has a shift register and a data register. The shift register sequentially outputs a shift signal based on a data control signal from the controller **15**. The data register acquires, based on the outputted shift signal, data for brightness of the gradation level to transfer the data to the gradation level voltage generators **142** provided in the respective columns in a parallel manner. The data register acquires data for gradation level by acquiring data corresponding to the display pixels PIX in one row on the display zone **11**.

The gradation level voltage generator **142** generates and outputs the original gradation level voltage V_{org} . This original gradation level voltage V_{org} is a voltage that has a value corresponding to display data for each display pixel PIX and that shows brightness of the gradation level of each organic EL element OLED. It is noted that the original gradation level voltage V_{org} is applied between an anode and a cathode of the organic EL element OLED and thus does not depend on the threshold voltage V_{th} of the transistor Tr_{13} . When the driving transistor Tr_{13} operates based on the characteristic line SP_w shown in FIG. **4A**, the gradation level voltage generator **142** outputs, to the data line L_d , an absolute voltage value obtained by adding this original gradation level voltage V_{org} to the threshold voltage V_{th} ($V_{org}+V_{th}$). Then, by the potential difference between the power source voltage line L_v and the data line L_d , current for allowing the organic EL element

OLED to emit light with brightness depending on the display data flows in the transistor Tr_{13} .

During the writing operation, when current flows from the power source voltage line L_v to the data line L_d , the gradation level voltage generator **142** calculates a value obtained by multiplying, with -1 , a voltage having a sum of the original gradation level voltage V_{org} and the threshold voltage V_{th} to output the value. When current flows from the data line L_d to the power source voltage line L_v , the gradation level voltage generator **142** directly outputs the voltage having the sum of the original gradation level voltage V_{org} and the threshold voltage V_{th} without multiplying the voltage with a coefficient. It is noted that the original gradation level voltage V_{org} is set to have a higher voltage with an increase of gradation level of display data.

The gradation level voltage generator **142** also may include, for example, a Digital to Analogue Converter (DAC) and an output circuit. The DAC converts, based on a gradation level reference voltage supplied from a power supply section (not shown), a digital signal voltage of display data to an analog signal voltage. It is noted that this gradation level reference voltage is a reference voltage based on the values of gradation level. The output circuit outputs, with a predetermined timing, the analog signal voltage converted by the DAC as the original gradation level voltage V_{org} .

The voltage converter **143** applies the predetermined pre-charge voltage to the data line L_d . After the application, after a transient response period (natural relaxation period), the voltage of the capacitor C_s (reference voltage V_{ref}) is read via the data line L_d .

After the reading, the voltage converter **143** determines a coefficient a to estimate a threshold voltage of the transistor Tr_{13} after the characteristic variation. Next, the voltage converter **143** multiplies the coefficient a with the reference voltage V_{ref} to generate the first compensation voltage $a \cdot V_{ref}$ to output the first compensation voltage $a \cdot V_{ref}$ to the voltage calculator **144**.

In the example of FIG. **10**, current flowing in the data line L_d during the writing operation is set to flow from the data line L_d to the data driver **14**. Thus, the first compensation voltage $a \cdot V_{ref}$ is set so that $a \cdot V_{ref} < V_{ccw} - V_{th1} - V_{th2}$ is established. In this formula, V_{th1} represents a threshold voltage of the transistor Tr_{13} and V_{th2} represents a threshold voltage of the transistor Tr_{12} . Then, current flows from the power source voltage line L_v via the drain and source of the transistor Tr_{13} , the drain and source of the transistor Tr_{12} , and the data line L_d .

The voltage calculator **144** performs addition and subtraction of the original gradation level voltage V_{org} from the gradation level voltage generator **142**, the first compensation voltage $a \cdot V_{ref}$ from the voltage converter **143**, and the previously-set second compensation voltage V_{ofst} . When the gradation level voltage generator **142** includes the DAC, the addition and subtraction processings are performed for analog signals. It is noted that the second compensation voltage V_{ofst} is determined based on an output variation characteristic of the threshold voltage V_{th} of the transistor Tr_{13} for example. Next, the voltage calculator **144** outputs the voltage obtained by addition and subtraction as the compensated gradation level voltage V_{pix} to the data line L_d . During the writing operation, voltage calculator **144** determines the compensated gradation level voltage V_{pix} so as to satisfy the following formula (11) for example.

$$V_{pix} = a \cdot V_{ref} - V_{org} + V_{ofst} \quad (11)$$

The respective changing-over switches SW_1 to SW_3 switches ON and OFF based on the data control signal from

the controller 15, respectively. The changing-over switch SW1 turns ON or OFF the application by the voltage calculator 144 of the compensated gradation level voltage V_{pix} to the data line Ld. The changing-over switch SW2 turns ON or OFF an operation in which the voltage converter 143 reads a voltage of the data line Ld. The changing-over switch SW3 turns ON or OFF the application of the recharge voltage V_{pre} to the data line Ld.

The controller 15 controls the selection driver 12, the power source driver 13, and the data driver 14 to operate the respective drivers with a predetermined timing. The selection driver 12 sequentially sets the display pixel PIX to the selected status. The power source driver 13 applies the power source voltage V_{cc} to the respective power source voltage lines Lv. The data driver 14 applies the compensated gradation level voltage V_{pix} to the respective display pixels PIX.

The pixel driving circuits DC of the respective display pixels PIX performs a series of driving control operations under the control by the controller 15. This driving control operation including: a compensated gradation level voltage setting operation (precharge operation, transient response, reference voltage reading operation); a writing operation; a retention operation; and a light-emitting operation. By the driving control operation, the pixel driving circuit DC causes the display zone 11 to display image information based on a video signal.

The display signal generation circuit 16 extracts gradation level signals included in the video signal inputted from the exterior of the display apparatus 1. After the extraction, the display signal generation circuit 16 supplies the gradation data signals to the data driver 14 with regards to every one row of the display zone 11. When the video signal includes a timing signal defining the timing at which the image is to be displayed, the display signal generation circuit 16 may extract the timing signal to output the timing signal to the controller 15. Then, the controller 15 outputs the respective control signals to the respective drivers based on the timing defined by the timing signal.

(Method for Driving Display Apparatus)

Next, a method for driving the display apparatus 1 will be described. It is noted that the following section will represent the respective display pixels PIX placed at positions (i, j) on the display zone 11 (n rows x m columns) by display pixels PIX (i, j) ($1 \leq i \leq n$, $1 \leq j \leq m$).

As shown in FIG. 11, the method for driving the display apparatus 1 of Embodiment 1 including: a selection step, a not-selected status switching step, a not-selected status retention step, a power source voltage switching step, and a light-emitting step. The respective steps are operations carried out in the respective display pixels PIX so that the respective display pixels PIX in the entire display zone 11 independently perform the operations of the respective steps. This selection step is a step for carrying out an operation shown in FIG. 13 (precharge operation, compensated gradation level voltage setting operation, writing operation). The not-selected status retention step is a step for performing the retention operation shown in FIG. 2. The light-emitting step is a step for performing the light-emitting operation shown in FIG. 2.

As shown in FIG. 12, the display apparatus 1 repeats a series of operations with a redetermined cycle period T_{cyc} . The cycle period T_{cyc} is a period required for one display pixel PIX to display one pixel of an image of one frame for example. In Embodiment 1, the cycle period T_{cyc} is a period required for the display pixels PIX for one row to display an image of one row of video frames.

First, in the compensation period T_{det} in the selection period T_{sel} , a precharge operation is performed. In the precharge operation, the voltage converter 143 applies the redetermined precharge voltage V_{pre} to data line Ld of the respective columns. As a result, the precharge current I_{pre} from the power source voltage line Lv flows in the respective rows to the data line Ld. Thereafter, as shown in FIG. 13, the changing-over switch SW3 is turned OFF and the application of the precharge voltage V_{pre} by the voltage converter 143 is stopped. As a result, the precharge operation is completed. It is noted that a timing at which the application of the precharge voltage V_{pre} is completed is included in the compensation period T_{det} .

When the read timing $t1$ shown in FIG. 13 has passed since the stoppage of the application of the precharge voltage V_{pre} , the voltage converter 143 reads a reference voltage $V_{ref}(t1)$.

In the compensated gradation level voltage setting operation, the gradation level voltage generator 142 generates the original gradation level voltage V_{org} corresponding to the display data supplied from the display signal generation circuit 16. The voltage calculator 144 compensates the original gradation level voltage V_{org} generated by the gradation level voltage generator 142 to generate the compensated gradation level voltage V_{pix} . When the voltage calculator 144 generates the compensated gradation level voltage V_{pix} , the compensated gradation level voltage setting operation is completed. Thereafter, the writing operation is performed.

In the writing operation, the voltage calculator 144 applies the compensated gradation level voltage V_{pix} to the respective data lines Ld. As a result, the writing current (the drain-source current I_{ds} of the transistor Tr13) flows in the capacitor Cs.

In the retention operation, a voltage depending on the written compensated gradation level voltage V_{pix} (charge enough to flow writing current) written by a writing operation between the gate and the source of the transistor Tr13 is charged in the capacitor Cs and is retained. Hereinafter, a period during which the retention operation is performed will be referred to as a "retention period T_{hld} ".

In the light-emitting operation, as shown in FIG. 12, based on the charging voltage retained by the capacitor Cs, the light emission driving current I_{em} (e.g., $I_{em}(i)$, $I_{em}(i+1)$) is supplied to the organic EL element OLED. The organic EL element OLED emits light with gradation level depending on display data. Hereinafter, a period during which the light-emitting operation is performed will be referred to as a "light-emitting period T_{em} ". During the light-emitting period T_{em} , the light emission driving current I_{em} desirably equals to the drain-source current I_{ds} of the transistor Tr13.

Hereinafter, the respective operations during the above-described selection operation will be described by an example of the display pixels PIX in the "i"th row. The reference voltage reading operation and the compensated gradation level voltage generation operation are performed during the election period T_{sel} for the display pixels PIX in the "i"th row now being processed.

As shown in FIG. 13, a period during which the precharge operation is performed during the compensation period T_{det} will be referred to as a "precharge period T_{pre} ". During this precharge period T_{pre} , the power source voltage line Lv is applied with the power source voltage V_{ccw} . The voltage converter 143 applies the predetermined precharge voltage V_{pre} to the respective data lines Ld. As a result, the drain-source current I_{ds} depending on the precharge voltage V_{pre} flows in the transistor Tr13 of the respective display pixels

PIX arranged in a specific row (e.g., the “i”th row). The capacitor Cs accumulates charge depending on the precharge voltage Vpre.

As shown in FIG. 13, when the precharge operation is completed, the display driving apparatus DC turns OFF the changing-over switch SW3 to stop the application of the precharge voltage Vpre. After the completion of the precharge operation, a transient response is started. Thus, a timing at which the precharge operation is completed will be hereinafter referred to as “transient response start timing t0”. Hereinafter, a period from the start of the transient response to the completion will be referred to as a “transient response period Ttrs”.

During the transient response period Ttrs, the data driver 14 performs the reference voltage reading operation. After the time since the transient response start timing to has passed and the read timing t1 is reached, the voltage converter 143 reads, via data line Ld, the charging voltage of the capacitor Cs retained between the gate and the source of the transistor Tr13. The read charging voltage is the reference voltage Vref (t1) shown in FIG. 13.

Next, during the compensation period Tdet shown in FIG. 13, the pixel driving circuit DC performs the compensated gradation level voltage generation operation. In the compensated gradation level voltage generation operation, the voltage calculator 144 sets the compensated gradation level voltage Vpix based on the reference voltage Vref(t1).

As shown in FIG. 14, during the precharge period Tpre, the power source driver 13 applies the power source voltage Vcc of the writing operation level (=the first power source voltage Vccw ≤ reference voltage Vss) to the power source voltage line Lv connected to the display pixels PIX in the “i”th row. The selection driver 12 applies the selection signal Ssel of the selected level (high level) to the selection line Ls of the “i”th row. The display pixels PIX in the “i”th row are set to the selected status.

Then, in the respective display pixels PIX of the “i”th row, the respective transistors Tr11 are turned ON and the respective driving transistors Tr13 are in a diode-connected status. As a result, the power source voltage Vcc (=Vccw) is applied to the drain terminal and the gate terminal driving transistor Tr13 (contact point N11; one end of the capacitor Cs). The transistor Tr12 is also turned ON and the source terminal of the transistor Tr13 (contact point N12; the other end of the capacitor Cs) is electrically connected to the data lines Ld of the respective columns.

In synchronization with this timing, the controller 15 supplies a data control signal. As shown in FIG. 13, the data driver 14 turns OFF the changing-over switch SW1 to ON and turns ON the changing-over switches SW2 to SW3. As a result, the predetermined recharge voltage Vpre is applied to the respective capacitors Cs via the respective data lines Ld.

During the application of the precharge voltage Vpre, the maximum value of the threshold voltage of the driving transistor Tr13 after the variation in the element characteristic is a sum of the initial threshold voltage Vth0 and the maximum value ΔVth_max of the variation value ΔVth of the threshold voltage. The maximum value of the drain-source voltage of the transistor Tr12 is a sum of the initial drain-source voltage Vds12 and the maximum value ΔVds12_max of the variation value ΔVds 12 of the drain-source voltage Vds12 due to increased resistance of the transistor Tr12. It is also assumed that a voltage drop due to the selection transistor Tr12 shown in FIG. 14 and the wiring resistance from the power source voltage line Lv to the data line Ld except for the selection transistor Tr12 is Vvd. Then, the precharge voltage Vpre is set to satisfy the following formula (12). It is noted that the

potential difference (Vccw-Vpre) shown at the left-hand side of the formula (12) is a voltage applied to the selection transistor Tr12 and the driving transistor Tr13.

$$V_{ccw}-V_{pre} \geq (V_{th0}+\Delta V_{th_max})+(V_{ds12}+\Delta V_{ds12_max})+V_{vd} \quad (12)$$

The selection signal Ssel outputted to the selection line Ls is a positive voltage during the compensation period Tdet and is a negative voltage during periods other than the compensation period Tdet. Then, a voltage applied to the gate terminal of the transistor Tr12 is not remarkably close to the positive voltage. Thus, the maximum value ΔVds12_max of the variation value ΔVds12 the drain-source voltage is so small that the maximum value ΔVds12_max of can be ignored when compared with the maximum value ΔVth_max of the variation value ΔVth of the threshold voltage of the driving transistor Tr13. Thus, the formula (12) can be represented by the following formula (12a).

$$V_{ccw}-V_{pre} \geq (V_{th0}+\Delta V_{th_max})+V_{ds12}+V_{vd} \quad (12a)$$

Specifically, a voltage depending on the value of the precharge voltage Vpre is applied between both ends of the capacitor Cs (the gate and the source of the transistor Tr13). The voltage applied to the capacitor Cs is higher than the threshold voltage Vth after the variation in the element characteristic of the driving transistor Tr13. Thus, as shown in FIG. 14, the driving transistor Tr13 is turned ON to flow the precharge current Ipre depending on this voltage between the drain and the source of the transistor Tr13. Thus, both ends of the capacitor Cs immediately accumulates the charge based on this precharge current Ipre (voltage based on the precharge voltage Vpre).

The pixel driving apparatus DC owned by the display pixel PIX has a structure shown in FIG. 10. Thus, in order to flow the precharge current Ipre from the data line Ld in the data driver direction, the precharge voltage Vpre is set to have a negative potential to the power source voltage Vccw of the writing operation level (low level) Vpre < Vccw ≤ 0.

In the precharge operation, it is assumed that a signal applied to the source terminal of the transistor Tr13 is a current signal. In this case, a risk is caused where the wiring capacity and wiring resistance owned by the data line Ld and/or the capacity component included in the pixel driving apparatus DC may delay a change in a potential (charging voltage) in the capacitor Cs. However, the precharge voltage Vpre applied in Embodiment 1 is a voltage signal and thus the can be quickly charged with the capacitor Cs during the initial precharge period Tpre. Then, as shown in FIG. 13, the charging voltage of the capacitor Cs is rapidly close to the precharge voltage Vpre to subsequently gradually converge to the precharge voltage Vpre within the remaining period of the precharge period Tpre.

It is noted that, during the precharge period Tpre, the voltage of the precharge voltage Vpre applied to the anode terminal of the organic EL element OLED (contact point N12) is set to be lower than the reference voltage Vss applied to the cathode terminal TMc. The power source voltage Vccw is set to be equal to or lower than the reference voltage Vss. Thus, the organic EL element OLED is not in a positive bias status and thus has no current therein. Thus, during the precharge period Tpre, the organic EL element OLED does not emit light.

During the transient response period Ttrs after the precharge period Tpre (natural relaxation period), the data driver 14 maintains, as shown in FIG. 13, the changing-over switch SW1 in an OFF status and maintains the changing-over switch SW2 in an ON status. The data driver 14 switches the chang-

ing-over switch SW3 from ON to OFF. This blocks the application of the precharge voltage V_{pre} to the data line Ld and the display pixels PIX in the “i”th row in the selected status (pixel driving circuit DC).

Then, as shown in FIG. 15, the transistors Tr11 and Tr12 maintains an ON status. An electric connection between the pixel driving circuit DC and the data line Ld is maintained but an application of the voltage to the data line Ld is blocked. Thus, the other terminal side of the capacitor Cs (contact point N12) is set to have high impedance. The gate and the source of the transistor Tr13 (both ends of the capacitor Cs) have therebetween, by the above-described precharge operation, a potential difference that is equal to or higher than the threshold voltage after the variation of the transistor Tr13 ($V_{th0} + \Delta V_{th_max}$). Thus, as shown in FIG. 15, the transistor Tr13 maintains an ON status and a transient current Iref flows from the power source voltage line Lv via the transistor Tr13. During the transient response period Ttrs (natural relaxation period), as shown in FIG. 13, the source terminal side of the transistor Tr13 (contact point N12; the other end of the capacitor Cs) has a gradually-increasing potential toward the potential of the drain terminal side (power source voltage line Lv side). In accordance with this, the data line Ld electrically connected via the transistor Tr12 also has a gradually-increasing potential.

During the transient response period Ttrs, a part of the charge accumulated in the capacitor Cs is discharged. Thus, the gate-source voltage Vgs of the transistor Tr13 declines. Thus, the potential of the data line Ld changes from the precharge voltage V_{pre} to converge to the threshold voltage after the variation in the transistor Tr13 ($V_{th0} + \Delta V_{th}$). If the transient response period Ttrs is too long, the potential difference ($V_{ccw} - V(t)$) changes to converge to ($V_{th0} + \Delta V_{th}$). The mark “V(t)” represents a potential in the data line Ld changing with the time “t” and equals, as shown in FIG. 13, to the precharge voltage V_{pre} when the precharge period Tpre is completed. When the transient response period Ttrs is too long however, the selection period Tsel increases and thus the display characteristic (a video display characteristic in particular) remarkably deteriorates.

To prevent this, in Embodiment 1, the transient response period Ttrs is set so that the gate-source voltage Vgs of the transistor Tr13 is shorter than a period during which the potential converges to the threshold voltage after the variation ($V_{th} + \Delta V_{th}$). The transient response period Ttrs is suitably set so that the pixel driving circuit DC can perform the precharge operation and the writing operation during the selection period Tsel. Specifically, a timing at which the transient response period Ttrs is completed (reference voltage read timing) is set to a specific timing in a status in which the gate-source voltage Vgs of the transistor Tr13 is changing. It is noted that the organic EL element OLED does not emit light even during the transient response period Ttrs. The reason is that a value of a voltage applied to the contact point N12 at the anode terminal side of the organic EL element OLED is lower than the reference voltage Vss applied to the cathode terminal Tmc and thus a positive bias status is not provided.

Next, the reference voltage reading operation will be described. This reference voltage reading operation is identical with the operation shown in FIG. 13. Specifically, at the read timing t1, the voltage converter 143 reads the potential of the data line Ld (reference voltage Vref(t1)) connected thereto via the changing-over switch SW2 shown in FIG. 15. The reference voltage read timing t1 is a timing at which the transient response period Ttrs is completed. Specifically, the

transient response period Ttrs shown in FIG. 13 is equal to (the reference voltage read timing t1)–(transient response start timing t0).

As shown in FIG. 15, the data line Ld is connected to the source terminal (contact point N12) of the driving transistor Tr13 via the selection transistor Tr12 set to an ON status. The reference voltage Vref(t1) read by the voltage converter 143 is a function of the time “t” and is determined based on a voltage corresponding to the gate-source voltage Vgs of the transistor Tr13.

During the transient response period Ttrs, this voltage Vgs is different depending on the threshold voltage Vth of the transistor Tr13 or the threshold voltage after the variation ($V_{th0} + \Delta V_{th}$). Thus, the threshold voltage Vth or the threshold voltage after the variation ($V_{th0} + \Delta V_{th}$) can be substantially identified based on the change in the gate-source voltage Vgs. Then, with an increase of a variation amount ΔV_{th} of the threshold voltage, a ratio of the change in the gate-source voltage Vgs declines.

In the transistor Tr13, the variation amount ΔV_{th} increases with an increase of the variation of the threshold voltage Vth and the reference voltage Vref(t1) also decreases. Thus, based on the reference voltage Vref(t1), the threshold voltage Vth or the threshold voltage after the variation ($V_{th0} + \Delta V_{th}$) of the transistor Tr13 can be identified.

The reference voltage Vcan be represented by the following (13). It is noted that Vgs(t0) shown in the formula (13) represents a gate-source voltage of the transistor Tr13 at the read timing t1(t1). The mark “VR” represents a sum of the voltage drop Vds12 due to the source-drain resistance of the transistor Tr12 and a voltage drop due to the wiring resistance Vvd.

$$V_{ccw} - V_{ref}(t) = V_{gs}(t) + VR \quad (13)$$

Specifically, during a period from an arbitrary timing (t0) during the transient response period Ttrs to a timing (t1) at which the transient response period Ttrs is completed, a potential change in the data line Ld ($V_{ref}(t1) - V_{ref}(t0)$) depends on a change in the gate-source voltage of transistor Tr13 ($V_{gs}(t1) - V_{gs}(t0)$). The threshold voltage Vth of the transistor Tr13 is identified based on this change amount.

The voltage converter 143 retains the read reference voltage Vref(t1) via a buffer. Then, the voltage converter 143 inversely amplifies the reference voltage Vref to convert the voltage level to output the result as “the first compensation voltage a-Vref”. Then, the reference voltage reading operation is completed and the pixel driving circuit DC performs an operation for writing display data.

Next, this writing operation will be described. During the writing operation, the controller 15 supplies a data control signal to the changing-over switches SW1 to SW3 included in the voltage reader 145 shown in FIG. 10. As a result, as shown in FIG. 16, the changing-over switch SW1 is turned ON and the changing-over switches SW2 to SW3 are turned OFF. This provides an electric connection between the data line Ld and the voltage calculator 144. The power source driver 13 outputs the first power source voltage Vccw for a writing operation.

Next, display data from the display signal generation circuit 16 shown in FIG. 9 is transferred, via the resistor 141, to the gradation level voltage generators 142 provided in the respective columns (the respective data lines Ld). The gradation level voltage generator 142 acquires, from the transferred display data, gradation level values of the display pixel PIX (display pixel PIX set to a selected status) to be subjected to

the writing operation. Then, the gradation level voltage generator **142** determines whether the gradation level values have the 0th gradation level or not.

When the gradation level values have the 0th gradation level, the gradation level voltage generator **142** outputs, to the voltage calculator **144**, a predetermined gradation level voltage (a gradation level voltage) V_{zero} for causing the organic EL element OLED to perform a no-light-emitting operation (or a black display operation). This black gradation level voltage V_{zero} is applied to the data line Ld via the changing-over switch SW1 shown in FIG. 16. Then, the voltage calculator **144** does not perform a compensation processing based on the reference voltage V_{ref} (compensation processing for compensating the variation of the threshold voltage V_{th} of the transistor Tr13). The black gradation level voltage V_{zero} is set to $(-V_{zero} < V_{th} - V_{ccw})$. Then, the diode-connected transistor Tr13 has the gate-source voltage $V_{gs}(=V_{ccw} - V_{zero})$ lower than the threshold voltage V_{th} or the threshold voltage after the variation $(V_{th0} + \Delta V_{th})$ to result in $V_{gs} < V_{th}$. It is noted that the black gradation level voltage V_{zero} suppresses the variation of the respective threshold voltages of the transistors Tr12 and Tr13 and thus $V_{zero} = V_{ccw}$ is desirably established.

On the other hand, when the gradation level values does not have the 0th gradation level, the gradation level voltage generator **142** generates the original gradation level voltage V_{org} having a voltage value suitable for the gradation level values to output the original gradation level voltage V_{org} to the voltage calculator **144**. The voltage calculator **144** uses the first compensation voltage $a \cdot V_{ref}$ shown in FIG. 16 outputted from the voltage converter **143** to compensate this original gradation level voltage V_{org} so as to have a voltage value suitable for the variation of the threshold voltage V_{th} of the transistor Tr13.

Then, the voltage calculator **144** calculates the compensated gradation level voltage V_{pix} so that the original gradation level voltage V_{org} , the first compensation voltage $a \cdot V_{ref}$, and the second compensation voltage V_{ofst} to satisfy the above-described formula (11). It is noted that the second compensation voltage V_{ofst} is calculated based on a variation characteristic of the threshold voltage V_{th} of the transistor Tr13 (a relation between the threshold voltage V_{th} and the reference voltage V_{ref}) for example. The original gradation level voltage V_{org} is a positive voltage having an increasing potential with an increase of the gradation level of the display data.

The voltage calculator **144** applies the generated compensated gradation level voltage V_{pix} to the data line Ld via the changing-over switch SW1. The coefficient a of the first compensation voltage $a \cdot V_{ref}$ is a positive value while the second compensation voltage V_{ofst} is a positive value depending on the design of the transistor Tr13 ($-V_{ofst} < 0$). The compensated gradation level voltage V_{pix} is set to have a relatively negative potential based on the power source voltage V_{cc} of a writing operation level ($=V_{ccw} \leq \text{reference voltage } V_{ss}$) as reference. Thus, the compensated gradation level voltage V_{pix} declines toward a negative potential with an increase of a gradation level (and the voltage signal has an increasing amplitude).

The source terminal (contact point N12) of the transistor Tr13 included in the display pixel PIX set to the selected status is applied, based on the compensation voltage $(a \cdot V_{ref} + V_{ofst})$ depending on the threshold voltage V_{th} or the threshold voltage after the variation $(V_{th0} + \Delta V_{th})$ of the transistor Tr13, with the compensated gradation level voltage V_{pix} for which the original gradation level voltage V_{org} is compensated. Thus, the voltage V_{gs} depending on the compensated

gradation level voltage V_{pix} is applied between the gate the source of the transistor Tr13 (both ends of the capacitor Cs). In the writing operation as described above, instead of flowing current suitable for display data in the gate terminal and the source terminal of the transistor Tr13 to set a voltage, a desired voltage is directly applied to the gate terminal and the source terminal. Thus, potentials of the respective terminals and contact points can be quickly set to a desired status.

It is noted that, during the writing period T_{wrt} , the compensated gradation level voltage V_{pix} applied to the anode terminal of the organic EL element OLED is set to be lower than the reference voltage V_{ss} applied to the cathode terminal TMc. Thus, the organic EL element OLED is in a reverse bias status and thus does not emit light. Then, the writing operation is completed and the display apparatus **1** performs a retention operation.

Next, this retention operation will be described. As shown in FIG. 12, during the retention period T_{hld} , the selection driver **12** applies the selection signal S_{sel} of a not-selected level (low level) to the selection line Ls of the "i"th row. As a result, the retention transistor Tr11 is turned OFF as shown in FIG. 17 to cancel the diode-connected status of the driving transistor Tr13. The selection signal S_{sel} of the not-selected level also turns OFF the selection transistor Tr12 shown in FIG. 17 to block an electric connection between the source terminal of the transistor Tr13 (contact point N12) and the data line Ld. Then, a voltage for which the threshold voltage V_{th} or the threshold voltage after the variation $(V_{th0} + \Delta V_{th})$ is compensated is retained between the gate and the source of the transistor Tr13 of the "i"th row (both ends of the capacitor Cs).

As shown in FIG. 12, during the retention period T_{hld} , the selection driver **12** applies the selection signal S_{sel} of the selected level (high level) to the selection line Ls of the (i+1)th row. As a result, the display pixel PIX of the (i+1)th row is set to the selected status. Thereafter, until the selection period T_{sel} of the final row for a single group is completed, the respective rows are subjected to the above-described compensated gradation level voltage setting operation and writing operation. Then, the selection driver **12** applies, with different timings, the selection signal S_{sel} of the selected level to the selection lines Ls of the respective rows. It is noted that, as shown in FIG. 24, the display pixels PIX of the respective rows for which the compensated gradation level voltage setting operation and the writing operation are already completed continuously perform the retention operation until the display pixels PIX of all rows are written with the compensated gradation level voltage V_{pix} (a voltage depending on the display data).

This retention operation is performed between the writing operation and the light-emitting operation when all display pixels PIX in the respective groups are driven and controlled to emit light simultaneously for example. In this case, as shown in FIG. 24, the retention periods T_{hld} are different for the respective rows. In the example of FIG. 17, the changing-over switches SW1 to SW3 are all OFF. However, as shown in FIG. 12, when the display pixels PIX in the "i"th row perform retention operation (the retention period T_{hld} of the "i"th row), the display pixels PIX after the (i+1)th row simultaneously perform the compensated gradation level voltage setting operation and the writing operation. Thus, the respective changing-over switches SW1 to SW3 are individually switching controlled at a predetermined timing during every selection period T_{sel} of the display pixels PIX of the respective rows. Then, the retention operation is completed and the display pixels PIX perform the light-emitting operation.

Next, this light-emitting operation will be described. As shown in FIG. 12, during the light-emitting operation (light-emitting period T_{em}), the selection driver 12 applies the selection signal S_{sel} of the not-selected level (low level) to the selection lines L_s of the respective rows (e.g., the “ i ”th row and the $(i+1)$ th row). As shown in FIG. 18, the power source driver 13 applies, to the power source voltage line L_v , the power source voltage V_{cc} of the light-emitting operation level (the second power source voltage V_{cce}). This second power source voltage V_{cce} is a positive voltage having a higher potential than that of the reference voltage V_{ss} ($V_{cce} > V_{ss}$).

The second power source voltage V_{cce} is set so that the potential difference ($V_{cce} - V_{ss}$) is higher than a sum of the saturated voltage of the transistor Tr13 (pinch-off voltage V_{po}) and the driving voltage V_{oled} of the organic EL element OLED. Thus, as shown in the examples shown in FIG. 7 and FIG. 8, the transistor Tr13 operates in a saturated zone. The anode of the organic EL element OLED (contact point N12) is applied with a positive voltage depending on the voltage written by the writing operation between the gate and the source of the transistor Tr13 ($V_{ccw} - V_{pix}$). On the other hand, the cathode terminal TMc is applied with the reference voltage V_{ss} (e.g., ground potential) and thus the organic EL element OLED is in a reverse bias status.

As shown in FIG. 18, the power source voltage line L_v flows the light emission driving current I_{em} via the transistor Tr13 into the organic EL element OLED. This light emission driving current I_{em} has a current value depending on the compensated gradation level voltage V_{pix} . Thus, the organic EL element emits light with desired brightness of the gradation level. It is noted that the organic EL element OLED continues a light-emitting operation in the next cycle period T_{cyc} until the power source driver 13 starts the application of the power source voltage V_{cc} of the writing operation level ($=V_{ccw}$).

(Method for Driving Display Apparatus)

Next, a method for driving the above-described display apparatus 1 will be described. An example of FIG. 19 shows a voltage change in the data line L_d . In this case, the respective transistors of the pixel driving circuit DC are an amorphous silicon transistor. The voltage and the power source voltage V_{cc} of the data line L_d are set so that current flowing in the pixel driving circuit DC is drawn into the data driver 14. The precharge voltage V_{pre} is set to $-10V$. The selection period T_{tr} is set to 35 μsec , the precharge period T_{pre} is set to 10 μsec , the transient response period T_{tr} is set to 15 μsec , and the writing period T_{wrt} is set to 10 μsec , respectively. This selection period $T_{tr} = 35 \mu\text{sec}$ corresponds to a selection period allocated to the respective scanning lines when the display zone 11 has 480 scanning lines (selection lines) and the frame rate is 60 fps.

In the driving control operation of the display apparatus 1, the precharge operation, the reference voltage reading operation, and the writing operation are sequentially performed during the selection period T_{sel} .

In the precharge operation, the data driver 14 turns ON the changing-over switch SW3. As a result, the data line L_d is applied with the precharge voltage V_{pre} of a negative voltage ($-10V$). Then, the data line voltage sharply declines as shown in FIG. 19. Thereafter, the data line voltage gradually converges to the precharge voltage V_{pre} in accordance with the wiring capacity of the data line L_d and a time constant due to the wiring resistance. By this change in the data line voltage, the gate-source voltage V_{gs} corresponding to the precharge voltage V_{pre} is applied between the gate and the source of the transistor Tr13 in a row set to the selected status.

Thereafter, at the transient response start timing to, the data driver 14 turns OFF the changing-over switch SW3. This blocks the application of the precharge voltage V_{pre} to the data line L_d and the impedance is increased. However, the gate-source voltage V_{gs} is retained between the gate and the source of the transistor Tr13 due to the charging voltage of the capacitor C_s . Thus, the transistor Tr13 maintains the ON status. Thus, the transient current I_{ds} flows between the drain and the source of the transistor Tr13.

While the transient current I_{ds} flowing therebetween, the potential of the drain-source voltage V_{ds} declines and the potential of the gate-source voltage V_{gs} equal to that of this voltage V_{ds} also declines. Then, the voltage V_{gs} changes toward the threshold voltage V_{th} or the threshold voltage after the variation ($V_{th0} + \Delta V_{th}$) of the transistor Tr13. Thus, the potential of the source terminal of the transistor Tr13 (contact point N12) gradually increases as time passes.

In the driving control operation of Embodiment 1, current flowing in the display pixel (pixel driving circuit) is drawn from the data line L_d into the data driver 14. Thus, the data line L_d is set to have a negative voltage lower than that of the power source voltage V_{cc} . In this case, the higher gate-source voltage V_{gs} the transistor Tr13 has, the higher threshold voltage V_{th} or threshold voltage after the variation ($V_{th0} + \Delta V_{th}$) the transistor Tr13 has, as shown in FIG. 19.

In the transient response status, the gate-source voltage V_{gs} of the transistor Tr13 increases, as time passes, toward the threshold voltage V_{th} or the threshold voltage after the variation ($V_{th0} + \Delta V_{th}$). Thereafter, this voltage V_{gs} changes to converge to the threshold voltage V_{th} as shown by the characteristic lines ST1 and ST2 shown in FIG. 20. The transient response period T_{tr} is set to be shorter than a period during which the voltage V_{gs} converges to the threshold voltage V_{th} .

Then, with regards to a change in the data line voltage per hour, an increase in the gate-source voltage V_{gs} is higher as the threshold voltage V_{th} has a lower absolute value. As the threshold voltage V_{th} has a higher absolute value, an increase in the gate-source voltage V_{gs} is lower. In the case of the threshold voltage $V_{th(L)}$ close to the initial status, the variation ΔV_{th} is small and thus an increase in the voltage V_{gs} significantly changes (characteristic line ST1). When the variation ΔV_{th} is large on the other hand, an increase in the voltage V_{gs} gently changes (characteristic line ST2). In the example of FIG. 20, the characteristic lines ST1 and ST2 are used to detect the reference voltage V_{ref} before the voltage V_{gs} converges to the threshold voltage V_{th} . After the detection, changes in the respective characteristic lines ST1 and ST2 can be identified to estimate, based on the changes thereof, the threshold voltages $V_{th(L)}$ and $V_{th(H)}$ as a converge voltage. As described above, the reference voltage V_{ref} is a function of the transient response period T_{tr} and the threshold voltage V_{th} of the transistor Tr13.

Next, the following section will describe a relation between the threshold voltage of the driving transistor Tr13 and the reference voltage V_{ref} . The following example will assume, as in the example shown in FIG. 19, that the precharge voltage V_{pre} is $-10V$. The transient response period T_{tr} is set to 15 μsec .

The transistor Tr13 is set to have, as a driving capability, a constant K for calculating the saturated current I_{ds} between the drain and the source ($=K \times (W/L) \times (V_{gs} - V_{th})^2$) of 7.5×10^{-9} and a ratio between the channel width W and the length L of 80/6.5. The resistance between the source and the drain of the selection transistor Tr12 is set to 13 $M\Omega$ and a pixel content $C_s + C_{pix}$ as a sum of the capacitor C_s and the pixel parasitic capacitance C_{pix} is set to 1 pF. The parasitic capaci-

tance C_{para} of the data line L_d is set to 10 pF and the wiring resistance R_{data} of the data line L_d is set to 10 k Ω .

In this case, the transistor Tr_{13} has a relation between the threshold voltage V_{th} (initial threshold voltage V_{th0} +threshold voltage change amount ΔV_{th}) and the reference voltage V_{ref} having a characteristic shown in FIG. 21. Specifically, the lower the threshold voltage V_{th} is, the higher the reference voltage V_{ref} is. The higher the threshold voltage V_{th} is, the lower the reference voltage V_{ref} is. This characteristic is substantially linear and thus a relation between the reference voltage V_{ref} and the threshold voltage V_{th} can be represented by a linear function $y=a\cdot x+b$ as shown by the following formula (14). This slope “a” is substantially equals to “a” shown in the above-described formula (11). In the example of FIG. 21, the value of “a” is substantially 2. V_{ofst} represents the threshold voltage V_{th} (theoretical value) when the reference voltage V_{ref} is 0 that is a unique voltage value set based on verify conditions.

$$V_{th} = -a \cdot V_{ref} - V_{ofst} \quad (14)$$

In the writing operation, the data line L_d is applied with the compensated gradation level voltage V_{pix} . As shown in FIG. 19, the data line voltage sharply increases to subsequently converge toward the compensated gradation level voltage V_{pix} . Thus, in a row set to the selected status, the gate-source voltage V_{gs} depending on the compensated gradation level voltage V_{pix} is retained between the gate and the source of the transistor Tr_{13} (both ends of the capacitor C_s). The voltage calculator 144 adds and subtracts the original gradation level voltage V_{org} , the first compensation voltage $a \cdot V_{ref}$, and the second compensation voltage V_{ofst} to generate this compensated gradation level voltage V_{pix} . The original gradation level voltage V_{org} is set to a voltage value depending on the display data (data for brightness and color) in an initial status. In the initial status, the threshold voltage V_{th} does not vary. Thus, the compensated gradation level voltage V_{pix} can be represented by the following formula (15).

$$V_{pix} = -(V_{org} + V_{th}) \quad (15)$$

When the formula (15) is substituted into the formula (14), the above-described formula (11) is obtained. The voltage calculator 144 can add and subtract the respective voltages based on the formula (11) to generate the compensated gradation level voltage V_{pix} having a value subjected to a compensation processing in accordance with the variation ΔV_{th} of the threshold voltage. When the organic EL element OLED does not emit light, it is preferred that the formula (15) is not used and the compensated gradation level voltage V_{pix} can be set to the power source voltage V_{cc} (=the second power source voltage V_{ce} of the light-emitting operation level).

Next, a specific structure of the data driver 14 for realizing the above-described method for driving a display apparatus will be described. As shown in FIG. 22, the data driver 14 mainly includes the gradation level voltage generator 142, the voltage converter 143, the voltage calculator 144, and the changing-over switches SW1 to SW3. The data line L_d has parasitic capacitance C_{para} and wiring resistance R_{data} .

The gradation level voltage generator 142 includes a digital-analog voltage converter V-DAC (hereinafter referred to as “DA converter”). In this embodiment, this DA converter V-DAC has a voltage conversion characteristic shown in FIG. 23. The DA converter V-DAC converts data for gradation level (digital signal) supplied from the display signal generation circuit 16 to an analog signal voltage. The converted analog signal voltage is the original gradation level voltage V_{org} . The DA converter V-DAC outputs this original gradation level voltage V_{org} to the voltage converter 143.

It is noted that, in the example of FIG. 23, the drain-source current I_{ds} of the transistor Tr_{13} substantially in proportional to a digital input gradation level. Thus, the organic EL element OLED has the light-emitting brightness substantially in proportional to the value of flowing current (or current density) and is displayed with gradation level linear with regard to the digital input.

The voltage converter 143 shown in FIG. 22 includes a plurality of voltage follower-type amplification circuits and a plurality of inverted amplification circuits. In the amplification circuit, a + side input terminal of an operational amplifier OP1 is connected to the data line L_d via the changing-over switch SW2. An output terminal of the operational amplifier OP1 is connected to a – side input terminal of the operational amplifier OP1.

In the inverted amplification circuit, the + side input terminal of the operational amplifier OP2 is connected to the reference voltage. The – side input terminal of the operational amplifier OP2 is connected, via the resistance R1, the output terminal of the operational amplifier OP1 and is connected, via the resistance R2, the output terminal of the operational amplifier OP2.

The amplification circuit having the operational amplifier OP1 retains the voltage level of a reference voltage V_{ref} . It is noted that the retention capacity C_f is a capacity to retain the voltage level of the reference voltage V_{ref} .

The inverted amplification circuit inverts the voltage polarity of the reference voltage V_{ref} . The inverted amplification circuit also amplifies, in accordance with a voltage amplification rate determined based on a ratio between the resistances R2 and R1 ($R2/R1$), the voltage ($-V_{ref}$) having an inverted polarity. The voltage [$-(R2/R1) \cdot V_{ref}$] obtained after the amplification is the above-described first compensation voltage. The ratio $R2/R1$ corresponds to the slope “a” shown in the formula (14). The inverted amplification circuit also outputs the first compensation voltage [$-(R2/R1) \cdot V_{ref}$] to the voltage calculator 144.

The voltage calculator 144 includes an adder circuit. This adder circuit has the operational amplifier OP3 shown in FIG. 22. The + side input terminal of the operational amplifier OP3 is applied with the reference voltage via the resistance R. This + side input terminal is connected to an external input terminal of the second compensation voltage V_{ofst} via another resistance R. On the other hand, the – side input terminal is connected to the output terminal of the operational amplifier OP2 via the resistance R. This side input terminal is connected to the DA converter V-DAC via another resistance R and is connected to the output terminal of the operational amplifier OP3 via another resistance R.

The voltage calculator 144 adds and subtracts the original gradation level voltage V_{org} , the first compensation voltage [$-(R2/R1) \cdot V_{ref}$] and the second compensation voltage V_{ofst} to generate the compensated gradation level voltage V_{pix} . The voltage calculator 144 outputs this compensated gradation level voltage V_{pix} to the data line L_d via the changing-over switch SW1.

The respective changing-over switches SW1 to SW3 include a transistor switch. The respective changing-over switches SW1 to SW3 are turned ON or OFF based on the data control signal supplied from the controller 15 (any of switching control signals OUT, REF, PRE). This turns ON or OFF the connection between the data driver 14 (the voltage calculator 144, the voltage converter 143, an external input terminal of the precharge voltage V_{pre}) and the data line L_d .

(Method for Driving Display Apparatus)

Next, a driving method that is characteristic for the display apparatus 1 will be described. As shown in FIG. 9, the respective display pixels PIX of Embodiment 1 are divided to a group provided at the upper zone of the display zone 11 and a group provided at the lower zone of the display zone 11. The display pixels PIX include in the respective groups are applied with independent power source voltages Vcc via different power source voltage lines Lv1 and Lv2, respectively. Thus, the display pixels PIX in a plurality of rows included in the respective groups simultaneously perform a light-emitting operation.

The following section will describe a timing at which the display pixels PIX operate in the driving method as described above. The following section will assume that the display zone 11 shown in FIG. 9 includes display pixels in 12 rows and the respective display pixels are divided to a group of the first to sixth rows (a group provided at the upper zone of the display zone 11) and a group of the seventh to twelfth rows (a group provided at the lower zone of the display zone 11). As shown in FIG. 24, first, the display pixels PIX of the respective rows are caused to sequentially perform the compensated gradation level voltage setting operation (precharge operation, transient response, reference voltage reading operation) and the writing operation. When the writing operation is completed, all display pixels PIX in the group are caused to simultaneously emit light with gradation level depending on the display data. This light-emitting operation is sequentially repeated for the respective groups. As a result, data for one screen is displayed on the display zone 11.

For example, the respective display pixels PIX of the group of the first to sixth rows are applied, via the first power source voltage line Lv1, with the power source voltage Vcc having a low potential (=Vccw). Then, the compensated gradation level voltage setting operation, the writing operation, and the retention operation are repeatedly performed for the respective rows starting from the first row to the sixth row. With regards to the display pixels PIX of the respective rows, the voltage calculator 144 acquires, from the voltage converter 143, the first compensation voltage $a \cdot V_{ref}$ corresponding the threshold voltage V_{th} of the driving transistor Tr13. The display pixels PIX are written with the compensated gradation level voltage Vpix. The display pixels PIX in a row for which the writing operation is completed are then subjected to the retention operation.

At a timing at which the writing operation to the display pixels PIX in the sixth row is completed, the power source driver 13 applies a high potential power source voltage Vcc (=Vcce) to the respective display pixels PIX via the first power source voltage line Lv1. As a result, based on gradation level depending on the display data (compensated gradation level voltage Vpix) written to the respective display pixels PIX, all display pixels PIX included in this group (the first to sixth rows) are caused to simultaneously emit light. The display pixels of this group continuously emit light until the display pixels PIX in the first row are set to the next compensated gradation level voltage Vpix. A period during which the display pixels of this group continuously emit light until the display pixels PIX in the first row are set to the next compensated gradation level voltage Vpix is the light-emitting period Tem of the first to sixth rows. It is noted that this driving method causes the display pixels PIX in the sixth row (the final row of the group of the upper zone) to emit light without performing the retention operation after the writing operation.

On the other hand, at a timing at which the writing operation to the respective display pixels PIX of the group of the

first to sixth rows is completed, the power source driver 13 applies the power source voltage Vcc (=Vccw) for the writing operation to the respective display pixels PIX in the group of the seventh to twelfth rows via the second power source voltage line Lv2. Then, operations substantially the same as the above-described operations for the group of the first to sixth rows (the compensated gradation level voltage setting operation, the writing operation, and the retention operation) are repeated for the respective rows starting from the seventh row to the twelfth row. It is noted that, during these operations, display pixels in the group of the first to sixth rows continuously emit light.

At a timing at which the writing operation to the display pixels PIX in the twelfth row is completed, the power source driver 13 applies the power source voltage Vcc (=Vcce) for the light-emitting operation to the respective display pixels PIX. As a result, the display pixels PIX in six rows of this group (the seventh to twelfth rows) are caused to emit light simultaneously. Then, at a timing at which the writing operation to the display pixels PIX in all rows of each group is completed, all display pixels PIX in the group can be caused to emit light simultaneously. During display pixels in the respective rows in each group are set with a compensated gradation level voltage and during the writing current Ids is flowing therein, the respective display pixels in the group can be controlled not to emit light.

In the example of FIG. 24, the display pixels PIX in twelve rows are divided to two groups and a control is performed by which the data driver 14 causes the respective groups to emit light with different timings. Thus, a ratio between one frame period Tfr and a period during which black display is caused by a no-light-emitting operation (hereinafter referred to as "black insertion rate") can be set to 50%. Generally, in order to allow a person to clearly visually recognize video without feeling indistinctiveness or blur, this black insertion rate should be 30% or more. Thus, this driving method can display data with a relatively favorable display picture quality.

It is noted that display pixels in the respective rows may be also divided to three or more groups instead of two groups. Rows included in the respective groups are not limited to continuous rows and also may be divided to a group of odd-numbered rows and a group of even-numbered rows. The power source voltage line Lv also may be connected to the respective rows instead of being connected to divided groups. In this case, the respective power source voltage lines can be independently applied with the power source voltage Vcc so that the display pixels PIX in the respective rows can individually emit light.

As described above, according to Embodiment 1 of the present invention, during the writing period Twrt of display data, the compensated gradation level voltage Vpix is directly applied between the gate and the source of the driving transistor Tr13 and a desired voltage is retained in the capacitor Cs. This compensated gradation level voltage Vpix has a voltage value for which the display data and the variation of the element characteristic of the driving transistor are compensated. As a result, the light emission driving current Iem flowing in the light-emitting element (organic EL element OLED) can be controlled based on the compensated gradation level voltage Vpix and the light-emitting element can emit light with desired brightness of the gradation level. Specifically, voltage specification (voltage application) can be used to control the display gradation level of the light-emitting element.

Thus, the gradation data signal depending on the display data (compensated gradation level voltage) can be written, within the predetermined selection period Tsel, to the respec-

tive display pixels in a quick and secure manner. In this manner, the display apparatus 1 of the present invention can suppress insufficient writing of display data and can allow display pixels to emit light with preferred gradation level depending on the display data.

It is noted that Embodiment 1 can use the voltage specification (voltage application) to control the display gradation level of the light-emitting element for any of a case where the display zone has a larger size, a case where the display zone has a smaller size, a case where data of a low gradation level is displayed, and a case where current flowing in display pixels in a small display zone is small. In this regard, the gradation level control method of the present invention is advantageous over a method for using current specification for flowing current depending on display data to perform a writing operation (or to retain a voltage depending on display data) to control a gradation level.

According to Embodiment 1, prior to writing display data to the pixel driving circuit DC owned by the display pixel PIX, the first compensation voltage is acquired for which the original gradation level voltage Vorg is compensated in accordance with the variation in the threshold voltage Vth of the driving transistor Tr13. Thereafter, the writing operation is used to generate a gradation data signal (compensated gradation level voltage Vpix) compensated based on this compensation voltage and an unique voltage value (the second compensation voltage) set based on the verify conditions to apply the gradation data signal to the light-emitting EL element OLED. As a result, the variation in the threshold voltage is compensated and the respective display pixels (light-emitting elements) emit light with appropriate brightness of the gradation level depending on the display data. This can suppress the dispersion of the light-emitting characteristics of the respective display pixels PIX.

gradation data signal According to Embodiment 1, a gradation data signal (compensated gradation data signal) outputted from the data driver 14 is a voltage signal. Thus, even when the transistor Tr13 has the drain-source current Ids having a small value during the writing operation, the gate-source voltage Vgs depending on this current Ids can be quickly set. This is different from a method for directly controlling the current value of the drain-source current Ids of the transistor Tr13 to control the gradation level of the pixel. Thus, during the selection period Tsel, the compensated gradation level voltage Vpix can be written between the gate and source of the transistor Tr13 and the capacitor Cs. This eliminates a need in the structure of the pixel driving circuit DC structure for a memorization means (e.g., frame memory) for storing compensation data for generating the compensated gradation level voltage Vpix for example.

According to the driving method of Embodiment 1, even when a plurality of display pixels have different threshold voltages Vth, the respective threshold voltages Vth are estimated based on the reference voltage Vref to compensate the respective threshold voltages Vth. As a result, a plurality of pixels can be caused to operate with an identical light-emitting characteristic (e.g., identical brightness). For example, it is assumed that the display pixel A has the transistor Tr13 having a threshold voltage Vth_A and the display pixel B has the transistor Tr13 having a threshold voltage Vth_B. Based on the formula (14), the threshold voltage of the driving transistor Tr13 is compensated. It is also assumed that current flowing between the drain and source of the respective display pixels is IA and IB. In the saturated zone, IA and IB are

represented by the following formulae (16) and (17), respectively. It is noted that "K" in the formulae (16) and (17) represents a coefficient.

$$IA=K\{(Vorg+Vth_A)-Vth_A\}^2=K\cdot\{Vorg\}^2 \quad (16)$$

$$IB=K\{(Vorg+Vth_B)-Vth_B\}^2=K\cdot\{Vorg\}^2 \quad (17)$$

As described above, this method can compensate not only an influence by the threshold voltage change amount ΔV_{th} of the driving transistor Tr13 but also an influence by the dispersion of threshold value characteristics among the respective transistors. Thus, according to Embodiment 1, even when the threshold voltage of the display pixel A is different from the threshold voltage of the display pixel B in an initial status in which there is substantially no variation ΔV_{th} in the threshold voltage Vth, variation in the threshold voltages of the respective driving transistors Tr13 owned by the respective display pixels is compensated to provide an uniform display characteristic.

Embodiment 2

In the voltage specification-type gradation level control method according to Embodiment 1, the original gradation level voltage Vorg is compensated based on the reference voltage Vref to generate the compensated gradation level voltage Vpix. Then, this compensated gradation level voltage Vpix is applied to the respective display pixels PIX. The gradation level control method shown in Embodiment 1 is based on an assumption that an influence by the capacity component parasitic on the display pixel PIX can be sufficiently suppressed by the capacitor Cs connected between the gate and the source of the driving transistor Tr13. This method is also based on an assumption that, even when the power source voltage Vcc is switched from the writing level to the light-emitting level, there is no variation in the writing voltage retained in the capacitor Cs.

However, a mobile electronic apparatus such as a mobile phone frequently requires a smaller panel size and a fine picture quality. Such a requirement may prevent the storage capacitor of the capacitor Cs from being set to be higher than the parasitic capacitance of the display pixel PIX. In this case, when variation is caused in a writing voltage charged in the capacitor Cs at the start of the light-emitting operation, this causes variation in the gate-source voltage Vgs of the driving transistor Tr13. This causes variation in the light emission driving current Iem to prevent the respective display pixels from emitting light with brightness depending on display data.

In order to avoid this problem, instead of using the compensated gradation level voltage Vpix to compensate the variation in the threshold voltage Vth of the driving transistor Tr13, a value of the light emission driving current Iem may be compensated. The following section will describe the display apparatus 1 of Embodiment 2 of the present invention for performing the operation as described above.

First, the structure of the display apparatus 1 of Embodiment 2 will be described. The display apparatus 1 of Embodiment 2 has the same basic structure as those shown in FIG. 9 and FIG. 10. Specifically, as shown in FIG. 25, the display pixel PIX of Embodiment 2 is substantially the same as that of Embodiment 1. The pixel driving circuit DC owned by the display pixel PIX includes: the driving transistor Tr13 connected to the light-emitting element OLED in series; the selection transistor Tr12; and the retention transistor Tr11 for diode connection of the driving transistor Tr13.

In Embodiment 2, the data driver (display driving apparatus) **14** has the structure shown in FIG. **25** instead of the structure shown in FIG. **10**.

As in Embodiment 1, the gradation level voltage generator **142** of Embodiment 2 generates the original gradation level voltage V_{org} to output the original gradation level voltage V_{org} . With regards to this original gradation level voltage V_{org} , the unique voltage characteristic of the pixel driving circuit (driving transistor Tr_{13}) is compensated in order to allow a light-emitting element to emit light with desired brightness of the gradation level.

The data driver **14** (display driving apparatus) includes, instead of the voltage converter **143** shown in FIG. **10**, an adder section (voltage reader) **146** and a converter **147**. The data driver **14** also includes, instead of the voltage calculator **144** shown in FIG. **10**, an inversion calculator (compensated gradation data signal generator) **148**. The data driver **14** also includes a changing-over switch **SW4**. It is noted that the adder section **146** and the changing-over switch **SW2** will be collectively called as “voltage reader **149**”. The combination of the adder section **146**, the converter **147**, the inversion calculator **148**, and the changing-over switch **SW4** is provided in an amount of “ m ” in the data line L_d of each column, respectively.

The adder section (voltage reader) **146** applies the predetermined precharge voltage V_{pre} to the data line L_d . After the predetermined transient response period T_{trs} (natural relaxation period), the adder section **146** reads the reference voltage V_{ref} . The adder section **146** outputs, to the converter **147**, a voltage ($V_{ref}+V_{ofst}$) obtained by adding a previously set OFFSET voltage V_{ofst} to the reference voltage V_{ref} .

The converter **147** multiplies the voltage ($V_{ref}+V_{ofst}$) outputted from the adder section **146** with the predetermined coefficient α . This coefficient α is used to estimate the threshold voltage V_{th} after the variation of the characteristic of the transistor Tr_{13} . After the multiplication, the converter **147** outputs the resultant voltage $\alpha(V_{ref}+V_{ofst})$ to the inversion calculator **148**. It is noted that the voltage $\alpha(V_{ref}+V_{ofst})$ generated by the converter **147** can be represented, as shown in the following formula (21), by a predetermined multiple β of the threshold voltage V_{th} . It is noted that the “ βV_{th} ” will be called as “compensation voltage” hereinafter.

$$\beta V_{th} = \alpha \cdot (V_{ref} + V_{ofst}) \quad (21)$$

The inversion calculator **148** adds the original gradation level voltage V_{org} from the gradation level voltage generator **142** to the compensation voltage βV_{th} from the converter **147** to generate the compensated gradation level voltage (compensated gradation data signal) V_{pix} . When the gradation level voltage generator **142** includes a DA converter at this stage, the inversion calculator **148** adds the original gradation level voltage V_{org} to the compensation voltage βV_{th} in the form of an analog signal. Then, the inversion calculator **148** charges the generated compensated gradation level voltage V_{pix} in the capacitor C_s via the data line L_d (writing operation). It is noted that Embodiment 2 also allows, in order to flow writing current from the data line L_d into the data driver **14** during the writing operation to the display pixel PIX , the inversion calculator **148** to set the compensated gradation level voltage V_{pix} to a negative polarity. Then, the compensated gradation level voltage V_{pix} is set to satisfy the following formula (22). It is noted that, in the formula (22), $\beta > 1$,

original gradation level voltage $V_{org} > 0$, and $V_{in} < 0$ are established.

$$V_{pix} = -V_{in} = -V_{org} - \beta V_{th} \quad (22)$$

The changing-over switch **SW4** is connected between the output terminal of the inversion calculator **148** and a power source terminal for applying the black gradation level voltage V_{zero} . It is noted that the changing-over switch **SW4** desirably has resistance and capacity equal to those of the respective changing-over switches **SW1** to **SW3**. The changing-over switch **SW4** is turned ON or OFF based on the data control signal from the controller **15**. Based on this, the changing-over switch **SW4** controls the application to the data line L_d of the black gradation level voltage V_{zero} .

When the gradation level are the 0th gradation level (or when the organic EL element **OLED** does not emit light), the gradation level voltage generator **142** does not output the original gradation level voltage V_{org} . Then, the black gradation level voltage V_{zero} is applied to the output terminal of the inversion calculator **148** via the changing-over switch **SW4**. The formula (22) can be represented by the following formula (23). Specifically, the display driving apparatus **14** of Embodiment 2 has the above-described structure to compensate the unique voltage characteristic of the pixel driving circuit (driving transistor Tr_{13}) and to generate the compensated gradation level voltage V_{pix} for causing the light-emitting element **OLED** to emit light with desired brightness of the gradation level voltage V_{pix} to the capacitor C_s .

$$V_{pix} = -V_{in} = V_{zero} \leq V_{th} \quad (23)$$

(Method for Driving Display Apparatus)

Next, a method for driving the display apparatus **1** of Embodiment 2 will be described. As in Embodiment 1, Embodiment 2 also firstly performs an operation for setting a compensated gradation level voltage. The adder section **146** applies the redetermined precharge voltage V_{pre} to the data lines L_d on the respective columns. As a result, the adder section **146** flows the precharge current I_{pre} from the power source voltage line L_v into the data lines L_d of the respective rows. Thereafter, the adder section **146** stops the application of the precharge voltage V_{pre} . After the stoppage, after the transient response period T_{trs} , the adder section **146** reads the reference voltage $V_{pre}(t_0)$. As in Embodiment 1, this transient response period T_{trs} is set to be shorter than a period during which the gate-source voltage V_{gs} of the transistor Tr_{13} converges to the threshold voltage after the variation ($V_{th} + \Delta V_{th}$).

Next, the inversion calculator **148** compensates the original gradation level voltage V_{org} based on the compensation voltage βV_{th} set based on the reference voltage V_{ref} . The inversion calculator **148** generates the compensated gradation level voltage V_{pix} shown in the formula (22) to apply the compensated gradation level voltage V_{pix} to the respective data lines L_d . Then, the writing current I_{wrt} based on this compensated gradation level voltage V_{pix} flows in the respective display pixels PIX . This writing current I_{wrt} corresponds to the drain-source current I_{ds} of the transistor Tr_{13} .

Thus, Embodiment 2 sets, in order to compensate the writing current I_{wrt} , the voltage V_{gs} so that gate-source voltage V_{gs} of the driving transistor Tr_{13} satisfy the following formula (24). In the formula (24), V_{d0} represents a voltage among the voltages V_{gs} applied to the gate and the source of the transistor Tr_{13} during the writing operation that changes in accordance with the specified gradation level (digital bit). In the formula (24), γV_{th} represents a voltage depending on the threshold voltage V_{th} . This V_{d0} corresponds to the first

compensation voltage and γV_{th} corresponds to the second compensation voltage. It is noted that the constant γ in the formula (24) is defined by the following formula (25).

$$V_{gs} = 0 - (-V_d) = V_d + \gamma V_{th} \quad (24)$$

$$\gamma = 1 + (C_{gs11} + C_{gd13}) / C_s \quad (25)$$

By satisfying the formula (24), Embodiment 2 can use the compensated gradation level voltage V_{pix} to compensate the light emission driving current I_{em} flowing from the transistor **Tr13** into the organic EL element OLED during the light-emitting operation. Embodiment 1 is different from Embodiment 2 in that the compensated gradation level voltage V_{pix} had compensated the variation in the threshold voltage V_{th} of the transistor **Tr13**. It is noted that C_{gs11} in the formula (25) is a parasitic capacitance between the contact point **N11** and the contact point **N13** as shown in FIG. 27A. C_{gd13} represents a parasitic capacitance between the contact point **N11** and the contact point **N14**, C_{para} represents a parasitic capacitance of the data line **Ld**, and C_{pix} represents a parasitic capacitance of the organic EL element OLED.

In the above-described a method for driving a display apparatus, the shift from a writing operation to a light-emitting operation causes the selection signal S_{sel} applied to the selection line **Ls** to be switched from the a high level to a low level and also causes the power source voltage V_{cc} applied to the power source voltage line **Lv** to be switched from a low level to a high level. This causes a risk of variation in the gate-source voltage (a voltage retained in the capacitor C_s) V_{gs} of the driving transistor **Tr13**. In Embodiment 2, this voltage V_{gs} is set to satisfy the formula (24) to compensate the writing current I_{wrt} .

Then, the gate-source voltage V_{gs} for specifying the light emission driving current I_{em} flowing in the organic EL element OLED during a light-emitting operation is introduced. It is noted that the following section assumes that the power source voltage $V_{cc} (=V_{ccw})$ during the writing operation is a ground potential GND. As shown in FIG. 27A, during the writing operation, the display pixel **PIX** is applied with the selection signal S_{sel} of the selected level (high level) ($=V_{sh}$) and the power source voltage $V_{cc} (=V_{ccw} = GND)$ for a writing operation. The inversion calculator **148** applies the compensated gradation level voltage $V_{pix} (= -V_{in})$ having a negative polarity lower than that of the power source voltage $V_{ccw} (=GND)$ to the display pixel **PIX**.

As a result, the transistor **Tr11** and selection transistor **Tr12** are turned ON and the gate of the driving transistor **Tr13** (contact point **N11**) is applied with the power source voltage $V_{ccw} (=GND)$ and the source (contact point **N12**) of the transistor **Tr13** is applied with the compensated gradation level voltage V_{pix} having a negative polarity. As a result, a potential difference is caused between the gate and the source of the transistor **Tr13** to turn ON the transistor **Tr13**. Then, the writing current I_{wrt} flows from the power source voltage line **Lv** applied with the power source voltage V_{ccw} into the data line **Ld**. The V_{gs} (writing voltage V_d) depending on the value of this writing current I_{wrt} is retained in the capacitor C_s formed between the gate and the source of the transistor **Tr13**.

It is noted that C_{gs11}' shown in FIG. 27A is an effective parasitic capacitance that is caused between the gate and the source of the transistor **Tr11** when the gate voltage (selection signal S_{sel}) of the transistor **Tr11** changes from a high level to a low level. C_{gd13} is a parasitic capacitance caused between the gate and the drain of the transistor **Tr13** when a source-drain voltage of the driving transistor **Tr13** is in a saturated zone.

On the other hand, as shown in FIG. 27B, during the light-emitting operation, the selection line **Ls** is applied with the selection signal S_{sel} of the voltage ($-V_{sl} < 0$) of the not-selected level (low level) and is applied with the power source voltage V_{cc} for light emission having a high potential ($=V_{cce}$; 12-15V for example). The selection transistor **Tr12** is turned OFF to block the application by the inversion calculator **148** of the compensated gradation level voltage $V_{pix} (= -V_{in})$ to the data line **Ld**.

By applying the election signal S_{sel} having the voltage V_{sel} to the selection line **Ls**, the transistor **Tr11** is turned OFF to block the application of the power source voltage V_{cc} to the gate of the transistor **Tr13** (contact point **N11**) and to block the application of the compensated gradation level voltage V_{pix} to the source of the transistor **Tr13** (contact point **N12**). Then, a potential difference ($0 - (-V_d) = V_d$) caused between the gate and the source of the transistor **Tr13** during a writing operation is retained in the capacitor C_s . Thus, the gate-source potential difference V_d is maintained and the transistor **Tr13** maintains an ON status. As a result, the light emission driving current I_{em} in accordance with the gate-source voltage $V_{gs} (=V_d)$ flows from the power source voltage line **Lv** to the organic EL element OLED. Then, the organic EL element OLED emits light with brightness depending on a value of this current I_{em} .

It is noted that a voltage V_{oel} at the contact point **N12** shown in FIG. 27B represents a voltage of the organic EL element OLED during the light-emitting operation (hereinafter referred to as "light-emitting voltage"). C_{gs11} is a parasitic capacitance caused between the gate and the source when the gate voltage of the transistor **Tr11** (selection signal S_{sel}) has a low level ($-V_{sl}$). It is noted that a relation between C_{gs11}' of FIG. 27A and C_{gs11} of FIG. 27B is represented by the following formula (26). It is noted that the voltage V_{sh1} in the formula (26) represents a potential difference ($V_{sh} - (-V_{sl})$) between the high level (V_{sh}) and the low level ($-V_{sl}$) of the selection signal S_{sel} .

$$C_{gs11}' = C_{gs11} + (1/2) \times C_{ch11} \times V_{sh} / V_{sh1} \quad (26)$$

At the shift from the writing operation to the light-emitting operation, the voltage levels of the selection signal S_{sel} and the power source voltage V_{cc} are switched. Then, during the writing operation, the voltage $V_{gs} (=V_d)$ retained between the gate and the source of the transistor **Tr13** varies in accordance with the formula (27). In the formula (27), c_{gd} , c_{gs} , and c_{gs}' represent values obtained by normalizing the respective parasitic capacitances C_{gd} , C_{gs} , and C_{gs}' by the capacity of the capacitor and $c_{gd} = C_{gd} / C_s$, $c_{gs} = C_{gs} / C_s$, and $c_{gs}' = C_{gs}' / C_s$ are established. It is noted that a characteristic according to which the voltage V_{gs} varies in accordance with a change in the voltage applied to the pixel driving circuit DC is called as "a voltage characteristic unique to the pixel driving circuit DC".

$$V_{gs} = \{ V_d - (c_{gs} + c_{gd}) \cdot V_{oel} \} / (1 + c_{gs} + c_{gd}) + (c_{gd} \cdot V_{cce} - c_{gs}' \cdot V_{sh1}) / (1 + c_{gs} + c_{gd}) \quad (27)$$

The formula (27) is introduced by applying "law of conservation of charge amount" before and after the switching of a control voltage (selection signal S_{sel} , power source voltage V_{cc}) applied to the pixel driving circuit DC. As shown in FIG. 28A and FIG. 28B, a voltage applied to one end of the capacity components (capacities **C1** and **C2**) connected in series is changed from V_1 to V_1' . Then, the charge amounts Q_1 and Q_2 of the respective capacity components before the change and the charge amounts Q_1' and Q_2' of the respective capacity components after the change can be represented by the following formulae (28a) to (28d).

$$Q1=C1(V1-V2) \tag{28a}$$

$$Q2=C2V2 \tag{28b}$$

$$Q1'=C1(V1'-V2') \tag{28c}$$

$$Q2'=C2V2' \tag{28d}$$

Based on the formulae (28a) to (28d), $-Q1+Q2=-Q1'+Q2'$ is calculated, the potentials $V2$ and $V2'$ at a connection point of the capacity components $C1$ and $C2$ is represented by the following formula (29).

$$V2=V2-\{C1/(C1+C2)\} \cdot (V1-V1') \tag{29}$$

Next, the following section will describe the potential $Vn11$ at the gate (contact point $N11$) of the transistor $Tr13$ when the relations shown in the above-described formulae (28a) to (28d) and (29) are applied to the display pixel PIX (the pixel driving circuit DC and the organic EL element $OLED$) and the selection signal $Ssel$ is switched.

In this case, the equivalent circuits shown in FIGS. 26, 28A, and 28B can be substituted by the equivalent circuits shown in FIGS. 29A and 30B. In the example of FIG. 29A, the selection line Ls is applied with the selection signal $Ssel$ of the selected level (high level voltage Vsh) and the power source voltage line Lv is applied with the power source voltage $Vcc(=Vccw)$ having a low potential. In the example of FIG. 29B, the selection line Ls is applied with the selection signal $Ssel$ of the not-selected level (low level voltage Vsl). The power source voltage line Lv is applied with the power source voltage $Vcc(=Vccw)$ having a low potential.

During the application of the selection signal $Ssel$ of the selected level (Vsh), charge amounts retained in the respective capacity components $Cgs11$, $Cgs11b$, $Cds13$, and $Cpix$ and the capacitor Cs shown in FIG. 29A are represented by the following formulae (30a) to (30d). When the selection signal $Ssel$ of the not-selected level (Vsl) is applied, charge amounts retained in the respective capacity components $Cgs11$, $Cgs11b$, $Cds13$, and $Cpix$ and capacitor Cs shown in FIG. 29B are represented by the following formulae (30e) to (30h). The capacity component $Cgs11b$ shown between the contact points $N11$ and $N13$ shown in FIG. 29B is the gate-source parasitic capacitance $Cgso11$ other than the in-channel capacity of the transistor $Tr11$. The capacity component $Cgs11b$ between the contact points $N11$ and $N13$ shown in FIG. 29A is a sum of a value of $(Cgs11=Cch11/2+Cgs11)$ obtained by multiplying the channel capacity $Cch11$ of the transistor $Tr11$ with $1/2$ and $Cgs11(=Cgso11)$.

$$Q1=0 \tag{30a}$$

$$Q2=Cs \cdot Vd \tag{30b}$$

$$Q3=-Cpix \cdot Vd \tag{30c}$$

$$Q4=Cgs11b \cdot Vsh \tag{30d}$$

$$Q1'=Cgd13 \cdot V1 \tag{30e}$$

$$Q2'=Cs \cdot (V-V1) \tag{30f}$$

$$Q3'=-Cpix \cdot V \tag{30g}$$

$$Q4'=Cgs11 \cdot Vsh \cdot (V1-Vsl) \tag{30h}$$

When the law of conservation of charge amount is applied in the examples of FIG. 9A and FIG. 29B, a relation of the respective charges at the contact point $N11$ and at the contact point $N12$ are represented by the following formulae (31a) and (31b).

$$-Q1+Q2-Q4=-Q1'+Q2'-Q4' \tag{31a}$$

$$-Q2+Q3=-Q2'+Q3' \tag{31b}$$

When the formulae (31a) to (31b) are applied to the above-described formula (30a) to (30d), the potential $Vn11$ at the contact point $N11$ and the potential $Vn12$ at the contact point $N12$ are represented by the following formulae (32a) and (32b). It is noted that $Cgs11'$ and D shown in the formulae (32a) and (32b) are defined by the following formulae (33a) and (33b), respectively.

$$Vn11=V1=-(Cgs11 \cdot Cpix+Cgs11' \cdot Cs) \cdot Vsh1/D \tag{32a}$$

$$Vn12=-V=-Vd-(Cgs11' \cdot Cs) \cdot Vsh1/D \tag{32b}$$

$$Cgs11'=Cgs11+(Cch11' \cdot Cs)/(2 \cdot Vsh1) \tag{33a}$$

$$D=Cgd13 \cdot Cpix+Cgd13 \cdot Cs+Cgs11 \cdot Cpix+Cgs11' \cdot Cs+C_s \cdot Cpix \tag{33b}$$

The following section will describe a case where the method for introducing the potential as described above are applied to the respective steps from the writing operation to the light-emitting operation according to Embodiment 2 and the method for driving the display apparatus 1 in Embodiment 2. The method for driving the display apparatus 1 of Embodiment 2 is identical as that shown in the example of FIG. 11 and includes a selection step, a not-selected status switching step, a not-selected status retention step, a power source voltage switching step, and a light-emitting step.

Specifically, in Embodiment 2, the selection step is a step to send the selection signal $Ssel$ of the selected level to the display pixel PIX to select the display pixel PIX to write a voltage in accordance with the display data to the capacitor Cs owned by the display pixel PIX . The not-selected status switching step is a step to cause the respective display pixels PIX selected in the selection step to be in a not-selected status. The not-selected status retention step is a step in which a capacitor Cs is retained in the capacitors Cs of the display pixels PIX caused to be in a not-selected status by the switching step. The power source voltage switching step is a step in which the power source voltage Vcc applied to the driving transistor $Tr13$ connected to the capacitor that has retained the charging voltage in the not-selected status is switched from the writing operation level (low potential) to the light-emitting operation level (high potential). The light-emitting step is a step in which a light-emitting element is caused to emit light with brightness depending on display data.

First, the following section will describe a voltage change at each point when the selection step shifts to the not-selected status switching step. Before the shift, as shown in FIG. 30A, the transistor $Tr11$ and the transistor $Tr12$ are ON by the application of the selection signal (Vsh) of a high potential and the writing current $Iwrt$ flows between the drain and the source of the transistor $Tr13$. The contact point $N11$ has a potential of $Vccw$ (ground potential) and the contact point $N12$ has a potential of $-Vd$.

When the selection signal $Ssel$ of the not-selected level is applied to the transistor $Tr11$ and is applied to the transistor $Tr12$ in this status, the transistor $Tr11$ and the transistor $Tr12$ are switched from ON to OFF as shown in FIG. 30B. It is defined that the contact point $N11$ after the switching has a potential of $-V1$ and the contact point $N12$ after the switching has a potential of $-V$. When the selection signal $Ssel$ is switched from a positive potential of high level (Vsh) to a negative potential of a low level ($-Vsl$), the gate-source voltage Vgs' of the driving transistor $Tr13$ changes by $-\Delta Vgs$ from Vd . Then, the voltage Vgs' after the switching (writing

voltage (i.e., a potential difference between the potential Vn11 of the contact point N11 and the potential Vn12 of the contact point N12)) is represented by the following formula (34).

$$V_{gs}' = V_{n11} - V_{n12} = -V_1 - (-V) = V - V_1 = V_d - (C_{gs11} \cdot C_{pix} / D) \cdot V_{sh1} = V_d - \Delta V_{gs} \quad (34)$$

This voltage shift ΔV_{gs} is represented by $C_{gs11} \cdot C_{pix} \cdot V_{sh1} / D$. The capacity component $C_{s'}$ between the contact points N11 and N12 at the not-selected switching step is a parasitic capacitance component formed at a part other than the gate-source capacity of the transistor Tr13. In the formulae (32a), (32b), (33a), and (33b), "Cs" is a sum of the capacity component $C_{s'}$, the gate-source voltage parasitic capacitance C_{gso13} other than the in-channel capacity of the transistor Tr13, and the in-channel gate-source capacity of the transistor Tr13 in the saturated zone. This in-channel gate-source capacity is $2/3$ of the channel capacity C_{ch1} of the transistor Tr13. Thus, C_s shown in formula (32a), (32b), (33a), (33b) can be calculated as shown below.

$$C_s = C_{s'} + C_{gso13} + (2/3) \cdot C_{ch13}$$

In the saturated zone, the in-channel gate-drain capacity can be assumed as 0. Thus, only C_{gd13} is a gate-drain capacity C_{gso13} other than the in-channel capacity of the transistor Tr13. In the formula (34), C_{gs11}' is a sum of the gate-source parasitic capacitance C_{gso11} other than the in-channel capacity of the transistor Tr11 and the in-channel gate-source capacity of the transistor Tr11 when $V_{ds}=0$. This in-channel gate-source capacity is an integration value of $1/2$ of the channel capacity C_{ch11} of the transistor Tr11 and a voltage ratio (V_{sh} / V_{sh1}) of the selection signal S_{sel} . Specifically, C_{gs11}' shown in formula (34) can be represented as shown below.

$$C_{gs11}' = C_{gso11} + C_{ch11} \cdot V_{sh} / 2V_{sh1}$$

Next, a voltage change in the step for retaining the not-selected status of the display pixel PIX (not-selected status retention step) will be described. As shown in FIG. 31A, when the selection step (writing operation) shifts to the not-selected status, the transistor Tr13 maintains an ON status based on the voltage V_{gs}' retained between the gate and the source (capacity component $C_{s'}$). Then, the contact point N12 has a potential lower than that of the power source voltage $V_{cc}(=V_{ccw})$ and the drain-source current I_{ds} flows in the transistor Tr13. As shown in FIG. 31B, the current I_{ds} flowing in the transistor Tr13 causes the potential at the contact point N12 to increase to 0.

The drain voltage and the source voltage change until there is no different between the drain voltage of the transistor Tr13 (the potential of the contact point N14) and the source voltage (the potential of the contact point N12). A time required for this change is dozen microseconds. The change in the source potential causes the gate potential V_1' of the transistor Tr13 to change from the formulae (32a), (32b), (33a), and (33b) to a relation shown in the following formula (35).

$$V_1' = \{C_s / (C_{gs11} + C_{gd13} + C_s'')\} \cdot V - \{(C_{gs11} + C_{gd13} + C_s) / (C_{gs11} + C_{gd13} + C_s'')\} \cdot V_1 \quad (35)$$

It is noted that C_s'' shown in formula (35) represents a capacity obtained by adding the above-described $C_{s'}$ and C_{gso13} to $1/2$ of the in-channel gate-source capacity C_{sh13} of the transistor Tr13 when $V_{ds}=0$, as shown in the formula (36a). In the formula (35), C_{gd13}' is a sum of the above-described C_{gd13} and $1/2$ of the in-channel gate-source capac-

ity C_{ch13} of the transistor Tr13 when $V_{ds}=0$. Specifically, C_{gd13}' is represented by the following formula (36b).

$$C_s'' = C_{s'} + C_{gso13} + C_{ch13} / 2 = C_s - C_{ch13} / 6 \quad (36a)$$

$$C_{gd13}' = C_{gd13} + C_{ch13} / 2 \quad (36b)$$

In the formula (35), $-V_1$ and V_1' are not $-V_1$ and V_1' shown in FIG. 28 and are the potential ($-V_1$) of the contact point N11 in FIG. 31A and the potential (V_1') of the contact point N11 in FIG. 31B, respectively. In the not-selected status retention step, the capacity component C_{gd13}' between the contact points N11 and N14 shown in FIG. 31B is a sum of the gate-drain capacity C_{gso13} other than the in-channel capacity of the transistor Tr13 and $1/2$ of the channel capacity C_{ch13} of the transistor Tr13. Specifically, capacity component C_{gd13}' can be represented a shown below.

$$C_{gd13}' = C_{gdo13} + C_{ch13} / 2 = C_{gd13} + C_{ch13} / 2$$

Next, the following section will describe a voltage change at each point when the not-selected status retention step shifts to the power source voltage switching step and the power source voltage switching step shifts to the light-emitting step. As shown in FIG. 32A, the drain-source potential difference of the transistor Tr13 is 0 in the not-selected status retention step to prevent the drain-source current I_{ds} from flowing. As shown in FIG. 32B, when the not-selected status retention step shifts to the power source voltage switching step, the power source voltage V_{cc} is switched from the low potential (V_{ccw}) to the high potential (V_{cce}). When the power source voltage switching step shifts to the light-emitting step, the light emission driving current I_{em} flows in the organic EL element OLED via the transistor Tr13 as shown in FIG. 32C.

First, a case will be described where the not-selected status retention step shifts to the power source voltage switching step. During the shift, the drain-source voltage of the transistor Tr13 shown in FIG. 32A is closer to the potential 0. Thereafter, the power source voltage V_{cc} in the power source voltage switching step is switched from the low potential (V_{ccw}) to the high potential (V_{cce}). Thus, the potential V_{n11} of the gate (contact point N11) of the transistor Tr13 and the potential V_{n12} of the source (contact point N12) increase. The then potential V_{n11} is represented by the formula (37a) and then potential V_{n12} are represented by the formula (37b). It is noted that V_1'' and V'' are the potential V_{n11} of the contact point N11 and the potential V_{n12} of the contact point N12 shown in FIG. 32B, respectively.

$$V_{n11} = V_1'' = \{1 + C_{ch13} \cdot (3C_s + 2C_{pix}) / 6D\} \cdot V + (C_{gd13} \cdot C_{pix} + C_{gd13} \cdot C_s) \cdot V_{cce} / D \quad (37a)$$

$$V_{n12} = V'' = C_{gd13} \cdot C_s \cdot V_{cce} / D + C_{ch13} \cdot (C_{gs11} + C_{gd13} + 3C_s) \quad (37b)$$

Furthermore, the light-emitting step switches the power source voltage. Thus, the potential V_{lc} (the potential V_{n11} of the contact point N11 in the example of FIG. 32C) caused in the gate of the transistor Tr13 (contact point N11) is represented by the following formula (38).

$$V_{n11} = V_{lc} = -V_1'' + C_s \cdot (V_{pix} - V'') / (C_{gd13} + C_{gs11} + C_s) \quad (38)$$

The respective voltages shown in the above-described formulae (34), (35), (37a), (37b), and (38) are all rewritten to voltage signs in the not-selected status switching step. Thus, the gate-source voltage V_{gs} of the driving transistor Tr13 can be represented by the following formula (39).

$$V_{gs} = V_{n11} - V_{n12} = V_{lc} - V_{oel} = (V_d - \Delta V_{gs}) + \{(C_{gs11} + C_{gd13}) / (C_s + C_{gs11} + C_{gd13})\} \times \{C_{gd13} \cdot V_{cce} / (C_{gs11} + C_{gd13}) - V_{oel} - V\} \quad (39)$$

In the formula (39), "V" is the same as that shown in formula (32b) for which $V=Vd+(Cgs11' \cdot Cs/D) \cdot Vsh1$ is established and "Vd" is a voltage caused between the gate and the source of the transistor Tr13 during the writing operation for which $(Vd+(Cgs11' \cdot Cs) \cdot Vsh1/D)$ is established as shown in the formula (32b). The voltage shift ΔVgs in the formula (39) is a potential difference between the contact point N11 and the contact point N12 when FIG. 30A is switched to FIG. 30B and is represented by $Cgs11' \cdot Cpix \cdot Vsh1/D$ as shown in the formula (34).

Next, the following section will describe, based on the above-described formula (39), an influence by the threshold voltage Vth on the gate-source voltage Vgs of the transistor Tr13 for light-emission driving. In the formula (39), values of ΔVgs , V, and D are substituted to obtain the following formula (40).

$$Vgs = \left\{ \frac{Cs}{Cs + Cgs11 + Cgd13} \right\} \cdot Vd + \left\{ \frac{Cgs11 + Cgd13}{Cs + Cgs11 + Cgd13} \right\} \cdot \left\{ \frac{Cgd13 \cdot Vcce}{Cgs11 + Cgd13} - Voel - Cgs11' \cdot Vsh1 / (Cgs11 + Cgd13) \right\} \quad (40)$$

In the formula (40), the respective capacity components $Cgs11$, $Cgs11'$, and $Cgd13$ are normalized by the capacity component Cs to provide the formula (41).

$$Vgs = \left\{ \frac{Vd - (cgs + cgd) \cdot Voel}{1 + cgs + cgd} + \left\{ \frac{cgd \cdot Vcce - cgs' \cdot Vsh1}{1 + cgs + cgd} \right\} \right\} \quad (41)$$

In the formula (41), cgs , cgs' , and cgd are the same as those shown in formula (27). In the formula (41), the first term of the right-hand side depends only on the specified gradation level based on the display data and the threshold voltage Vth of the transistor Tr13. In the formula (41), the second term of the right-hand side is a constant added to the gate-source voltage Vgs of the transistor Tr13.

Thus, in order to compensate the threshold voltage Vth by specifying a voltage, the source potential during a writing operation (potential of contact point N12) - Vd may be set so that a value $(Vgs - Vth)$ during light emission (a value determining the driving current I_{oel} during light emission) does not depend on the threshold voltage Vth . For example, when gate-source voltage $Vgs = 0 - (-Vd) = Vd$ is maintained during light emission, $(Vgs - Vth)$ can be prevented from depending on Vth by establishing the relation of $Vgs = Vd = Vd0 + Vth$. Then, the driving current I_{oel} during light emission is represented only by $Vd0$ not depending on Vth . When the gate-source voltage during light emission varies from Vgs during a writing operation, a relation of $Vd = Vd0 + \epsilon Vth$ may be used.

In the formula (41), the dependence of the organic EL element OLED on the light-emitting voltage $Voel$ in the first term of the right-hand side is determined so as to establish the relations of the following formulae (42a) to (42c). It is noted that $f(x)$, $g(x)$, and $h(x)$ in the formulae (42a) to (42c) are a function of a variable "x" in the parentheses, respectively. Specifically, the gate-source voltage Vgs of the transistor Tr13 is determined to be a function of the light-emitting voltage $Voel$ as shown in the formula (42a). The light emission driving current I_{em} is determined so as to be a function of a difference between this voltage Vgs and the threshold voltage Vth ($Vgs - Vth$) as shown in the formula (42b). The light-emitting voltage $Voel$ is also determined to be a function of the light emission driving current I_{em} as shown in formula (42c).

$$Vgs = f(Voel) \quad (42a)$$

$$I_{em} = g(Vgs - Vth) \quad (42b)$$

$$Voel = h(I_{em}) \quad (42c)$$

During the writing operation, a data voltage for giving a voltage based on display data (gradation level voltage) to the source of the driving transistor Tr13 (contact point N12) is $Vd0$. This data voltage $Vd0$ is a term that does not depend on the threshold voltage Vth as described above. The threshold voltage of the transistor Tr13 at a time Tx is $Vth(Tx)$ and the threshold voltage at a time Ty after the time Tx is $Vth(Ty)$. A voltage $Voelx$ is applied at the time Tx between the anode and the cathode of the organic EL element OLED during the light-emitting operation and a voltage $Voely$ is applied between the anode and the cathode at the time Ty .

Then, voltages satisfying a condition of $Vth(Ty) > Vth(Tx)$ and a difference between the voltages applied to the organic EL element OLED at the time Ty and the time Tx are represented by $\Delta Voel = Voely - Voelx$. In order to compensate the variation ΔVth in the threshold voltage, Vth may be compensated to cause the $\Delta Voel$ to be close to 0 as much as possible. Thus, the voltage Vd of the first term of the right-hand side in the above-described formula (41) may be set as shown in the following formula (43).

$$Vd = Vd0 + (1 + cgs + cgd) \cdot \Delta Vth \quad (43)$$

In the formula (43), when assuming that the variation ΔVth is a difference from the threshold voltage $Vth = 0V$, $\Delta Vth = Vth$ can be represented. Since $(cgs + cgd)$ is a design value, when the constant ϵ is defined as $\epsilon = 1 + cgs + cgd$, the voltage Vd shown in the formula (43) is represented by the following formula (44). Based on this formula (44), the above-described formulae (24) and (25) are introduced.

$$Vd = Vd0 + (1 + cgs + cgd) \cdot \Delta Vth = Vd0 + \epsilon \cdot \Delta Vth \quad (44)$$

The formula (44) and formula (41) can be used to provide the following formula (45) showing a voltage relation not depending on the threshold voltage Vth of the transistor Tr13. It is noted that $Voel0$ in the formula (45) is the light-emitting voltage $Voel$ of the organic EL element OLED when the threshold voltage $Vth = 0V$.

$$Vgs - Vth = \left\{ \frac{Vd0 - (cgs + cgd) \cdot Voel0}{(cgd \cdot Vcce - cgs' \cdot Vsh1) / (1 + cgs + cgd)} + \right\} \quad (45)$$

It is noted that, in the black display status as the 0th gradation level, conditions for preventing a voltage equal to or higher than the threshold voltage Vth from being applied between the gate and the source of the transistor Tr13 (i.e., voltage conditions for preventing the light emission driving current I_{em} from flowing in the organic EL element OLED) are calculated. The conditions are represented by the formula (46) when the data voltage at the time 0 is $Vd0(0)$. Thus, in the data driver 14 shown in FIG. 25, the black gradation level voltage $Vzero$ applied to an output end of the inversion calculator 148 via the changing-over switch SW4 can be determined.

$$-Vd0(0) = Vzero \geq cgd \cdot Vcce - cgs' \cdot Vsh1 \quad (46)$$

Next, in Embodiment 2, conditions for setting the compensated gradation level voltage $Vpix (= -Vin)$ so as to compensate the gate-source voltage Vgs of the driving transistor Tr13 due to parasitic capacitance will be described. By performing the processings of the respective steps shown in FIG. 11, the gate-source voltage Vgs of the driving transistor Tr13 varies due to other parasitic capacitances. In order to compensate the variation amount of this voltage Vgs , the compensated gradation level voltage $Vpix$ in the writing period $Twrt$ (a period during which the compensated gradation level voltage $Vpix$ is applied) may be set as shown in the following formula (47). It

is noted that V_{ds12} in the formula (47) is a drain-source voltage of the transistor $Tr12$.

$$V_{pix} = -(V_d + V_{ds12}) = -V_{org} - \beta V_{th} \quad (47)$$

During the writing operation shown in FIG. 34, the writing current I_{wrt} flowing between the drain and the source of the transistor $Tr13$ can be represented by the following formula (48). It is noted that μ_{FET} in the formula (48) represents a transistor mobility, C_i represents a transistor gate capacity per a unit area, $W13$ represents a channel width of the transistor $Tr13$, and $L13$ represents a channel length of the transistor $Tr13$. V_{dse13} is an effective drain-source voltage of the transistor $Tr13$ during a writing operation and V_{th13} is a threshold voltage of the transistor $Tr13$. The term “p” represents a unique parameter (fitting parameter) suitable for the characteristic of the thin film transistor.

$$I_{wrt} = \mu_{FET} \cdot C_i \cdot (V_d - V_{th13}) \cdot V_{dse13} \cdot (W13/L13) \\ = p \cdot \mu_{FET} \cdot C_i \cdot (V_d - V_{th13})^2 \cdot (W13/L13) \quad (48)$$

During a writing operation, the writing current I_{wrt} flowing between the drain and the source of the transistor $Tr12$ can be represented by the following formula (49). In the formula (49), V_{th12} is a threshold voltage of the transistor $Tr12$ and a V_{ds12} is a drain-source voltage of the transistor $Tr12$. $W12$ is a channel width of the transistor $Tr12$ and $L12$ is a channel length of the transistor $Tr12$.

$$I_{wrt} = \mu_{FET} \cdot C_i \cdot (V_{sh} + V_d + V_{ds12} - V_{th12}) \cdot (W12/L12) \cdot V_{dse12} \quad (49)$$

The drain-source voltage V_{dse12} of the transistor $Tr12$ can be represented by the following formula (50a) based on the formulae (48) and (49). In the formula (50a), V_{sat12} is an effective drain-source voltage of the transistor $Tr12$ during a writing operation and is represented by the following formula (50b). It is noted that “q” is a unique parameter (fitting parameter) suitable for the characteristic of the thin film transistor.

$$V_{dse12} = V_{ds12} / \{1 + (V_{ds12}/V_{sat12})^q\}^{1/q} \quad (50a)$$

$$V_{sat12} = p \cdot (V_{sh} + V_d + V_{ds12} - V_{th12}) \quad (50b)$$

Generally, in an n-channel amorphous silicon transistor, the longer a time during which the transistor is in an ON status (a time during which the gate-source voltage is a positive voltage) is, the larger the shift of the threshold voltage to a higher voltage is. The driving transistor $Tr13$ is ON during the light-emitting period T_{em} . This light-emitting period T_{em} occupies a large part of the cycle period T_{cyc} . Thus, the threshold voltage of the transistor $Tr13$ shifts to the positive voltage as time passes and thus the transistor $Tr13$ has higher resistance.

On the other hand, the selection transistor $Tr12$ is ON only during the selection period T_{sel} . This selection period T_{sel} occupies a small part of the cycle period T_{cyc} . Thus, when compared with the driving transistor $Tr13$, the selection transistor $Tr12$ has a smaller temporal shift. Thus, when the compensated gradation level voltage V_{pix} is introduced, the variation in the threshold voltage V_{th12} of the transistor $Tr12$ can be ignored with regards to the variation in the threshold voltage V_{th13} of the transistor $Tr13$.

As shown in the above-described formulae (48) and (49), the writing current I_{wrt} is determined based on a Thin Film Transistor (TFT) characteristic fitting parameter (e.g., p, q), a parameter determined by a transistor size, a process parameter (e.g., transistor gate thickness, amorphous silicon mobility), and a set value owned by the selection signal (e.g., voltage V_{sh}). Thus, an equation when I_{wrt} shown in formula (48) is equal to I_{wrt} shown in formula (49) is subjected to an numeric analysis to calculate the drain-source voltage V_{ds12}

of the transistor $Tr12$. This voltage V_{ds12} has a relation shown in the formula (47) ($V_{pix} = -V_d - V_{ds12}$) with the compensated gradation level voltage V_{pix} . Thus, V_{ds12} can be determined to calculate the compensated gradation level voltage V_{pix} .

When the inversion calculator 148 outputs this compensated gradation level voltage V_{pix} during the writing period T_{wrt} , $-V_d$ is written to the source of the transistor $Tr13$ (contact point $N12$). Thus, the transistor $Tr13$ during the writing period T_{wrt} has a gate-source voltage of V_{gs} to establish the drain-source voltage $V_{ds} = 0 - (-V_d) = V_d + \epsilon \cdot \Delta V_{th}$. By flowing the writing current I_{wrt} as described above, the driving current I_{oled} for which the shift of the threshold voltage V_{th} due to an influence by parasitic capacitance for example is compensated can be flowed in the organic EL element OLED during the writing period T_{wrt} .

Next, the following section will describe the display apparatus 1 according to Embodiment 2 and an effect by the driving method of the display apparatus 1 with reference to a specific test result. The potential ($-V_d$) at the source (contact point $N12$) of the driving transistor $Tr13$ during a writing operation is set based on the data voltage V_{d0} and a multiple of the threshold voltage V_{th} by a fixed number (multiple of γ) as shown in the formula (24) ($-V_d = -V_{d0} - \gamma V_{th}$). This potential is set based on the voltage V_{gs} retained between the gate and the source. On the other hand, the compensated gradation level voltage $V_{pix} (= -V_{in})$ generated by the data driver 14 (inversion calculator 148) is set based on the original gradation level voltage V_{org} and a multiple of the threshold voltage V_{th} by a fixed number (multiple of β) ($-V_{in} = -V_{org} - \beta V_{th}$) as shown in the formula (22).

The following section will examine conditions required for the relation between the data voltage V_{d0} and the original gradation level voltage V_{org} to not to depend on the constants γ or β and the threshold voltage V_{th} . As shown in FIG. 34, during the writing operation, the higher input data (specified gradation level) of the original gradation level voltage V_{org} is, the wider a difference between the data voltage V_{d0} for giving a voltage depending on display data (gradation level voltage) to the source of the driving transistor $Tr13$ and the original gradation level voltage V_{org} ($V_{d0} - V_{org}$) is. For example, in the 0th gradation level (black display status), the data voltage V_{d0} and the original gradation level voltage V_{org} are both $V_{zero} (= 0V)$. On the other hand, at the 255th gradation level (the highest gradation level), a difference between the data voltage V_{d0} and the original gradation level voltage V_{org} ($V_{d0} - V_{org}$) is about 1.3V. This is due to a fact that, the higher the applied compensated gradation level voltage V_{pix} is, the higher the writing current I_{wrt} is and a transistor $Tr13$ also has a higher source drain voltage.

It is noted that the example of FIG. 34 shows the power source voltage $V_{cc} (= V_{ccw})$ during the writing operation of the ground potential $GND (= 0V)$ and the power source voltage $V_{cc} (= V_{cce})$ during the light-emitting operation of 12V. A potential difference (voltage range) V_{sh1} between the high level (V_{sh}) and the low level ($-V_{sl}$) of the selection signal S_{sel} is 27V. The transistor $Tr13$ for light emission driving has the channel width $W13$ of 100 μm and the transistor $Tr11$ and transistor $Tr12$ have the channel widths $W11$ and $W12$ of 40 μm . The display pixel PIX has a size of 129 $\mu m \times 129 \mu m$, the pixel has an aperture ratio of 60%, and the capacitor C_s has capacitance of 600 fF (= 0.6 pF).

The following section will describe a relation between the compensated gradation level voltage to input data and the threshold voltage during a writing operation. As shown in the formula (22), the compensated gradation level voltage $V_{pix} (= -V_{in})$ depends on the constant β and the threshold voltage

V_{th} . When assuming that this constant β is fixed, the higher the threshold voltage V_{th} is, the lower the compensated gradation level voltage V_{pix} by this threshold voltage V_{th} as shown in FIG. 35. This tendency is found in substantially all gradation level zones of the input data (specified gradation level).

In the example of FIG. 35, when the constant $\beta=1.08$ is set and the threshold voltage V_{th} is changed in an order of 0V, 1V, and 3V, the characteristic line of the compensated gradation level voltage V_{pix} to the respective threshold voltages V_{th} substantially translates in the low voltage direction. At the 0th gradation level (black display status), the compensated gradation level voltage V_{pix} is $V_{zero}(=0V)$ regardless of the value of the threshold voltage V_{th} . It is noted that test conditions of FIG. 35 are the same as those shown in FIG. 34.

Next, the following section will describe a relation between the light emission driving current I_{em} of the organic EL element OLED and the threshold voltage V_{th} with regards to input data in a light-emitting operation. It is noted that input data has 256 gradation levels among which the lowest gradation level are the 0th gradation level and the highest gradation level are the 255th gradation level. The compensated gradation level voltage V_{pix} shown in the formula (22) is applied from the data driver 14 to the respective display pixels PIX. As a result, the writing voltage $V_{gs}(=0-(-V_d)=V_{d0}+\gamma V_{th})$ shown in formula (24) is applied between the gate and the source of the driving transistor Tr13. When the constant γ is substantially fixed, the light emission driving current I_{em} having a substantially fixed current value flowed in the organic EL element OLED regardless of the value of the threshold voltage V_{th} as shown in FIG. 36A and FIG. 36B. This tendency is found in substantially all gradation level zones of input data (specified gradation level). It is noted that test conditions of FIG. 36A and FIG. 36B are the same as those shown in FIG. 34.

The example of FIG. 36A shows a test result when the constant $\gamma=1.07$ and the threshold voltage $V_{th}=1.0V$. The example of FIG. 36B shows a test result when the constant $\gamma=1.05$ and the threshold voltage $V_{th}=3.0V$ are set. When FIG. 36A is compared with FIG. 36B, the light emission driving current I_{em} shows substantially the same characteristic line regardless of different values of the threshold voltages V_{th} .

This test result also showed that a brightness change (difference in brightness) to theoretical value is suppressed to 1.3% or less in substantially all gradation levels (hereinafter this suppression effect is called as “ γ effect”). When $\gamma=1.07$ was established as shown in FIG. 36A for example and when the respective specified gradation levels (8 bit) were 63, 127, and 255, the respective brightness changes were 0.27%, 0.62%, and 1.29%. When $\gamma=1.05$ was established as shown in FIG. 36B and when the respective specified gradation levels (8 bit) were 63, 127, and 255, the respective brightness changes were 0.27%, 0.61%, and 1.27%.

Next, the following section will describe a relation between light emission driving current to input data and variation in the threshold voltage (shift) in a light-emitting operation. It was found that, with regards to the dependency of “ γ effect” on the variation amount of the threshold voltage V_{th} (V_{th} shift width), when the constant γ was assumed as constant, the higher variation width the threshold voltage V_{th} has, the smaller difference in current to the light emission driving current I_{em} in the initial threshold voltage V_{th} .

As shown in FIG. 37A and FIG. 37B, when $\gamma=1.1$ and V_{th} was changed from 1V to 3V (V_{th} shift width was 2V) and when the respective specified gradation levels (8 bit) were 63, 127, and 255, the respective brightness changes were 0.24%,

0.59%, and 1.29%. As shown in FIG. 37A and FIG. 37C, when $\gamma=1.1$ and V_{th} was changed from 1V to 5V (V_{th} shift width was 4V) and when the specified gradation levels (8 bit) were 63, 127, and 255, the respective brightness changes were 0.04%, 0.12%, and 0.27%.

By the above result, it was found that, the higher variation amount (V_{th} shift width) the threshold voltage V_{th} has, the characteristic line is closer to theoretical value. Specifically, it was found that a brightness change (difference in brightness) to theoretical value could be reduced (or suppressed to about 0.3% or less).

It is noted that, in order to show the advantage of the effect by this embodiment, the above-described a test result having the “ γ effect” will be compared with a test result not having the “ γ effect”. The test result not having the “ γ effect” is obtained by driving applying such a voltage V_{th} between the gate and the source of the transistor Tr13 that does not depend on the constant γ in the relation shown in the formula (24) ($V_{gs}=0-(-V_d)=V_{d0}+\gamma V_{th}$). As shown in FIGS. 38A and 39B, in the case of the test result not having the “ γ effect”, a relation between input data and the light emission driving current and the threshold voltage showed a characteristic line according to which, regardless of the constant γ , the higher threshold voltage V_{th} the transistor Tr13 had, the light emission driving current I_{em} was smaller. It is noted that the example of FIG. 38A shows the characteristic line of the light emission driving current I_{em} when the constant $\gamma=1.07$ is set and the threshold voltage $V_{th}=1.0V$ and 3.0V is set. The example of FIG. 38B shows the characteristic line of the light emission driving current I_{em} when the constant $\gamma=1.05$ is set and the threshold voltage $V_{th}=1.0V$ and 3.0V is set.

It was found that, in substantially all gradation level zones, a brightness change to theoretical value (difference in brightness) was 1.0% or more and a brightness change to theoretical value was 2% or more in an intermediate gradation level (the 127th gradation level in the examples of FIGS. 38A and 39B) in particular. When $\gamma=1.07$ and when the respective specified gradation levels (8 bit) were 63, 127, and 255, the respective brightness changes were 1.93%, 2.87%, and 4.13%. When $\gamma=1.05$ and when the respective specified gradation levels (8 bit) were 63, 127, and 255, the respective brightness changes were 1.46%, 2.09%, and 2.89%.

When this brightness change reaches about 2% in the intermediate gradation level, a user recognizes the change as a printed image. Thus, when a voltage V_{gs} not depending on the constant γ (writing voltage; $-V_d=-V_{d0}-V_{th}$) is retained in the capacitor C_s , the displayed picture has a deteriorated quality. On the other hand, according to Embodiment 2, a voltage retained in the capacitor C_s is a writing voltage for which the constant γ is compensated ($=0-(-V_d)=V_{d0}+\gamma V_{th}$). Thus, as shown in FIG. 36 and FIG. 37, a brightness change to theoretical value (difference in brightness) at the respective gradation levels can be significantly suppressed. Thus, the display apparatus 1 of Embodiment 2 can prevent an image from being printed to display the image with preferred display picture quality.

Next, the following section will describe a relation between the compensated gradation level voltage V_{pix} and the gate-source voltage V_{gs} of the transistor Tr13. The source of the transistor Tr13 (contact point N12) and the data line Ld have therebetween a potential difference due to resistance when the transistor Tr12 is ON. Thus, the contact point N12 retains a voltage obtained by adding the data voltage V_{d0} to a voltage obtained by multiplying the threshold voltage V_{th} of the transistor Tr13 with γ . By the retention of this voltage, such a voltage is retained as the compensated gradation level voltage V_{pix} at the contact point N12 that is obtained by

adding the original gradation level voltage V_{org} to a voltage β times higher than the threshold voltage V_{th} , as shown in the formula (22).

The following section will examine, in the relation between the compensated gradation level voltage V_{pix} and the gate-source voltage V_{gs} of the transistor $Tr13$ shown in the formulae (22) and (24), a change γV_{th} of $V_{gs}(=V_d)$ when βV_{th} is OFFSET to $V_{pix}(=V_{in})$.

As shown in FIG. 39, when the threshold voltage V_{th} changes from 0V to 3V, the constant β determining the compensated gradation level voltage V_{pix} is fixed to the input data (specified gradation level). On the other hand, the constant γ determining the gate-source voltage V_{gs} of the transistor $Tr13$ changes to have a substantially fixed slope with regards to the input data (specified gradation level). In the example of FIG. 39, $\gamma=1.097$ may be set for $\beta=1.08$ in the intermediate gradation level (which is in the vicinity of the 128th gradation level when the number of gradation levels are 256) so that the constant γ has an ideal value (which is shown by a chain line in FIG. 39). Since the constant β and the constant γ can be set to relatively close values, $\beta=\gamma$ may be set for a practical use.

In consideration of the above test results, a constant $\gamma(=\beta)$ for determining the gate-source voltage V_{gs} of the driving transistor $Tr13$ is desirably 1.05 or more. It was found that the compensated gradation level voltage V_{pix} may be set so that the voltage V_d retained in the source (contact point $N12$) of the transistor $Tr13$ in at least one gradation level of input data (specified gradation level) is the voltage $(-V_{d0}-\gamma V_{th})$ shown in the formula (24).

Furthermore, the dimension of the transistor $Tr13$ (a ratio W/L between the channel width W and the channel length L) and the voltage of the selection signal S_{sel} (V_{sh} and $-V_{sl}$) are desirably set so that a change in the light emission driving current I_{em} in accordance with variation in the threshold voltage (V_{th} shift) is within about 2% of the maximum current value in an initial status.

The compensated gradation level voltage V_{pix} is a value obtained by adding the drain-source voltage of the transistor $Tr12$ to the source potential $(-V_d)$ of the transistor $Tr13$. The larger absolute value of the difference between the power source voltage V_{ccw} and the compensated gradation level voltage V_{pix} ($V_{ccw}-V_{pix}$) is, the higher value the current flowing between the drain and the source of each of the transistors $Tr12$ and $Tr13$ during the writing operation has. This causes an increased potential difference between the compensated gradation level voltage V_{pix} and the source potential $(-V_d)$ of the transistor $Tr13$.

However, when an influence on the voltage drop by the drain-source voltage of the transistor $Tr12$ is reduced, an effect P times higher than the threshold voltage V_{th} directly appears in the "γ effect". Specifically, if the OFFSET voltage γV_{th} that can satisfy the relation of the formula (24) can be set, variation in the value of the light emission driving current I_{em} when the writing operation status shifts to the light-emitting operation status can be compensated. In this case, an influence by the drain-source voltage of the transistor $Tr12$ must be considered.

As shown in FIG. 34, the transistor $Tr12$ is designed so that the drain-source voltage of the transistor $Tr12$ is about 13V at the maximum gradation level (the maximum drain-source voltage) in the writing operation. In this case, as shown in FIG. 39, a difference between a constant $\gamma(=1.07)$ at the lowest gradation level (the 0th gradation level) and a constant $\gamma(=-1.11)$ at the highest gradation level (the 255th gradation level) is sufficiently small. Thus, the difference can be approximated to β shown in the formula (22).

The voltage V_{d0} of the gate-source voltage V_{gs} of the transistor $Tr13$ of a difference between the power source voltage V_{ccw} and the compensated gradation level voltage V_{pix} ($V_{ccw}-V_{pix}$) is the original gradation level voltage V_{org} . The compensated gradation level voltage V_{pix} is set to a voltage obtained by adding the OFFSET voltage βV_{th} to the original gradation level voltage V_{org} to have a negative polarity. During the writing operation, this compensated gradation level voltage V_{pix} is set to satisfy the formula (22). In this case, the maximum voltage between the drain and the source of the transistor $Tr12$ can be appropriately set to approximate the constant γ to the constant β . As a result, the respective gradation levels can be accurately displayed in a range from the lowest gradation level to the highest gradation level.

The following section will describe the characteristic of the change of the pixel current to the driving voltage of the organic EL element OLED (having a pixel size of $129\mu m \times 129\mu m$ and an aperture ratio of 60%) used for the test. As shown in FIG. 40, the pixel current of this organic EL element OLED has a small current value on the order of $10 \times 10^{-3} \mu A$ to $10 \times 10^{-5} \mu A$ in a zone in which the driving voltage is a negative voltage. The pixel current also showed the lowest value when the driving voltage is about 0V and sharply increases with an increase of the driving voltage in a zone in which the driving voltage is a positive voltage.

The following section will describe a relation between the in-channel parasitic capacitance of a transistor applied to the display pixel PIX and the voltage. First, based on a Meyer capacity model generally referred to with regards to the parasitic capacitance of the thin film transistor TFT, a relation between the capacity and the voltage (capacity characteristic) is shown under conditions under which the gate-source voltage V_{gs} is higher than the threshold voltage V_{th} ($V_{gs} > V_{th}$) (i.e., conditions under which a channel is formed between the source and the drain).

The in-channel parasitic capacitance C_{ch} of the thin film transistor is classified to a gate-source parasitic capacitance C_{gs_ch} and a gate-drain parasitic capacitance C_{gd_ch} . A capacity ratio between the respective parasitic capacitances C_{gs_ch} and C_{gd_ch} and the in-channel parasitic capacitance C_{ch} (C_{gs_ch}/C_{ch} , C_{gd_ch}/C_{ch}) has a predetermined characteristic with regards to a difference between the gate-source voltage V_{gs} and the threshold voltage V_{th} ($V_{gs}-V_{th}$).

As shown in FIG. 41, when the voltage ratio is 0 (the drain-source voltage $V_{ds}=0V$), the capacity ratio C_{gs_ch}/C_{ch} is equal to the capacity ratio C_{gd_ch}/C_{ch} and both of the capacity ratios are $1/2$. When the voltage ratio increases and the drain-source voltage V_{ds} reaches the saturated zone, the capacity ratio C_{gs_ch}/C_{ch} is about $2/3$ and the capacity ratio C_{gd_ch}/C_{ch} is asymptotic to 0.

As described above, according to Embodiment 2, the display apparatus 1 applies the compensated gradation level voltage V_{pix} having the voltage value shown in the formula (50a) at the writing operation of the display pixel PIX . Thus, the voltage V_{gs} can be retained between the gate and the source of the transistor $Tr13$. It is noted that this voltage V_{gs} corresponds to display data (gradation level values) and is set to compensate an influence by a voltage change in the pixel driving circuit DC. Thus, the current value of the light emission driving current I_{em} supplied to the organic EL element OLED during a light-emitting operation can be compensated.

Specifically, the light emission driving current I_{em} having the current value corresponding to the display data is flowed in the organic EL element OLED. Thus, the organic EL element can be caused to emit light with brightness depending on display data. This can suppress the dislocation of the gradation level in the respective display pixels to provide a display

apparatus having a superior display quality. It is noted that Embodiment 2 also can appropriately use a method for driving a display apparatus that is substantially the same as that of Embodiment 1.

Various embodiments and changes may be made thereunto without departing from the broad spirit and scope of the invention. The above-described embodiments are intended to illustrate the present invention, not to limit the scope of the present invention. The scope of the present invention is shown by the attached claims rather than the embodiments.

Various modifications made within the meaning of an equivalent of the claims of the invention and within the claims are to be regarded to be in the scope of the present invention.

What is claimed is:

1. A display apparatus, comprising:

a light-emitting element for emitting light with a gradation level depending on supplied current;

a pixel driving circuit for supplying the current to the light-emitting element depending on a voltage applied via a data line;

a precharge voltage source for applying a predetermined precharge voltage to the pixel driving circuit via the data line;

a voltage reader for reading, after the application of the precharge voltage by the precharge voltage source, the voltage of the data line only one time after a predetermined transient response period; and

a compensated gradation data signal generator for generating, based on the read voltage of the data line, a compensated gradation data signal having a voltage value corresponding to an element characteristic unique to the pixel driving circuit to apply the compensated gradation data signal to the pixel driving circuit.

2. The display apparatus according to claim 1, wherein: the display apparatus includes an original gradation level voltage generator for generating an original gradation level voltage having a voltage value not depending on the element characteristic unique to the pixel driving circuit, and

the original gradation level voltage is for causing the light-emitting element to emit light with a desired brightness corresponding to the gradation level.

3. The display apparatus according to claim 2, wherein: the compensated gradation data signal generator generates the compensated gradation data signal based on the original gradation level voltage, a first compensation voltage generated based on the voltage of the data line, and a second compensation voltage determined based on the element characteristic unique to the pixel driving circuit.

4. The display apparatus according to claim 3, wherein: the compensated gradation data signal generator comprises a calculation circuit for calculating the original gradation level voltage, the first compensation voltage, and the second compensation voltage to generate the compensated gradation data signal.

5. The display apparatus according to claim 1, wherein: the display apparatus includes a black gradation level voltage source for applying, to the pixel driving circuit, a black gradation level voltage for causing the light-emitting element to perform a black display, and a switch for connecting the black gradation level voltage source to the data line at a predetermined timing.

6. The display apparatus according to claim 1, wherein: the display apparatus includes a connection path switching switch for connecting the data line to the voltage reader,

the compensated gradation data signal generator, and the precharge voltage source respectively with a predetermined timing.

7. The display apparatus according to claim 6, wherein: the voltage reader is structured to read, after the precharge voltage is applied to the pixel driving circuit and the connection path switching switch is switched to block application of the precharge voltage by the precharge voltage source to the data line, the voltage of the data line after the transient response period, and the transient response period is shorter than a time required for the voltage of the data line to converge to a converge voltage value unique to the pixel driving circuit.

8. The display apparatus according to claim 7, wherein: the precharge voltage source applies, when the connection switching switch is used to connect the precharge voltage source to the data line, the precharge voltage, and the precharge voltage has a voltage value having a higher absolute value than an absolute value of the converge voltage value unique to the pixel driving circuit.

9. The display apparatus according to claim 6, wherein: the display apparatus further includes a controller for performing, within a predetermined period: (i) using the connection path switching switch to connect the precharge voltage source to the data line to apply the precharge voltage to the pixel driving circuit, (ii) using the connection path switching switch to connect the voltage reader to the data line to read the voltage of the data line corresponding to the element characteristic unique to the pixel driving circuit after the transient response period, and (iii) using the connection path switching switch to connect the compensated gradation data signal generator to the data line to apply the compensated gradation data signal to the pixel driving circuit.

10. The display apparatus according to claim 1, wherein the display apparatus includes: a selection driver for applying a selection signal to the pixel driving circuit via a selection line to cause the pixel driving circuit to be in a selected state, and a display panel in which a plurality of display pixels are arranged in a matrix manner, each of the plurality of display pixels including a pair of one said light-emitting element and one said pixel driving circuit, and

wherein:

the plurality of display pixels are arranged in a row direction and a column direction,

the data line is connected to the pixel driving circuits of a plurality of the display pixels arranged in the column direction, and

the selection line is connected to the pixel driving circuits of a plurality of the display pixels arranged in the row direction.

11. The display apparatus according to claim 1, wherein: the pixel driving circuit includes a driving transistor serially connected to the light-emitting element, and a variation amount of the element characteristic unique to the pixel driving circuit is a variation amount of a threshold voltage of the driving transistor.

12. The display apparatus according to claim 1, wherein the pixel driving circuit includes:

a driving transistor serially connected to the light-emitting element;

a selection transistor connected between the driving transistor and the data line; and

a diode connection transistor for causing the driving transistor to be in a diode-connected state.

13. The display apparatus according to claim 12, wherein the pixel driving circuit is structured such that:

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a first end of a current path of the driving transistor is connected with a power source voltage for which a potential is switched with a predetermined timing and a second end of the current path of the driving transistor is connected with a first end of the light-emitting element, 5

a first end of a current path of the selection transistor is connected with the second end of the current path of the driving transistor and a second end of the current path of the selection transistor is connected with the data line, 10

a first end of a current path of the diode connection transistor is connected with the power source voltage and a second end of the current path of the diode connection transistor is connected with a control terminal of the driving transistor, 15

control terminals of the selection transistor and the diode connection transistor are connected to the selection line, and 20

a second end of the light-emitting element is connected to a fixed reference voltage.

14. The display apparatus according to claim 11, wherein: 20

a voltage between a control terminal of the driving transistor and one terminal of a current path of the driving transistor is determined based on a sum of a first voltage component that does not depend on the element characteristic unique to the pixel driving circuit for causing the light-emitting element to emit light with desired brightness corresponding the gradation level and a second voltage component that at least 1.05 times the threshold voltage of the driving transistor. 25

15. The display apparatus according to claim 11, wherein: 30

a voltage retained between a control terminal of the driving transistor and one terminal of a current path of the driving transistor by the compensated gradation data signal that specifies a compensated gradation level is determined by a sum of a first voltage component that does not depend on the element characteristic unique to the pixel driving circuit for causing the light-emitting element to emit light with a desired brightness corresponding to the gradation level and a second voltage component that is higher than the threshold voltage of the driving transistor by a predetermined multiple. 35

16. The display apparatus according to claim 1, wherein the display apparatus includes: a selection driver for applying a selection signal to the pixel driving circuit via a selection line to cause the pixel driving circuit to be in a selected state, and 45

a display panel in which a plurality of display pixels are arranged in a matrix manner, each of the plurality of display pixels including a pair of one said light-emitting element and one said pixel driving circuit, 50

wherein the plurality of display pixels are arranged in a row direction and a column direction, the data line is connected to the pixel driving circuits of a plurality of the display pixels arranged in the column direction, and the selection line is connected to the pixel driving circuits of a plurality of the display pixels arranged in the row direction, 55

wherein the pixel driving circuit includes a driving transistor serially connected to the light-emitting element, a selection transistor connected between the driving transistor and the data line, and a diode connection transistor for causing the driving transistor to be in a diode-connected state, and a variation amount of the element characteristic unique to the pixel driving circuit is a variation amount of a threshold voltage of the driving transistor, and 60

wherein a driving current flowing in the light-emitting element via a current path of the driving transistor by the 65

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compensated gradation data signal and based on a voltage between a control terminal of the driving transistor and one terminal of the current path of the driving transistor is associated with an element size of the selection transistor and a voltage of the selection signal so that all gradation levels for causing the light-emitting element to emit light can cause a variation amount of a current value due to variation in the threshold voltage of the driving transistor that is within 2% of a maximum current value in an initial state under which the driving transistor has no variation in the threshold voltage.

17. The display apparatus according to claim 1, wherein: the compensated gradation data signal generator generates, based on the read voltage of the data line and a voltage retained in the pixel driving circuit, the compensated gradation data signal having the voltage value corresponding to the element characteristic unique to the pixel driving circuit to apply the compensated gradation data signal to the pixel driving circuit.

18. A display apparatus, comprising: 18

a light-emitting element for emitting light with a gradation level depending on supplied current;

a pixel driving circuit for supplying the current to the light-emitting element depending on a voltage applied via a data line;

a precharge voltage source for applying a predetermined precharge voltage to the pixel driving circuit via the data line;

a voltage reader for reading, after the application of the precharge voltage by the precharge voltage source, the voltage of the data line only one time after a predetermined transient response period; and

a compensated gradation data signal generator for generating, based on the read voltage of the data line and a voltage retained in the pixel driving circuit, a compensated gradation data signal having a voltage value corresponding to a voltage characteristic unique to the pixel driving circuit to apply the compensated gradation data signal to the pixel driving circuit.

19. The display apparatus according to claim 18, wherein: the display apparatus includes an original gradation level voltage generator for generating an original gradation level voltage having a voltage value not depending on the voltage characteristic unique to the pixel driving circuit, and 19

the original gradation level voltage is for causing the light-emitting element to emit light with a desired brightness corresponding to the gradation level.

20. The display apparatus according to claim 19, wherein: the compensated gradation data signal generator generates the compensated gradation data signal based on the original gradation level voltage and a compensation voltage generated based on the voltage of the data line and the voltage characteristic unique to the pixel driving circuit.

21. The display apparatus according to claim 20, wherein: the compensated gradation data signal generator comprises a calculation circuit for calculating the original gradation level voltage and the compensation voltage to generate the compensated gradation data signal.

22. The display apparatus according to claim 18, wherein: the pixel driving circuit includes a driving transistor serially connected to the light-emitting element, and 22

the voltage characteristic unique to the pixel driving circuit is based on a change in a voltage between a control terminal of the driving transistor and one terminal of a current path of the driving transistor.

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23. A method for driving a display apparatus, comprising:
 applying a predetermined precharge voltage to a pixel driving circuit via a data line;
 reading, after the application of the precharge voltage, the voltage of the data line only one time after a predetermined transient response period which is shorter than a time during which the voltage of the data line converges to a converge voltage value unique to the pixel driving circuit;
 generating, based on one of: (i) the read voltage of the data line and (ii) the read voltage of the data line and a voltage retained in the pixel driving circuit, a compensated gradation data signal having a voltage value corresponding to an element characteristic unique to the pixel driving circuit;
 applying the generated compensated gradation data signal to the pixel driving circuit; and
 supplying current depending on a voltage applied via the data line from the pixel driving circuit to a light-emitting element.

24. A display driving apparatus, comprising:
 a precharge voltage source for applying, via a data line, a predetermined precharge voltage to a pixel driving circuit connected to a light-emitting element;
 a voltage reader for reading, after the application of the precharge voltage by the precharge voltage source, the

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voltage of the data line only one time after a predetermined transient response period; and
 a compensated gradation data signal generator for applying, based on one of: (i) the read voltage of the data line and (ii) the read voltage of the data line and a voltage retained in the pixel driving circuit, a compensated gradation data signal having a voltage value corresponding to an element characteristic unique to the pixel driving circuit to apply the compensated gradation data signal to the pixel driving circuit.

25. A method for driving a display driving apparatus, comprising:
 applying a predetermined precharge voltage to a pixel driving circuit via a data line;
 reading, after the application of the precharge voltage, the voltage of the data line only one time after a predetermined transient response period;
 generating, based on one of: (i) the read voltage of the data line and (ii) the read voltage of the data line and a voltage retained in the pixel driving circuit, a compensated gradation data signal having a voltage value corresponding to an element characteristic unique to the pixel driving circuit; and
 applying the generated compensated gradation data signal to the pixel driving circuit.

* * * * *

专利名称(译)	用于驱动显示驱动装置的显示驱动装置和方法，以及用于驱动显示装置的显示装置和方法		
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摘要(译)

根据显示数据，使发光元件（OLED）以优选的亮度和灰度等级发光。在预充电时段期间，数据驱动器经由数据线（Ld）将预充电电压（Vpre）施加到电容器（Cs）。在施加预充电电压之后，电压转换器在瞬态响应时段（Ttrs）之后读取参考电压Vref以产生补偿电压（a·Vref）。电压计算器基于补偿电压（a·Vref）补偿具有根据由灰度级电压发生器产生的显示数据的值的原始灰度级电压Vorg。结果，电压计算器产生补偿灰度级电压Vpix，其对应于用于驱动发光的晶体管Tr13的元件特性的变化量，以将补偿的灰度级电压Vpix施加到数据线Ld。

